Special Report:
DSP coprocessor boards share the workload with CPUs  pg 108
HMIs Performance Analysis Card (PAC) provides real-time software performance analysis and real-time software test coverage for all HMI-200 series in-circuit emulators. This option operates completely transparent to the system under test and collects its data in real-time to establish a true profile of the software execution.

Features:
- Hardware implemented
- Up to eight modules can be defined
- Histograms for each module are displayed
- Minimum, Maximum and Average time duration for each module displayed
- Coverage mode displays which pieces of the code did and did not execute
- Trace data has a time stamp

Benefits:
- More efficient code produces higher performance products for your company
- Better tested code eliminates bugs generated from untested code and creates higher quality software for your company
- The Emulator and Performance Analysis together shorten the design cycle time allowing your company to have its window of opportunity in the marketplace

Available Emulators:
- 68000
- 68030
- 68340
- 68HC11 Family
- 8085
- 68008
- 68302
- 6809/6809E
- includes DI & F3
- 64180/Z180
- 68010
- 68331
- 68HC001
- D85000
- Z80
- 68020
- 68352
- 8051 Family
- 8096/80196 Family
- CIRCLE NO. 201
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SPECIFICATIONS

<table>
<thead>
<tr>
<th>Frequency (MHz)</th>
<th>Insertion loss, typ (dB)</th>
<th>Isolation, typ (dB)</th>
<th>1 dB compression, typ (dBm @ in port)</th>
<th>RF input, max dBm (no damage)</th>
<th>VSWR (on), typ</th>
<th>Video breakthrough to RF, typ (mV p-p)</th>
<th>Switching speed, typ (nsec)</th>
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<tbody>
<tr>
<td></td>
<td>Reflective</td>
<td>Absorptive</td>
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<tr>
<td>50</td>
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</table>

RF input, max dBm (no damage): 20 dBm (port), 24 dBm (total)

Price (1-9 qty): YSW-2-50DR (pin) $19.95, YSWA-2-50DR (pin) $23.95, YSW-500R (connector) $39.95, YSWA-500R (connector) $69.95.

Mini-Circuits
P.O. Box 350166, Brooklyn, New York 11235-0003 (718) 934-4500 Fax (718) 332-4661 Telexes: 6852844 or 620156

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Tougher SBL-mixers, spanning 25KHz to 2000MHz, with +7dBm, +10dBm, and +13dBm LO models, priced from $4.50 (10 qty) are available only from Mini-Circuits. Don’t settle for a substitute or equivalent… insist on Ultra-Rel™ SBLs.

<table>
<thead>
<tr>
<th>Model</th>
<th>Frequency (MHz)</th>
<th>Conv. Loss (dB)</th>
<th>Isolation (dB)</th>
<th>LO Level (dBm)</th>
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<tr>
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<td>40</td>
<td>+13</td>
<td>11.70</td>
</tr>
</tbody>
</table>

*ULTRA-REL™ MIXERS 5 yr. Warranty*

with extra long life due to unique HP monolithic diode construction, 300°C high temp. storage, 1000 cycles thermal shock, vibration, acceleration, and mechanical shock exceeding MIL requirements.
SPECIAL REPORTS

DSP coprocessor boards 108

The technology in these number crunchers is developing so fast that about the only things moving faster are the instructions and data they handle. Besides faster µPs, architectural innovations—especially parallel and pipelined processors—are adding to the boards' speed. But as is so often the case, software is struggling to keep pace.—Dan Strassberg, Associate Editor

Windows-based engineering software 130

The PC is the most popular computer for engineering development work, but lack of graphics-display and printing standards has blocked developing appropriate workstation-class engineering software. Windows 3.0 opens the flood gates.

—Steven H Leibson, Executive Editor

DESIGN FEATURES

Techniques let you write general-purpose Spice models 149

By incorporating flexibility into your Spice models, you'll develop a library of accurate models that you can adapt for many applications, rather than reinventing the wheel every time. An example of such a model is a universal power converter.—David Caldwell, Consultant

Phase compensation extends op amp stability and speed 181

Because most op amps lack provision for altering internal phase compensation, circuit designers often add external compensation to counter the effects of capacitance loading and parasitic capacitance and inductance.—Jerald Graeme, Burr-Brown Corp

Continued on page 7
Our Westcor division’s family of configurable AC or DC input fan cooled StakPAC switchers reveals a new world of power density and output flexibility to the system designer...whatever your power needs. Each StakPAC is built with field proven robotically manufactured Vicor VI-200 Series power components providing you the flexibility of a customized supply combined with the off-the-shelf availability of standard catalog products...“first article” StakPACs are typically delivered in 2 weeks.

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Component Solutions For Your Power System
TECHNOLOGY UPDATES

European EMC regulations: Europe lays down EMC Law 57

A law regulating the electromagnetic compatibility of many products takes effect in Europe on January 1, 1992. Deciding how to make the products conform will be up to the design engineer.
—Brian Kerridge, European Editor

High-density PLD architectures: Family tree sorts out high-density PLDs 75

Bringing order to the welter of high-density programmable logic devices is no easy task. After conferring with experts, EDN bravely offers this hopefully comprehensive and extensible overview.—Charles H Small, Senior Editor

EDITORS’ CHOICES

CMOS monolithic 5-tap, delay-line IC 93
Surface-micromachined acceleration sensor 95

PRODUCT UPDATE

Low-power, 1.8-in. hard-disk drive 99

NEW PRODUCTS

Integrated Circuits ........................................ 215
CAE & Software Development Tools ................. 223
Test & Measurement Instruments .................. 233
Computers & Peripherals ................................. 247
Components & Power Supplies ......................... 251

DEPARTMENTS

News Breaks .................................................. 17
Signals & Noise .............................................. 29
Ask EDN ....................................................... 39
Calendar ....................................................... 40
Editorial ....................................................... 49
Design Ideas .................................................. 199
Literature ...................................................... 257
Professional Issues ......................................... 261
Career Opportunities .................................... 273
Business/Corporate Staff ................................. 278
EDN’s International Advertisers Index ............... 280
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There used to be only limited choices. For $60,000 or so, you could get overpriced EDA software and a single PCB design environment. It also came with free, virtually endless levels of frustration, because these systems are hard to use and even more difficult to learn. Which made productivity look something like an inverted bell curve.

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EDN September 16, 1991
Some might call it sleeping on the job. We call it true static operation—and that’s how the low power Am386 microprocessors use a full 35% less power than the other so-called low power 386 at any sustained clock speed.

They’re not only the most efficient 386s on the planet, they’re also the fastest. Our Am386SXL-25 CPU clocks in at 25MHz.

25% faster than the i386SX-20, while our Am386DXL-40 CPU boasts a 40MHz clock speed.

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Cost crossover today makes 4-meg DRAMs more economical per bit than 1-meg DRAMs. And given all the benefits in reliability and board real estate, that's good news.

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All the modules listed here have reliability specs based on 600 temperature cycles (0-125°C) and 500 hours (85°C, 85% RH). Available features include 70, 80, and 100 ns access
times, fast page mode, low-power versions, gold lead finish, and customer-specific labeling.

**SAMSUNG MEMORY MODULES BASED ON 4-MEG DRAMs**

<table>
<thead>
<tr>
<th>Megabytes</th>
<th>Part Number</th>
<th>Organization</th>
</tr>
</thead>
<tbody>
<tr>
<td>1</td>
<td>KMM581000AN</td>
<td>1M x 8</td>
</tr>
<tr>
<td>1</td>
<td>KMM591000AN</td>
<td>1M x 9</td>
</tr>
<tr>
<td>4</td>
<td>KMM584000A</td>
<td>4M x 8</td>
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<td>4</td>
<td>KMM594000A</td>
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<td>8</td>
<td>KMM5362000A</td>
<td>2M x 36</td>
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</tbody>
</table>

Samsung is one of the world’s leading manufacturers of both DRAMs and memory modules. Our outstanding quality, reliability, and availability have helped us gain this leading position.

For data sheets on our 4-meg DRAMs and 4-meg-based modules, call 1-800-423-7364 or (408) 954-7229 today. Or write to Memory Module Marketing, Samsung Semiconductor, 3725 No. First St., San Jose, CA 95134.
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With the TMC1175, video driving amplifiers can be eliminated. The Track-and-Hold circuit is built-in; so is the voltage reference. All digital inputs and three-state outputs are TTL-compatible. And all performance specifications are guaranteed over the -20°C to 75°C temperature range.

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The TMC1175 is available in 24-pin plastic skinny DIP, 28-lead PLCC and 24-lead plastic SOIC (small outline) suitable for surface mount applications.

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TRW LSI Products Inc.

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If you're looking for the right general purpose switch, switch to HP. Our new broadband GaAs MMIC SPDT devices offer low insertion loss and high isolation for improved system performance from DC-6GHz.

HP's great GaAs news also includes a family of high-gain, high-power MMIC traveling wave amplifiers. Each is designed to operate from 2-26.5GHz, and 100% RF tested to provide guaranteed spec performance.

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You can vary the gain of Analog Devices' AD600 and AD602 dual amplifiers from 0 to 40 dB and −10 to 30 dB, respectively, without affecting the 35-MHz, 3-dB bandwidth of the device. The amplifiers comprise a fixed-gain amplifier preceded by a variable attenuator. The attenuator is made up of a 7-section R-2R ladder network, which continuously interpolates between the tap points. The result is very accurate gain; the gain error is ±0.5 dB max at the extremes of the voltage-control range and ±0.2 dB max in the center. The attenuator also prevents large input voltages from reaching the fixed-gain stage, letting its design be optimized for low noise. This fact combined with the linearity of both the attenuator and fixed-gain stages leads to low noise and THD specifications of 1.4 nV/√Hz and −60 dBc, for ±1V outputs, respectively.

The amplifiers implement, in terms of dB, a linear gain law. For example, applying a gain-control voltage of −0.625 to +0.625V, the gain of the AD600 increases linearly from 0 to 40 dB. Group delay is stable and typically ±2 nsec. The amplifiers are optimized for driving flash ADCs in ultrasound applications, but also apply to those circuits that require a combination of precise gain, low noise and distortion, and wide bandwidth. Each amplifier dissipates a maximum of 125 mW. The $15 (100) amplifiers are available in either 16-pin DIPs or SOICs, and operate over a 0 to 70°C temperature range. Analog Devices Inc, Wilmington, MA, (617) 937-1428, FAX (617) 831-4273.—Anne Watson Swager

COMBINATION OPTICAL DRIVE FITS 3½-IN. FORM FACTOR

The 3½-in. OD-3000 multifunction optical drive stores 128M bytes using MO (magneto-optical) technology and can read optical ROM (0-ROM) disks. The MO media can withstand 10 million write cycles and still record data reliably, where other rewritable optical technologies typically limit media to 10,000 write cycles. The drive features a 3000-rpm rotational speed that results in an average rotational-latency spec of 10 msec. The drive requires an average of 42 msecs to seek to data. Other key specs include 11W power dissipation during read/write operations and 2.6W when the drive is inactive. The drive can read data continuously from disk at 640k bytes/sec and write data continuously at 203k bytes/sec. The drive costs $1050 (1000) and the rewritable media costs $60 per disk. Teac America Inc, Montebello, CA, (213) 726-0303, FAX, (213) 727-7621.—Maury Wright

SCSI BUS MONITOR PROVIDES MENU-DRIVEN DEBUGGING

For $895, you can buy Workstation Products Inc's Pathfinder 1000 SCSI bus monitor, which analyzes the activity on your bus- or debug-driver software. Plug this device between your SCSI bus and an ASCII terminal to achieve nonintrusive synchronous or asynchronous monitoring. The device does not use an address on the SCSI bus. In its run mode, the monitor captures commands and data until its event buffers are full. In continuous mode, the monitor continues to capture data until you stop it. In trigger mode, you can specify the condition under which the device begins or stops capturing data. The monitor comes with 2 kbytes of memory, a power supply, manual, and a 6-in. SCSI cable with a 50-pin connector. A monitor with 8 kbytes of memory costs $995. Workstation Products Inc, Richardson, TX, (314) 669-9687.—J D Mosley
NEWS BREAKS

LOGIC-ANALYZER FAMILY BETTERS PRICE/PERFORMANCE RATIO
The TA4000 series of logic analyzers from Thurlby-Thandar embodies a range of advanced features at a bundled price substantially below competitor's products. Three models offer a choice of 32, 48, or 80 channels. Asynchronous sampling is at 100 MHz max across all channels, or at 400 MHz max across 8 or 16 channels. Memory depth at 100- and 400-MHz sampling is 2 and 8 kwords, respectively. A 5-nsec glitch capture operates on eight channels without loss of memory depth. Synchronous sampling is at 50 MHz max across all channels, and includes an 8-level branching-trigger facility that steps at up to 20 nsec. Optional disassemblers cover a range of 8-, 16-, and 32-bit µPs. In addition to internal nonvolatile memory, you can store 512 kbytes of data on a front-panel plug-in memory card. Included as standard in the price are interfaces for IEEE-488, Centronics, RS-232C, and composite video. The 32-, 48-, and 80-channel logic analyzers cost £2495, £2995, and £3995, respectively. Disassemblers cost £195. Thurlby-Thandar Ltd, Huntingdon, UK, (480) 412451, FAX (480) 450409.—Brian Kerridge

ENGINEERING SPREADSHEET WORKS WITH PICTURES
If you've adapted Lotus 1-2-3 to help you analyze data and complex functions, you've sacrificed the visual impact of looking at plots, graphs, and curves. DSP Development Corp's Dadisp (Data analysis and display) provides the spreadsheet's utility while maintaining the visual effect of your data. The data analysis software, which runs on PCs and under the X-Window system on most common workstations, accepts data from numerous sources, including ASCII and binary file formats and many data-measurement and -acquisition devices. Additionally, you can manually enter data sets into a spreadsheet-like table. Once entered, you view and manipulate the data either graphically or in tables. The software includes a range of mathematical, statistical, and engineering functions and lets you create and add custom functions as needed. Special functions include contour plotting, density plots, spectral 3-D plots, and 4-D plots. The user interface provides as many as 100 windows that operate as cells in the X-Y dimension of a 3-D spreadsheet; changing data in the Z-dimension of a cell causes the software to recalculate all dependent data in other cells. You can overlay data and zoom in and out of windows as needed. The software starts at $895. The PC version costs $1695. DSP Development Corp, Cambridge, MA, (617) 577-1133, FAX (617) 577-8211.—Michael C Markowitz

DRIVERS LET YOU COMPARE DRAWINGS IN AUTOCAD
Nth Graphics's Nth Drive display-list processing software and Nth Engine display-controller drivers now include a drawing management and viewing module called Nth View/AC, which lets you open an unlimited number of AutoCAD .DWG files for viewing and plotting without leaving your active drawing. This module produces display-list zooms and real-time pans. An icon-based interface and a command window called the Top N provide pop-up control of your screen. Each drawing you add to the screen appears in a window that you can size, move, and overlap onto other windows. In addition, a garbage-collection scheme works continuously in the background to purge the display list of each vector you erase or move during an edit session. The display controller with a suite of drivers starts at $995. The processing software sells for $695. Both products include the drawing management module. Nth Graphics Ltd, Austin, TX, (800) 624-7552 or (512) 832-1944, FAX (512) 832-5954.—J D Mosley
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The industry's first integrated SPARC® multiprocessing solution — the CY7C605 Multiprocessing Cache Controller/MMU.

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—Anne Watson Swager

RASTER-IMAGE ACCELERATOR IC RENDERS FONTS IN REAL TIME

The D7001 IC renders outline fonts on the fly in graphics-display and page-printer applications. The IC can render outline fonts scaled to any size fast enough for laser printers to print at full engine speeds of 17 pages per minute and slower. A single IC can also be used in mother-board graphics applications to directly drive WYSIWYG (what you see is what you get) display and printer engines. You can use the IC in applications with fonts based on Bezier curves, B-spline curves, and vectors. The chip includes multiple filling algorithms to handle both Roman characters and Kanji glyphs. For 12-point type at 300-dpi-resolution fonts, the IC can render more than 7500 cps. Available now for $35 samples, the IC comes in a 144-pin quad flatpack. Destiny Technology Corp, Milpitas, CA, (408) 262-9400, FAX (408) 262-0221.

—Maury Wright

GATE-ARRAY FAMILY OFFERS HIGH I/O-TO-GATE RATIO

The HG62S gate-array family from Hitachi offers as many as two I/O pins for each 100 used gates. Family members come in sizes from 14,451 to 34,797 raw gates, with 160 to 240 I/O pads. The array uses 0.8-µm, 2-layer metal CMOS technology, has input buffers with 0.8-nsec propagation delay and output buffers with 1.8-nsec delay and 24-mA drive. Internal gate delays are 0.3 nsec for a 2-input power NAND with a fanout of two. The devices are available in EIAJ plastic quad flatpacks in 64- to 208-pin sizes at a cost of $0.07 to $0.10 per pin (10,000). Hitachi America Ltd, Brisbane, CA (415) 589-8500, FAX (415) 583-4207.—Richard A Quinnell

DEVICE CONVERTS CMOS SRAM INTO NONVOLATILE MEMORY

More than just a power source for static RAMs (SRAMs), the bq2502 Integrated Backup Unit from Benchmark provides power monitoring and switching for one or two banks of RAM. This encapsulated DIP module contains a nonvolatile-SRAM controller chip and a 3V lithium battery. To avoid accidental discharge and simplify handling procedures, the manufacturer ships each module with its battery-output pin electrically isolated. After installation, the module monitors $V_{cc}$ to detect an out-of-tolerance power supply, switches to the internal battery supply if $V_{cc}$ decays, write-protects the memory during power failures and during system power-up, then switches back to the $V_{cc}$ supply when reliable operation resumes. Priced at $6 (1000), these modules come in 12-pin DIPs that are less than 0.375-in. tall. Benchmark Microelectronics, Carrollton, TX, (214) 407-0011, FAX (214) 407-9845, contact John Landau.—J D Mosley
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'020/'030 Compatibility
Software compatibility between Synergy SBCs means users have simple upgrades to the SV430 from our '020 and '030 SBCs. Force offers compatibility only from the '030 level, and Motorola offers "upward migration"—a polite phrase that means rewriting your code.

I/O Modules
Synergy's EZ-Bus modules are compatible with our entire line of SBCs. This means Synergy's current line of 12 intelligent I/O modules are immediately available for the SV430—today. No other vendor comes close for selection, functionality or availability.
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lowpass, highpass, bandpass, narrowband IF

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- rugged hermetically-sealed pin models • BNC, Type N; SMA available
- surface-mount • over 100 off-the-shelf models • immediate delivery

Bandpass, Narrowband IF

<table>
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<th>MODEL NO.</th>
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</tr>
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</table>

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<table>
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<th>Vendor</th>
<th>Platform</th>
<th>Operating System/Rev</th>
<th>Description</th>
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<td>Sun OS 4.1.1, Verilog 1.5C</td>
<td>Simulation, Fault grading, Design verification</td>
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<td>Krios</td>
<td>4.0 up</td>
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<td>Mentor Graphics</td>
<td>HP9000, Sun/SPARC, Parade</td>
<td>Sun OS 4.1.1, Verilog 1.5C</td>
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<td>Sun OS 4.1.1, Verilog 1.5C</td>
<td>Design synthesis, Test synthesis</td>
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<td>PC386</td>
<td>DOS 3.3, Workview 4.0</td>
<td>Design capture, Simulation</td>
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</table>

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Questionable values appear in table

In J D Mosley's article, "Improvements unleash new application areas" (EDN, October 11, 1990, pg 97), there is a mistake in Table 1. The data corresponding to Optical Output Power are in fact the data corresponding to Total Power Dissipation. Values of about 100 mW of optical output power for the IREDs (infrared emitters) are far off the values of commercial products.

I have verified the values of the Motorola IREDs in the manufacturers' data book:

**MLED71**
- Total power dissipation . . . 90 mW
- Power output . . . . . . . . 5 mW

**MLED930**
- Total power dissipation . . 250 mW
- Power output . . . . . . . . 4 mW

It’s impossible to check the other IREDs, but I think they are also wrong.

One of the most important applications for these devices is in optical communications; for a good comparison, an additional column should indicate the speed, such as rise and fall times.

_Francisco J Gabiola Ondarra_  
_Profesor Titular de EU_  
_Dpto-Ingenieria Electronica_  
_ETSI Telecommunication_  
_Ciudad Universitaria S/N_  
_Madrid, Spain_

(Ed Note: In Table 1, I used the Motorola Semiconductor values listed in the Motorola data book.)

How discontinued parts affect engineering design

We have had the experience of designing a part (Allegro Microsystems UCN5825B) into a product, and then, just as we introduced the product, found out that the company was discontinuing the part. The part is advertised in the 1991 IC Master, and our distributor [at the time of this writing] had not been informed that the part was discontinued. We found out by accident when calling an applications engineer at the company about another problem.

This part is a BiMOS combination of a shift-register and high-voltage driver. It has four outputs, each of which can handle a 2A drive. Not only is there not a second source for the part, no other part even comes close—at least none that we can find. We not only have to redesign the board, but we also have to either change specifications or squeeze in two packages where one served before.

Perhaps we were foolish in using a single-sourced part, even if it has been available for several years, but most of the company's parts in this category are single sourced. Why would anyone ever use any of them if he or she seriously suspected that the parts would be abruptly discontinued?

I understand that the company has been purchased by a foreign company. Do the new owners think that this method of operation is going to protect their investment?

_Norman L Rogers_  
_President_  
_Z-World Engineering_  
_Davis, CA_

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theory.

feedback you need to eliminate defects where it's most cost-effective—at the source.

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case styles
T, TH, case W 38, X 65 bent lead version, KX81 bent lead version
TMO, case A 11, T case B 13, FT, FTB, case H 16

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T1-1T 5995-01-153-0668
T2-1 5995-01-106-1218
T3-1T 5995-01-153-0298
T4-1 5995-01-024-7626
T9-1 5995-01-165-8153
T16-1 5995-01-984-7439
TMO1-1 5995-01-178-2612

MCL NO. NSN
TM01-1 5995-01-183-6414
TM02-1 5995-01-215-4038
TM02-5-6 5995-01-215-4038
TM02-5-6T 5995-01-215-8697
TM03-1T 5995-01-169-7512
TM03-4 5995-01-067-1012
TM04-2 5995-01-091-3553
TM04-6 5995-01-132-8102
TM05-1T 5995-01-183-0779
TM09-1 5995-01-141-0174
TM016-1 5995-01-138-4593
### FORMERS

3KHz-800MHz from $3.25

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**CASE STYLE NUMBER**

- For A and B configurations
- Maximum amplitude unbalance: 0.1 dB over 1 dB frequency range
- 0.5 dB over entire frequency range

CIRCLE NO. 23

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*Denotes 75 ohm models

**FOR A AND B CONFIGURATIONS**

**Maximum Amplitude Unbalance:**
- 0.1 dB over 1 dB frequency range
- 0.5 dB over entire frequency range

**Maximum Phase Unbalance:**
- 1° over 1 dB frequency range
- 5° over entire frequency range

C72-2 REV. B
You have to build a
to build just

The new Tek TDS Series

More than a million Tektronix oscilloscopes have all been leading up to this: the most powerful, versatile, and intuitive instruments ever developed for the mainstream of test and measurement.

The new TDS 500 Series is the culmination of everything Tek has learned in the design, manufacture and use of digitizing oscilloscopes. It's an achievement made possible only by the unique integration of acquisition functions and combinational trigger logic onto a single board.

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Only by the addition of Tek's TriStar™ Digital Signal Processor (DSP).

Only by Tek's capacity for taking the hard work out of high performance.

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And if you think oscilloscopes aren't as easy to use and comprehend as they
million oscilloscopes
one like this.

could be, you owe yourself a demo of
the TDS. Its simplified front panel,
VGA-quality display resolution, on-line
help text, innovative icons that instantly
differentiate menu functions — all add up
to a scope that makes the user's manual
more a formality than a necessity.

The TDS Series signals the start of a
new generation of friendlier, more
powerful instruments from the
world's leading supplier of digitizing
and analog oscilloscopes. To get a first-
hand feel for why performance like this
only comes along about once in a million
scopes, contact your Tek sales engineer
or call 1-800-426-2200.

One company measures up.

EDN September 16, 1991

CIRCLE NO. 24
Introducing Fluke's 70 Series II, next-generation multimeters that meet the increasing demands of your job and your budget.

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No matter which 70 Series II you choose, you get simple, one-handed operation. High resolution. And built-in, go anywhere reliability.

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Best of all, every 70 Series II is a Fluke, backed by a worldwide service network and an industry-leading 3 year warranty.

So the next time you're in the market for a new meter, ask for the one that guarantees old-fashioned value. Fluke 70 Series II. For more information call 1-800-6789-LIT. Or call 1-800-44-FLUKE, ext 33 for the name of your nearest Fluke distributor.
Reader wants to send real-time video via phone lines

I am looking for videophone boards or modules that will accept/deliver NTSC video and that will send "still" or maybe even near-real-time video signals over standard phone lines.

Tom Hill
Sammons Communications
Duncanville, TX

Unfortunately, off-the-shelf technology hasn't yet advanced to the stage where you can plug a television broadcasting station into your PC. However, sending individual video images via modem is a piece of cake—your computer for hours and running broadcasting station into your PC. as long as you don't mind tying up

The principal stumbling block is your requirement for using "standard phone lines," which seems to indicate that you also want to use a standard 2400-bps phone-line modem. You can do that. You can even use your favorite communications package—just have your communications software send the image as a binary file, rather than ASCII.

However, you have to consider the practical aspects of the task. It isn't unusual for a full-color computer image to encompass half a megabyte of data. To pump this much data through a 2400-bps modem would theoretically take about 56 minutes per image—and that doesn't include pauses for hand-shaking or error correction. Even if you beefed up your equipment to include a 9600-bps modem, each image would require 14 minutes for transmission. Such requirements preclude the 30-frame/sec display rate required for real-time video.

One alternative, suggested by Videotex Systems (Dallas, TX), is to equip both the sending and receiving computers with image-compression boards. Although such boards can reduce your transmission time, they also degrade the image: The greater the compression, the greater the degradation. But even if you bought boards that could provide 100× compression, you still wouldn't reach real-time video rates. And even if you could transmit 15M bytes every second, where would you store all that data?

Our advice is to videotape whatever it is you want to record in "real time" and let an overnight delivery service hand the tape to the person you're trying to reach. You'll both save a lot of time, money, and hassle. And if the objective is to have the recipient alter your images in some way, this delivery method lets that person use the video-input port of a video graphics card to download your recorded images into his or her computer for subsequent manipulation.

Wants to access EDN BBS

I am interested in obtaining a program from your bulletin board system (BBS). I do not have a modem attached to my computer, but the computer is linked to the Janet network, which can access the American Internet system. I am writing to inquire if your bulletin board has an Internet address and if so the method of accessing the program from this connection.

Paul Drummond
The New Medical School
Newcastle-upon-Tyne, UK

The United States National Science Foundation runs Internet, which is a noncommercial service, so we can't get an address on it. EDN has investigated links to commercial services and X.25 networks, but we found that the fees were too high for us to continue to offer a free BBS. However, we're getting some high-speed modems soon and are considering putting another EDN BBS computer in the United Kingdom. This computer would be updated every week via streaming tape.

EDN

Ask EDN solves nagging design problems and answers difficult questions. Address your letters to Ask EDN, 275 Washington St, Newton, MA 02158. FAX (617) 558-4470; MCI: EDNBOS. Or send us a letter on EDN's bulletin-board system at (617) 558-4241; leave a letter in the ask_edn Special Interest Group.
NEW PRODUCTS – NICOLET’S PRO OSCILLOSCOPES

“Measurement Experts” get more choices from Nicolet

Nicolet Pro Oscilloscopes offer advanced trigger options in a waveform-analyzer-class scope

Nicolet invented the first digital oscilloscope to help engineers make better measurements. And for almost twenty years, they continued to focus on producing and improving top-end instruments for their “measurement expert” customers. Nicolet’s new line of “Pro” digital oscilloscopes offers advanced trigger, display and programming features, while maintaining Nicolet’s insistence on the highest standards of data integrity.

Nicolet Pro Oscilloscopes

The seven Nicolet Pro Oscilloscopes range from 8-bit units running at 200 Megasamples per second to differential-input 12-bit high-accuracy models. The Nicolet Pro 90 is a unique configuration of both, with independent timebases for simultaneous recordings at different accuracy levels and speeds.

Advanced Triggering in an Analog World

But the real innovation is that Nicolet has found a way to apply logic-analyzer style “advanced” triggering to the analog world. Many scopes have logic-analyzer style trigger modes. But logic-analyzer implementations of glitch and dropout triggers assume the input signals are square-waves. With most scope applications, baseline noise and variations of input slew rate can mimic the intended trigger events. The results are false triggers, spurious “jitter” on repetitive signals, and incorrect timing on single-shot events – in short, false data.

Nicolet’s new scopes are different, with a unique variable-sensitivity control to prevent false triggers. Only Nicolet Pro Oscilloscopes arm or trigger when the input passes sequentially through two operator-selected voltages, eliminating triggers due to noise or baseline instability. And using the advanced modes is easier than you’d think – Nicolet displays the trigger level and sensitivity right on the waveform, and provides an on-screen icon of the chosen trigger type, source and key parameters.

Quality Measurement for Electronics

Of course, every Nicolet Pro model offers the familiar “quality measurement” features characteristic of Nicolet products, including ultra-long 256K memory, built-in MS-DOS floppy plus optional hard drive, and Nicolet’s on-board programming language, TACT, for custom solutions to most measurement problems without an external PC. And even with four records of 256K each on the screen, Nicolet’s crisp vector display instantly shows you a one-in-a-million transient.

Call Nicolet Test Instruments

(800) 356-8088

Nicolet Pro Digital Oscilloscopes offer advanced triggering with sensitivity control for the analog world of noisy signals.

CALENDAR


Failure Mode and Effect Analysis (seminar), Boston, MA. Quality Alert Institute, 1475 S Colorado Blvd, Suite 206, Denver, CO 80222. (800) 221-2114; in CO, (212) 353-4420. FAX (800) 473-8348. September 27.


Electronic Imaging East, Boston, MA. Miller Freeman Expositions, 1050 Commonwealth Ave, Boston, MA 02215. (800) 223-7126; in MA, (617) 232-3976. FAX (617) 232-0854. September 30 to October 3.


Telecom ‘91: World Telecommunications Exhibition, Geneva, Switzerland. International Telecom-

40 CIRCLE NO. 26

EDN September 16, 1991
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These 5.25" Wren and Elite drives and 8" Sabre drives feature data rates as high as 27 MB/second, average seek times as low as 11.5 msec and latency as low as 5.56 msec. With a choice of high performance interfaces including SCSI, SCSI-2, IPI and SMD, you can easily configure the ideal storage solution for your requirement.

Because these drives utilize Seagate's own thin-film heads, thin-film discs, voice-coil motors and printed circuit boards, you can be assured you're getting the highest quality disc drive available. In fact, our MTBF specification is as high as 250,000 hours in a Class A computer room environment.

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Painted Bamboo and Wire by Nance O'Banner
Oakland, California

CIRCLE NO. 27
The PQFP Test Clip Solution...
...for hands-free testing of SMT PQFP packages.

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- SWEDEN 4-744-0300
- SWITZERLAND 45-48-52-00
- TAIWAN 2-721-9533

You Guessed It!

IEEE GaAs IC Symposium ‘91, Monterey, CA. Jo Ann McDonald, The Legacy Co, Box 151, King City, CA 93930. (408) 385-5321. Registration: (202) 347-5900. FAX (202) 347-6109. October 20 to 23.


Object-Oriented Analysis and Design Seminar, Washington, DC. Technology Transfer Institute, 741 10th St, Santa Monica, CA 90402. (213) 394-8306. FAX (213) 451-2104. October 21 to 23.

munication Union, Place des Nations, CH-1211 Genève 20, Switzerland. (22) 730-5236. (22) 733-7256. October 7 to 15.


Modern Electronic Packaging Seminar, Burlington, MA. Technology Seminars Inc, Box 487, Lutherville, MD 21093. (301) 252-3425. FAX (301) 761-7942. October 9 to 11.

Symposium on High Density Integration in Communications and Computer Systems, Waltham, MA. Harry Lockwood, GTE Laboratories Inc, 40 Sylvan Rd, Waltham, MA 02254. (617) 466-2786. FAX (617) 890-8320. October 17 to 18.

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It's TODD SUPERMAX 1000, an extraordinary OEM power supply of revolutionary proportions. And those proportions are small. Smaller than anything in its class. At just 3.38"H x 8"W x 12"L, its compact size allows for great flexibility in a system's mechanical design. In fact, three SUPERMAX 1000 units can be mounted where two standard shoe box units fit before.

SUPERMAX 1000 is the 1000-watt power supply designed right from scratch with Power Factor Correction built in for maximum performance and economy.

Long recognized as the leading innovator in the power supply industry, TODD now brings its advanced open frame switching power supply technology to the high-power shoe box world. SUPERMAX 1000 requires fewer components, so reliability, efficiency—even “no-fan” cooling—are greatly enhanced.

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Now to help speed your evaluation, the Semiconductor Products Center of Hughes Aircraft Company is offering a special evaluation kit to assist in the development phase of your design. All you need is an IBM™ compatible PC. You can read and program any of the NSP devices, including future NSP devices, right from your keyboard.

The kit contains all the necessary hardware and software. You can be up and running in just minutes. Included is a custom interface circuit, cable to connect to the parallel port of your PC, sample devices, data sheets, complete documentation, and "quick start" instructions.

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In June, I received an announcement from the IEEE (Institute of Electrical and Electronics Engineers) that the group was presenting an award to Apple Computer Inc for creating the personal computer. The award singles out Apple "for the creation and establishment of the broadly successful personal computer." The Apple II computer was very successful and it—along with the Visicalc spreadsheet program—pushed desktop computers into commercial use. However, Apple neither created nor established the personal computer.

The award committee's chairman told me that the IEEE chose its words carefully so that it would not appear that Apple had invented the first personal computer. However, my thesaurus says that both create and establish can also mean originate and start.

The chairman also told me that the committee used only published resources and that it didn't interview people who developed small computers in the 70s. By not talking with those people, the IEEE was led astray. If nothing else, I'm disappointed in the IEEE for its misinformed role in helping to further solidify myth into historical fact. There are many people and many computers that deserve recognition for their roles in advancing us toward today, when PCs are a part of daily life for almost everyone.

History proves that Apple was not the first to create a PC. Back in the late 60s and early 70s Digital Equipment Corporation shrunk its 12-bit PDP-8 into a desktop computer, the PDP-8/L, which became popular in controller applications. A group calling itself the Amateur Computer Society was founded by hard-core hackers in 1970, and many members spent considerable time and money trying to clone DEC's PDP-8/L. As I recall, coming up with the proper core memory was a nightmare.

Once Intel's 8-bit 8008 microprocessor arrived in 1973, designing your own computer became easier. Hobbyist computers such as the Mark-8 and Seebel-8 became available. Intel's more sophisticated 8080 made possible computers such as the MITS Altair and the IMSAI. Later processors from Zilog and MOS Technology formed the heart of the Apple II, Radio Shack's TRS-80, and Commodore's PET. Let's not forget IBM's 5100, a portable computer from 1975 that you could program in APL. Other mid-70s computer developments from the Digital Group, Southwest Technical Products, Processor Technology, Sphere, and others are just too numerous to relate.

In the early days of the microprocessor revolution, there were many parallel and sequential efforts—often somewhat blurred even in the minds of those of us who were present. Apple came in on the tail end of that first burst of innovation. One thing is for sure; Apple neither created nor established the personal computer. The IEEE should withdraw its award as graciously and as quickly as possible.

Jon Titus
Editor

Send me your comments via FAX at (617) 558-4470, or on the EDN Bulletin Board System at (617) 558-4241, 300/1200/2400, 8, N, 1.
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latches. And the first member of our ACT 2 family, the powerful A1280, with 8,000 gates, up to 998 flip-flops, and 140 I/O pins, it’s the highest capacity FPGA today. And our A1240-1 is the fastest. In the A1240-1, 16-bit counters run at 75 MHz, 16-bit accumulators at 33 MHz. Enough capacity and speed to handle almost any application.

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CIRCLE NO. 36
A law regulating the electromagnetic compatibility of many products takes effect in Europe on January 1, 1992. Deciding how to make the products conform will be up to the design engineer. Some specifications have yet to appear, but enough technical information is available to make a start.

Brian Kerridge, European Editor

Ohm's Law, Kirchoff's Laws, and now Europe's EMC Law. All electronic circuits produce electromagnetic emissions (EMI) at some level. Equally, all circuits become susceptible to EMI at some level. Europe's Electromagnetic Compatibility (EMC) Law sets out exactly what levels are acceptable in both cases for your product. In the future, when designing products for Europe, you will have to consider the EMC Law alongside other circuit constraints.

As part of Europe's move toward a single market structure, politicians and technocrats decided to formalize and harmonize EMC regulations. The result is European Directive 89/336/EEC (European Economic Community), entitled Approximation of the Laws of the Member States relating to Electromagnetic Compatibility issued by the Council of European Communities. Products will require a "CE" mark, as well as other documentary evidence, as proof of conformance.

In principle, as from January 1, 1992, it becomes a criminal offense to contravene the regulations. In practice, you still have a breathing space of two or three years in which to prepare.

If you declare compliance and your product fails to conform, ultimately it must be removed from sale and your stock impounded. If you fabricate documentation in order to imply compliance, then your company will face legal action against its European signatory.

The range of products affected by the new ruling is vast. According to an interpretation of the Directive by Chris Grimes, Chief Consultant on EMC with Siemens Plessey Assessment Services, "If an electron flows in your product, then the Directive is applicable to it."

The EMC Directive encompasses regulations on emissions and immunity for conducted and radiated electromagnetic sources, line distortion, and electrostatic discharge (ESD). CENELEC (European Committee for Electrotechnical Standardization) is the European authority producing the new series of technical documents (distinguished by...
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European EMC regulations

European Standard prefix “EN” (from its title in German). Generally, the new documents specify harmonizations of existing specifications from CISPR (International Special Committee on Radio Interference), or the national standards of the European countries. Table 1 identifies the EN documents produced so far and the provisional EN documents (prENs) under development, cross-referenced to established specifications. When deciding which specifications apply to your product, look for product-specific versions first, such as in the case of information technology equipment. If more than one specification applies, adopt the toughest. In the case where no specification exists for your product, the Directive still requires your product to conform to the EMC law. (How to deal with that situation appears later.)

Transition period eases pain

But don't think all issues are cut and dried. Although legislation will be in place from day one, some of the technical specifications will come later. Partly because of this delay, a transition period will enable a smoother switch from National to harmonized European specifications. The end date of the transition period is under consideration, but may extend to 1995. In the transition period, you can either wait, or attain compliance from day one using a mixture of whatever new specifications exist together with prevailing national specifications. Naturally, there is some confusion, and even experts in the same European countries cannot entirely agree on what you need to do to conform. Differences also exist between the EEC's member states over what technical specifications should apply. Even wording of the Directive itself proves troublesome. The Council intends to publish a further document by the end of this year to clarify some issues, such as what “taken into service” and “placed on the market” mean.

Make no mistake, though—despite these discordant notes, the EMC Directive exists and will soon apply throughout the EEC's 12 member states and the four EFTA (European Free Trade Association) countries. By the end of the transition period at the latest, all electronic products must conform, and only harmonized EN specifications will count. Compliance will be mandatory for products in current production, regardless of country of origin.

When politicians, specmakers, and marketeers have had their say, it will be up to you, the design engineer, to decide how to make the product conform.

That your product must ultimately conform is certain. How you reach conformance is less certain. The issues are complex, and subject to various interpretations. At the very least, your company will need to assign one person the responsibility of studying, interpreting, and tracking the developing situation.

Fig 1 shows EDN’s interpretation of the various routes to compliance. Several organizations are already offering specialist help and advice. (See box, “Who can help?”)

Three ways lead to compliance

In overall terms, the route to placing a compliant product on the European market is straightforward. First, you adopt one of three possible methods to convince yourself that the product conforms technically. Then, you apply a “CE” mark to the product and ship it with a declaration-of-compliance certificate.

The certificate must name a com-

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Table 1—European standards relating to EMC

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<th>Emission</th>
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<th>Subject</th>
<th>Equivalent standard</th>
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<td>Radio and TV receivers</td>
<td>CISPR 13</td>
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<td>Household appliances</td>
<td>CISPR 14</td>
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<td>Lighting equipment</td>
<td>CISPR 15</td>
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Notes:
1. European standard designation is EN; provisional status is prEN.
2. No EN number yet, still at harmonization status.

EDN September 16, 1991
European EMC regulations

company signatory. Ideally, that person should be a resident European native. In the case of manufacturers outside the EEC, that person would normally be in the employ of your representative or distributor.

The three methods of reaching a level of confidence that your product complies are:

- self-certification
- third-party certification
- technical-construction file.

Self-certification appears to be the most direct route, as it is informal and involves minimal interactions outside your company. As the Directive stands, this route allows you freedom to do whatever convinces you that your product complies. When you feel certain of compliance, then your path is clear to apply the CE mark and get on with the selling.

The danger with this route is if someone officially challenges your product’s conformance. How able will you be to support your belief that the product does indeed conform? If you are unable to convince the EEC trade authorities, then your product must be withdrawn and your company stands the risk of being blacklist. In extreme cases, your European signatory could end up explaining things in court.

Nonetheless, companies outside Europe will favor this route, especially where the convenience of local EMC test facilities exist. In the case of a challenge, when test results from a reputable source are available, the danger of a product ban diminishes.

Third-party certification is the route that offers optimal assurance that your product conforms. Essentially, you subcontract the work to an accredited laboratory. The laboratory tests, reports, and certifies product compliance. A third-party test house must be accredited, otherwise the laboratory is not authorized to issue certificates. In the UK, NAMAS, a department of NPL, accredits such laboratories. DAE is the accrediting authority in Germany.

At present, accredited labs exist only in Europe. By the end of 1991, NAMAS expects there will be around 30 accredited labs for EMC testing in the UK. Germany will have around 15. Ideas to allow third-party testing in laboratories outside Europe are in the early stages. In the case of self-certification, it is not essential for your laboratory to be accredited.

Paperwork proves powerless

The technical-construction-file route is the most uncertain way to have your product declared compliant. In the first place, there is no clear idea yet of what should be in a technical-construction file. The attraction of this route is that the need for testing is not mandatory. The general intention is that the file

---

**Fig 1—EDN’s guide to compliance with Europe’s EMC Directive.**

---

**NOTES:**
2. European Committee for Electrotechnical Standardization.
3. For example, in the UK the National Physical Laboratory (NPL) is the National Standards Authority and the National Measurement Accreditation Service (NAMAS) is the department within the NPL to handle the accreditation.
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<table>
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<th>FUNCTION</th>
<th>PROPAGATION DELAY (Max)</th>
<th>OUTPUT ENABLE (Max)</th>
<th>OUTPUT DISABLE (Max)</th>
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<td>5.2ns</td>
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<tr>
<td>Transceivers</td>
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<td>4.8ns</td>
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<tr>
<td>Registers</td>
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<td>5.5ns</td>
<td>5.0ns</td>
</tr>
<tr>
<td>Latches</td>
<td>4.2ns</td>
<td>5.5ns</td>
<td></td>
</tr>
</tbody>
</table>

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European EMC regulations

contains sufficient information to convince a “competent body” that your product complies. A competent body is another independent agency, authorized by governments to vet technical-construction files and issue approval certificates. By the end of 1991, each EEC member state’s trade department will issue a list of accredited test houses and competent bodies.

Geoff Orford, at NAMAS, believes the technical-construction-file route, as the directive has outlined it, has little merit. He says that most EMC Standards are simply recipes for testing, and therefore you cannot hope to demonstrate compliance without some tests.

Grimes says the value of the technical-construction-file route shows up when manufacturers have a range of similar products. He recommends manufacturers to third-party test the worst-case product in the range, and then seek compliance for the rest of the range with technical-construction files. The technical-construction-file route also theoretically allows early compliance with the directive in the case of temporary absence of standards. Although, on what basis a competent body will make a judgment remains uncertain.

Grimes says he expects a technical file to include a technical report, a detailed block diagram, photographs, a wealth of EMC test data, and the test equipment’s history.

A CE mark signifies that your product complies with all applicable EEC Directives. Some toys, for example, have to comply with three earlier Directives, and are among

Who can help?

For more information on Europe’s EMC Law, circle the appropriate numbers on the Information Retrieval Service card or use EDN’s Express Request service. When you contact any of the following companies or organizations directly, please let them know you read about them in EDN. When you contact them directly from outside Europe, faxing is the best option. For example, the UK Government’s Department of Trade and Industry EMC office operates a system of taking phone calls by answering machine. The office answers routine overseas queries by fax.

For a copy of Directive 89/336/EEC: Alan Armstrong Ltd
2 Artwirght Rd
Reading RG2 0SQ, UK
(734) 751771
FAX (734) 755164
Circle No. 719

For European Norm documents: BSI Sales
Linford Wood
Milton Keynes MK14 6LE, UK
(908) 221166
FAX (908) 222484
Circle No. 720

For general information on the EMC Directive: Bundesamt für Post und Telekom Herrera Lehning, Referat 124 Postfach 8001 Tempelstrasse 2-4 W-6560 Mainz 1, Germany (011) 18 1200 FAX (011) 18 5600 Circle No. 721

Department of Trade and Industry Tony Bond Manufacturing Technology Div 4E 151 Buckingham Palace Rd London SW1W 8SS, UK (711 215) 1498 FAX (71 215) 1529 Circle No. 722

For accreditation information: Deutsche Akkreditierungsstelle Elektrotechnik Herr Dr Facklam, Geschäftsstelle Stresmannalle 19 W-6000 Frankfurt, Germany (06) 6302 280 FAX (06) 6302 317 Circle No. 723

NAMAS Executive Geoff Orford National Physical Laboratory Teddington TW11 0LW, UK (011) 942 7140 FAX (011) 943 7134 Circle No. 724

International EMC Standards and Test house facilities:

ERA Technology Ltd
Gordon Jackson
EMC Dept
Cleeve Rd
Leatherhead KT22 7SA, UK
(032) 374151
FAX (032) 374496 Circle No. 725

Siemens Plessey Assessment Services Ltd
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(032) 844449
FAX (032) 853354 Circle No. 726

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The SDC-14605 and SDC-14615 series, are two- and three-channel versions of the SDC-14575. All channels are independent, except for the reference inputs and digital output pins, which are shared. Output angle data is enabled onto the tri-state data bus in two or three bytes. Enable MSB (EM) is used for the most significant 8 bits and Enable LSB (EL) is used for the least significant 8 bits.

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For additional information please contact Bill Cullum at (516) 567-5600, extension 389.
European EMC regulations

the first products already displaying CE marks. The first CE marks showing adherence to the EMC Directive should appear by the end of 1991, according to Tony Bond, head of the EMC office of the UK’s Department of Trade and Industry. He believes manufacturers will want to demonstrate compliance sooner rather than later in order to beat competitors.

As the transition period passes, Bond expects purchasing managers to show increasing preference to CE-labeled goods. By the end of the transition period, only goods with the CE mark will be acceptable. Bond warns against procrastinating in complying with the Directive. He points out that it’s more expensive to massage a finished product through to compliance than it is to design in EMC features from the outset.

He also thinks manufacturers in the UK will provide a natural watchdog service over other suppliers. He says the system will be “complaints driven”—competitors will step forward to expose one another.

In Germany, the Ministry of Telecoms has 50 offices spread throughout the country to police contraventions of EMC and other Directives. These offices routinely purchase and test products. If your product is found lacking, you will have to pay heavily for the test work, and be given a fixed period in which to conform. You may also be punished for importing the goods in the first place. Essentially, if you get to this stage in Germany, you’re in big trouble.

All routes demand heavy toll

Attaining compliance will be expensive. Even discounting your additional design effort and manufacturing costs, the extra work in assembling documentation, and the likely need for third-party testing, will cost at least $2500 per design. Naturally, companies flinch at this level of penalty, especially coming at a time when business is not exactly booming. The authorities, recognizing this situation, claim the transition period introduces a degree of flexibility into the approval procedure. But still there is not really a low-cost route.

At a recent forum of EMC-Directive experts in the UK, a delegate from a small company producing custom designs asked how he could afford to meet the Directive and survive. The experts had no satisfactory answer. The only advice from the panel (a test house representative), was to discuss the problem with a test house. It seems that companies in this predicament have a difficult decision to make: They can either dodge the directive and risk getting caught, or go out of business.

If you consider self-certification using your own set-up, the cost is exorbitant. Tom Leahy, technical manager with Schaffner EMC Ltd, estimates a minimum of £280,000 is necessary in order to do emission and immunity testing. Of that figure, £100,000 buys you an electromagnetically shielded and damped room of around 25m², which he says is essential to obtain repeatable test results. Leahy sees that the main problem with setting up your own facility is in locating experienced engineers to make the measurements. He reports mainly multinationals following this route, and only a few of the smaller companies.

For third-party EMC testing, TRL Ltd charges a daily rate of £750, which is typical for the industry. Mark Heaven, EMC consultant with TRL, estimates that compliance tests on the average product will take about two or three days. This period assumes the work goes smoothly, and the product passes. Before you submit a product to TRL, the company likes to consult with you on critical aspects of the design. These consultations minimize the chance of failure in the test house, and therefore limits your expense. According to Heaven, 80% of all EMC failures result from cables. Offending cables include line cords, data-links (such as RS-232C and IEEE-488), and signal leads. Apertures in the product’s enclosure have the second largest effect on a product’s failure.

Heaven says fixing EMC problems in a finished product is often a losing battle, and costly. Unless you carry out substantial redesign, involving changes to the pc-board layout, all you can do is install more shielding or filtering. The best way is to be conscious of EMC requirements throughout the design process. In that way, you can minimize, or even eliminate, additional product and manufacturing cost. Also, you optimize your chance of passing the test routine the first time. Some products cannot avoid cost penalties, however—notably, enclosures for information-technology products. Additional shielding using electroless plating on plastic surrounds increases component cost as much as three to ten times.

Wolfgang Sammet, EMC specialist with Siemens, also emphasizes
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<thead>
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<td>WI, Brookfield</td>
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<td>CA, Van Nuys</td>
<td>Oct. 24</td>
</tr>
</tbody>
</table>

New +5V RS-232 Transceiver Doubles Speed of Existing +5V RS-232 Devices!

The MAX232A +5V dual RS-232 transceiver is specifically designed for low-power operation. Quiescent operating supply current is a mere 500µA unloaded. And, the MAX232A is guaranteed to operate at data rates up to 20kb/s.

RS-232 Transceivers at 1/10th the Power!

The MAX220 dual +5V transceiver is designed specifically for low-power operation. Quiescent operating supply current is a mere 500µA unloaded. And, the MAX220 is guaranteed to operate at data rates up to 20kb/s.

+5V Linear Voltage Regulator Has 150mV Dropout at 200mA

The MAX667 is the only CMOS linear voltage regulator that has both low dropout and ultra-low, 25µA, no-load quiescent current. Ideal for battery-powered applications. Also features 1µA shutdown mode.

Maxim Integrated Products, Inc., 120 San Gabriel Drive, Sunnyvale, CA 94086. Tel. 408/737-7600. FAX 408/737-7194

CIRCLE NO. 43
the importance of good design practice from the beginning. He says particular attention to grounding and short signal paths on your pc-board layout pays dividends. He also meets many problems at a system level. It is quite common for a collection of modules that pass an EMC test as individual units to fail when connected together. This situation highlights the problem of "configuration control," which Sammet sees as the major obstacle in the future. Several EMC specialists suggest Henry W. Ott's Noise Reduction Techniques in Electronic Systems (Wiley-Interscience, 1988) as a comprehensive and readable text to help you design around EMC problems.

Germany leads Europe on the EMC specification front. German National Standards Institution (VDE) specifications for commercial equipment have been around for decades. Siemens's commitment to the EMC business is exceptional. The company has extensive test facilities in Munich and markets a variety of EMC components for products and installations. Siemens has run EMC training seminars for design engineers for the last 20 years. Currently, the program takes place six times a year at international venues. Despite these advances, it is Sammet's view that a lot more needs to be done. In particular, he thinks electricians and technicians, as well as design engineers, need to be aware of, and understand how their work affects EMC.

The impact and complexity of the new EMC legislation is likely to influence all involved to move cautiously through the early months of 1992. Nobody knows exactly what to expect.

So far, every sign from the authorities suggests a common-sense approach, particularly in the UK. The objective of the EMC Law is to be protective more than pernicious. If you can demonstrate that you've taken a responsible attitude, then your problems should be few. The authorities anticipate that most companies will respond in this way, just as they have with safety regulations.

Some anomalous and difficult areas persist, however. It's not likely that they will disappear until the new regulations have passed a burn-in period.

Lack of commonality throughout the EEC is one such problem. In the transition period, for example, it will be possible for different specifications to apply in different countries, but all these specifications will lead to qualifying for the same CE mark. For example, as German VDE specifications are the toughest, it will be attractive to qualify elsewhere. Even after the transition period, it's likely that there won't be common rules for authorizing competent bodies or accrediting test houses. At present, NAMAS in the UK has mutual agreements with France and the Netherlands. The Western European Laboratory Accreditation Cooperation is engaged in providing common rules, but progress is at snail's pace.

Looking further afield, there is

What does it all mean?
The following list of acronyms are in common usage in the Standards and EMC world:

<table>
<thead>
<tr>
<th>Acronym</th>
<th>Description</th>
</tr>
</thead>
<tbody>
<tr>
<td>ANSI</td>
<td>American National Standards Institute</td>
</tr>
<tr>
<td>BS1</td>
<td>British Standards Institution</td>
</tr>
<tr>
<td>CE</td>
<td>European Community, used for CE mark of compliance (from its title in French)</td>
</tr>
<tr>
<td>CENELEC</td>
<td>European Committee for Electrotechnical Standardization (from its title in French)</td>
</tr>
<tr>
<td>CISPR</td>
<td>International Special Committee on Radio Interference (from its title in French)</td>
</tr>
<tr>
<td>DAE</td>
<td>German Laboratory Accreditation Service (from its title in German)</td>
</tr>
<tr>
<td>EEC</td>
<td>European Economic Community (Belgium, Denmark, France, Germany, Greece, Ireland, Italy, Luxembourg, The Netherlands, Portugal, Spain, and the United Kingdom)</td>
</tr>
<tr>
<td>EFT A</td>
<td>European Free Trade Association (Austria, Finland, Sweden, and Switzerland)</td>
</tr>
<tr>
<td>EMC</td>
<td>Electromagnetic Compatibility</td>
</tr>
<tr>
<td>EMI</td>
<td>Electromagnetic Interference</td>
</tr>
<tr>
<td>EN</td>
<td>European Standard (from its title in German)</td>
</tr>
<tr>
<td>ESD</td>
<td>Electrostatic Discharge</td>
</tr>
<tr>
<td>ETSI</td>
<td>European Telecoms Standards Institute</td>
</tr>
<tr>
<td>FCC</td>
<td>Federal Communications Commission</td>
</tr>
<tr>
<td>IEC</td>
<td>International Electrotechnical Commission</td>
</tr>
<tr>
<td>ILAC</td>
<td>International Laboratory Accreditation Cooperation</td>
</tr>
<tr>
<td>NAMAS</td>
<td>National Measurement Accreditation Service (Department of NPL)</td>
</tr>
<tr>
<td>NPL</td>
<td>National Physical Laboratory (in UK)</td>
</tr>
<tr>
<td>prEN</td>
<td>Provisional EN, not fully ratified</td>
</tr>
<tr>
<td>RFI</td>
<td>Radio Frequency Interference</td>
</tr>
<tr>
<td>VDE</td>
<td>German National Standards Institution (from its title in German)</td>
</tr>
<tr>
<td>WELAC</td>
<td>Western European Laboratory Accreditation Cooperation</td>
</tr>
</tbody>
</table>
15-BIT ADC USES ONLY 10 µA SUPPLY CURRENT!

Simple 8-bit µP Interface for $8.00*!

Maxim's new MAX135, low-noise, ±5V-powered, multi-slope integrating ADC, provides ±0.005% accuracy at 16 conversions per second, while requiring only 125µA of supply current over temperature. The MAX135 extends resolution to 18 bits with 3 internal Super LSBs—sub-LSB bits for data averaging. 8-bit data bus and 3 logic control lines simplify µP interfacing. All this comes packaged in space-saving 28-pin DIP and SO packages!

- ±0.005% Accuracy & 15µV Resolution at 16 Conv/sec
- 28-Pin SOIC Replaces 40-Pin DIP
- Supply Current Over Temp: 125µA max (Normal Mode) 10µA max (Sleep Mode)
- 18-Bit Resolution and Improved Accuracy with Data Averaging
- ±10pA Input Current

3-Wire Serial µP Interface Available Soon

Soon, Maxim will introduce the MAX132, a 3-Wire serial-interface version of the MAX135, packaged in a space-saving 24-pin DIP and SO.

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EDN September 16, 1991
CIRCLE NO. 44
LOW DROPOUT REGULATORS

TK114xx
2.0V 2.5V 3.0V 3.25V 3.5V 3.75V 4.0V 4.5V 4.75V 5.0V 5.5V 6.0V 8.0V
- 200 mW Power Rating
- ON/OFF Switch
- Internal Protection Features

TK115xx
2.0V 2.5V 3.0V 3.25V 3.5V 4.0V 4.5V 4.75V 5.0V 5.5V 8.0V
- 600 mW Power Rating
- Low Noise
- Internal Protection Features
- Active HIGH and Active LOW Control
- External Boost Transistor Connectable

TK116xx
2.0V 2.5V 3.0V 3.25V 3.5V 4.0V 4.5V 5.0V 5.5V 8.0V 9.0V
- 500 mW Power Rating
- Internal Protection Features

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Mount Prospect, IL 60056

CIRCLE NO. 45

books that work the way you work

Analog Circuit Design:
Art, Science, Personalities
Jim Williams, Linear Technology Corp., Editor

Troubleshooting
Analog Circuits
Robert A. Pease, National Semiconductor

24 masters of analog circuit design share their experience in this comprehensive and useful guide to analog theory and applications. June 1991 352pp. cloth 0 7506 9166 2 $44.95

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UPDATE

European EMC regulations

a strong case for establishing equivalent competent bodies and accredited test houses outside Europe. This move would make it much more straightforward for international manufacturers to use the third-party test route to comply. However, the likelihood of this happening in the next five years seems remote. Yet another organization, the International Laboratory Accreditation Cooperation, supports the idea, but implementing any program is way off.

The most persistent headaches will result from difficulties of configuration control. For example, if a PC plug-in card complies in PC type A, but fails in PC type B, you will have to decide how many other PC types you should try it in. If you are a systems integrator, your headaches multiply. All your systems may have a different configuration, and the system may pass at one site, but fail at another. If you're a small company making custom designs, it's unlikely you can pass the cost of testing to your customer for every single product.

Europe's EMC Law is here to stay and is certain to disturb the tranquility of your R&D lab. In design-cycle terms, the 1995 drop-dead date is not so far away. Tune in to Europe's EMC emissions, before Europe designs in immunity to your products.

Article Interest Quotient
(Circle One)
High 515 Medium 516 Low 517
FASTEST, +5V-SUPPLY
12-BIT ADC-ONLY $10*

FREE Precision Laser-Trimmed Reference Included On-Chip

Maxim now offers a 7.5µs analog-to-digital converter (ADC) with internal voltage reference, clock, and track/hold that typically consumes less than 3mA (15mW). The MAX190 saves additional power with an on-command power-down that extends battery life in portable applications. And, the new ADC simplifies external circuitry with high-impedance differential inputs and rail-to-rail signal range for both unipolar and bipolar conversions.

✦ Single +5V Supply
✦ 12-Bit Resolution, 1/2LSB Linearity
✦ Internal or External Reference
✦ 7.5µs Conversion Time
✦ Low Power: 15mW typ.
✦ 150µW Power-Down with 35µs Start-Up
✦ Internal Clock and Track/Hold
✦ High Immunity to Latch-Up

On battery power, the MAX190 converts rail-to-rail signals to either serial or parallel data in 7.5µs.

Choose Your Interface: 3-Wire Serial or 8-Bit Parallel

The MAX190 features a 3-wire serial and two 8-bit parallel interface modes for easy µP connection. The MAX190 comes in both plastic and ceramic DIP and SO packages with less than 1/2LSB linearity over temperature.

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**PACEWRAP R3100**
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- Eight-word-deep Write Buffer - with readback.
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- Parity generation - allows use of main memory without parity.
- Bus snooping support.

**BiCameral SCRAM Cache ZIP Module**
- Dual 8Kx60 High-Speed SCRAM
- 32K Byte I and D caches from a single module including address latches.
- Available for up to 33 MHz CPU with minimum board space required.
- Space saving 6.350 x 0.815-inch 124-pin ZIP module

**16Kx60 Cache SCRAM ZIP Module**
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Performance Semiconductor Corporation
610 E. Weddell Drive, Sunnyvale, California 94089
Telephone: (408) 734-9000

CIRCLE NO. 48
QUAD VOLTAGE-OUTPUT 12-BIT DACS REPLACE 4 OP AMPS AND 4 DACS!

Save Valuable Board Space With 24-Pin SO Package

Maxim's new MAX526 quad voltage-output A/D converter replaces 4 digital-to-analog converters (DACs) and 4 op-amps with a single CMOS monolithic IC! The new DAC delivers performance you'd expect from hybrid and module quad DACs. Maxim guarantees monotonic 12-bit performance with 1/2 LSB relative accuracy over temperature for all 4 outputs, and 1 LSB total unadjusted error with no zero- or full-scale adjustments. And, 10V outputs settle to 1/2 LSB in 5µs.

- Four 12-Bit DACs in One Package
- Buffered Voltage Output
- 1 LSB Total Unadjusted Error
- Double-Buffered Logic Inputs
- 24-pin DIP and SO Packages
- Parallel µP Interface

Input Double Buffering & Output Amplifiers Simplify Design

The MAX526's double-buffered 8-bit parallel interface simplifies digital connections by eliminating "glue" logic. The analog interface is also simplified by built-in output amplifiers, eliminating external op-amps and providing the speed and drive needed for most applications.

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Use it to incorporate full 16-bit or 8-bit VGA into low-cost personal computers. You only need two industry standard 256K x 4 DRAMs and as few as five other ICs. Whatever memory speed you select — 80ns, 100ns, or 120ns — you’ll get a complete VGA display system with greater performance than systems using a more expensive solution with 64K x 4 DRAMs.

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Maxim now offers you a selection of the fastest low-power single, dual and quad TTL comparators. For example, the new MAX903 can deliver an 8ns response time, while drawing only 3.6mA (18mW) per comparator from a +5V supply (enabling signals in excess of 100MHz to be processed). Although other comparators may operate from a single supply, the MAX900 series are the only high-speed comparators with an input voltage range that extends down to ground. In many applications this eliminates the negative supply, saving board space, power consumption and cost.

Separate Analog and Digital Supplies Allow:
- Single +5V to +10V Analog Supply
- Split ±5V for Bipolar Operation

Input Range Includes Ground and Eliminates Need for Negative Supply

Select A High Speed Comparator For Your Low Power Application

<table>
<thead>
<tr>
<th>Device</th>
<th># Comps</th>
<th>Prop Delay (ns)</th>
<th>Power Consumption (mW)</th>
<th>Single +5V Operation</th>
<th>Input Voltage (Single +5V Supply)</th>
<th>TTL Outputs</th>
<th>Price†</th>
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<td>125</td>
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<td>+1.25V to +3.5V</td>
<td>Complementary</td>
<td>$3.13</td>
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</table>

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Ask for literature package M14A013.
Bringing order to the welter of high-density programmable-logic devices is no easy task. After conferring with numerous experts, EDN bravely offers this hopefully comprehensive and extensible overview.

Charles H Small, Senior Editor

HIGH-DENSITY PLD ARCHITECTURES

Family tree sorts out high-density PLDs

A mind-numbing variety of high-density PLDs (those having more than 2000 “equivalent gates”) is already available. And hardly a month passes without yet another new or enhanced high-density PLD or two becoming available. Further, unconfirmed sightings of “stealth chips” (publicized, but not announced) suggest that soon even more devices may appear.

EDN interviewed experienced users and high-density-PLD makers, asking each to take a stab at categorizing these devices. No two replies were even remotely similar. However, we synthesized some very general categories, and we submit the family-tree chart in Fig 1 and a supplementary chart (Table 1) for your approval. Though comprehensive, the charts need to be extensible, because when the stealth chips bolt from their secret black projects into the market, they will have to fit in somewhere.

The companies listed offer PLDs having significantly higher capacity than standard PLDs such as the 22V10. Yet notice that neither chart mentions just how much larger. The only metric available for comparing high-density PLDs’ capacities is “equivalent gates.” However, the high-density-PLD industry has not converged on a unified method of calculating equivalent gates. The industry is even further away from coming up with a metric that designers will accept and can use.

This lack of a useful capacity specification for high-density PLDs is unfortunate.

Fig 1—This family tree attempts to break down available high-density PLDs down into useful categories. Hopefully, as new devices appear, they will hang from branches that fit organically into this tree.
The Most Diverse Family In Memory.

Designs That Endure High Temperatures
Consistant Performance At Low Powers
Massive And Reliable Memory
Perfectly Suited For Cold Climates
High Speed Processing Performance

A Complete Line Of 1-Meg SRAMs.
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Fast or slow. Hot or cold. Even your massive memory requirements are right here.

And we can ship the package styles most in demand for your new designs today - and tomorrow. Our new production facility in San Antonio, TX will build on the reputation for timely delivery that has made us a breed apart.

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-40° to +85°c, 3 volts and X9.20 nsec

If your current designs incorporate the latest technology, call us. Virtually every new idea in SRAM will be here at Sony first. And our U.S. design team (with their 0.8 & 0.5-micron CMOS technology) stands ready to get you the right product for your design; whether it's for a laptop or workstation.

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<table>
<thead>
<tr>
<th>1-Meg SRAM</th>
<th>Speed</th>
<th>Packaging</th>
<th>Data Retention</th>
<th>Special Features</th>
<th>Availability</th>
</tr>
</thead>
<tbody>
<tr>
<td>128Kx8</td>
<td>100/120</td>
<td>DIP 600mil</td>
<td>L/LL</td>
<td>B/X</td>
<td>Now</td>
</tr>
<tr>
<td>256Kx4</td>
<td>17/30/35</td>
<td>SOJ 400mil</td>
<td>Sync ASM</td>
<td></td>
<td>3/Q '91</td>
</tr>
</tbody>
</table>

L = Low  LL = Low.Low  B = 3 Volt  X = Extended Temperature
High-density PLD architectures

Experienced users agree that the three most important specs for a high-density PLD are capacity, speed, and price. Incidentally, users are not thrilled with the specs for speed either, finding that using such specs requires careful study of the fine print and considerable experimentation. And while they can get firm specs for price, most think the prices are too high.

Returning to Fig 1, the first and most definite cut of the analytical scalpel divides field-programmable gate arrays (FPGAs) from devices that realize canonical, sum-of-products, Boolean equations. FPGAs have largely uncommitted interconnections. That is, both ends of each possible internal connection are user programmable; the connections between logic elements on-chip are not deterministic. FPGAs compose the logic-based-cell branch of the tree.

The sum-of-products devices, in a fashion very similar to their PAL-device and PLA-device forbears, have at least one end of every internal connection fixed, leaving only one end for you to connect. Their internal connections are deterministic. Sum-of-products devices compose the logic-gate-based branch.

A couple of comments are in order. First, you must realize that FPGA is a misnomer. FPGAs do not resemble conventional mask-programmed gate arrays at all. Unfortunately, the much more apt term “logic-cell array,” LCA, is a trademark of Xilinx. If you could see the die of an FPGA, you would find a rectangular array of logic cells surrounded by a phalanx of I/O cells. Running between (and, in some cases, over) the cells are uncommitted connecting lines of different length and current-carrying capacity. The logic cells of the various FPGAs contain different amounts of logic, and you can program each device’s logic cell into a unique—and sometimes quirky—set of Boolean functions.

The fewer logic elements in an FPGA’s logic cell, the more fine is its “granularity”; conversely, the more logic elements in an FPGA’s logic cell, the more coarse is its granularity. The divisions between fine, medium, and coarse granularity in Table 1 are rough estimations made only for comparison.

An FPGA’s granularity is a compromise between complexity and fan-in. If the granularity is fine, then the FPGA’s simple logic cells will each need few inputs. Hence, fan-in will not be a problem. However, the device will obviously need many logic cells to perform a given function. If, on the other hand, an FPGA’s granularity is coarse, then its more-complex logic cells will be relatively powerful, and you will need fewer of them for a given task. But a complex logic cell will, perforce, need more inputs than a simple cell would, perhaps leading to fan-in problems that may strain the internal-connection resources of the device.

GEC Plessey’s logic cell is little more than a simple gate. Toshiba’s cell is similar because both FPGAs stem from Pilkington designs. The logic cells in initial offerings of Actel’s Act devices were simple combinatorial-logic blocks; the company’s second-generation devices have combinatorial cells and cells containing registers. Compared to Plessey’s Era logic cell, Xilinx’s LCA logic cell is complex, containing both combinatorial logic and registers.

Quicklogic’s devices defy classification. Conceptually, they are AND/OR SOP devices. Physically, they resemble logic-cell arrays, having core macro-cells surrounded by interconnection channels. Algotronix’s logic-cell devices easily connect into rectangular arrays so that you can assemble large blocks of tiled, programmable logic. At press time, information on the Fujitsu devices was sketchy.

Designing with these logic-cell-based devices hearkens back to the days when engineers used discrete logic or small-scale integration (SSI). Breaking up a logic design into bits that will fit into individual cells and then connecting those cells is usually too complex a task to be done manually. Hence, designers rely on software for these tasks. The software they use has much in common with place-and-route software for printed-circuit boards.

Boolean equation realized

The logic-gate devices on the left of Fig 1 have the same theoretical underpinning as earlier PAL devices and PLA devices: the fundamental theorem that says you can realize any logic function with a sum-of-products Boolean equation. You can sum ORed, NANDed, or NORed products leading to AND-OR, NAND-NAND, or NOR-NOR sum-of-products equations. The elegance and simplicity of these equa-
High-density PLD architectures

tions translates into a simple, regular structure for a programmable-logic device.
Their simplicity and regularity also beget simpler and faster-compiling software than the software for FPGAs. Designing with the logic-gate-based devices has much in common with designing for PAL devices. However, their prewired structure suffers from the same bugaboo that haunts PAL devices: low gate-utilization rates.
The designers of logic-gate-based, high-density PLDs have enhanced earlier PAL-device and PLA-device architectures in several ingenious ways, striving to make their devices' layouts more flexible. Altera, for example, hard wires only three AND terms to each OR gate in its Max devices. To set up product terms having more than three ANDed inputs, you wire in some floating, uncommitted AND gates. Thus, the device does not have the rigid 8-AND-gates/OR-gate structure of many PAL devices. Note that this flexibility costs you some extra delay when you wire in floating gates.

Similarly, Advanced Micro Devices' Mach devices allow you to assign blocks of ANDed terms, in groups of four, among OR gates. Actel's Act devices also share product terms. Lattice's pLSI devices permit you to allocate groups' connections at several levels. National's MAPL devices contain "pages" of PLAs. Just like the MAPL devices' PLA-device ancestors, the connections between ANDed terms and OR gates are completely programmable.

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TECHNOLOGY UPDATE

High-density PLD architectures

FPGA. These devices are indeed arrays of a single type of gate—NAND gates and NOR gates, respectively. However, these arrays of gates still do not even remotely resemble a conventional mask-programmed gate array. In Signetics’ and Exel’s devices, a programmable crosspoint matrix potentially connects any gate’s output to any gate’s input. Thus, these devices’ so-called “folded” architecture permits chaining NAND or NOR gates to realize the sum-of-products form.

But these are no ordinary gates. Even the most brilliant logic designer will have to spend some time thinking through the possibilities inherent in, for example, Signetics’ array of 256-input NAND gates. Obviously, fan-in will never be a problem.

Future high-density PLDs will add more leaves and branches to the family tree in Fig 1. Fig 2 provides a conceptual model for other areas high-density PLDs may move into. This figure ranges digital devices along three axes. Note that, except for finite-state-machine sequencers, programmable logic falls on the control-logic axis. Future high-density PLDs could move in new directions, combining control logic with data storage or data handling.

WHAT’S COMING IN EDN
The Magazine Edition’s October 1, 1991, issue will include EDN’s DSP-chip directory. This annual feature updates the latest developments in the rapidly evolving technology of digital signal processing (DSP). In addition to updating the chips’ many parts and features, this year’s directory addresses how the choices of operating systems and interfaces to host operating systems are making DSP available to more applications.

Also coming in EDN in October and November is more from the mind of Jim Williams. We’ll devote 50 pages to his study of high-speed analog design.
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Bulk-micromachined accelerometers combine a silicon membrane—formed by chemical etching—with thin-film piezo resistors connected in a bridge circuit. In operation, acceleration exerted on the device deforms the membrane, resulting in a change in the resistance of the piezo resistors and producing a small output from the bridge circuit. But bulk-micromachined accelerometers are usually sensitive to temperature variations—not a desirable attribute in automotive applications—and require complex external signal-conditioning circuitry to amplify and linearize the output signal. The size of bulk-micromachined devices also makes them relatively expensive.

By contrast, surface-micromachined devices are typically only 10 to 20% as large as bulk-type devices, thereby providing more efficient use of silicon real-estate. Of even greater importance, surface micromachining uses conventional IC fabrication techniques, which allow the manufacturer to include the signal-processing circuitry on the same chip as the micromachined structure. The specific nature of its surface-micromachined structure and signal-processing circuitry distinguishes this accelerometer.

The structure forms a capacitive sensor that, when viewed from above, looks like a letter H. The long, thin arms of the “H” act as tethers to secure the floating micromachined element to the substrate. The thicker central mass is free to move in a plane perpendicular to the tethers. Projecting from the central mass is a series of filaments that look like the fingers of a comb. Each of these filaments is one plate of a series of parallel-plate variable capacitors; the other plates are secured to the substrate and interleave with the moving-mass plates. Acceleration or deceleration in the axis of sensitivity exerts a force on the central mass that displaces the interdigitized capacitor plates, causing a fractional change in capacitance.

The device operates within a force/balance electronic control loop. Basically, this circuitry splits a carrier signal into two phases, 180° apart. These signals then are transferred to electrodes on opposite sides of the movable center member. There is no signal on the center member if the structure is perfectly centered. Under acceleration, one capacitor increases in value while the other one decreases, causing the phase of the carrier on the higher side to appear on the center member. Other circuitry then amplifies, demodulates, and filters this signal to produce a 0.25 to 4.74V output that is proportional to acceleration.

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The ADXL-50, which operates over the −55°C to +125°C temperature range, comes in a 10-pin, TO-100 metal can. The device costs $23 (100); in automotive OEM quantities, it costs $5.—Dave Pryce
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Circle No. 732

EDN’s Editors’ Choice

On occasion, a new product will show a great deal of innovation and thus appear as an EDN Editors’ Choice selection. To qualify for special coverage by our editors, an innovative product must:
• Offer significantly higher levels of performance in ways not previously available
• Solve a continuing problem much more effectively than its predecessor
• Exhibit a marked degree of cleverness, which differentiates it from earlier products
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These versatile devices withstand rough handling and retain your data even when exposed to dust, dirt, moisture, magnetic fields, and other environmental hazards.

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On the stimulus side, Tek’s new HFS pulse generators feature a revolutionary digital architecture with up to 18 channels and full functionality to 630 MHz. You can stress timing margins by adjusting each channel’s edge placement with 10 ps resolution at all frequencies.

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Push the limits without pushing your luck: let your Tek sales engineer show you the characterization system that easily pays for itself. Or call 1-800-426-2200 for assistance.
Low-power, 1.8-in. hard-disk drive holds 21.4 Mbytes, withstands 200g shocks

Discard your notions of the appropriate applications for hard-disk drives. The 1.8-in. Model 1820 drive stores 21.4M bytes in a head-disk assembly measuring 0.394 × 2.01 × 2.76 in. The drive employs a separate controller card measuring 0.276 × 2.01 × 3.03 in. Together, the two components weigh 95 g. You can mount the drive and controller card independently or piggyback the controller on the head-disk assembly. The controller card has an IDE (integrated drive electronics) interface, which is the interface PCs commonly use. Engineering samples of the product cost $485.

The disk drive runs on 5V and can run from batteries. It draws 2W while reading or writing information, 1W when idle, 35 mW in standby mode, and 15 mW in sleep mode. The drive spins up in 1.5 sec typ, so you can keep it in the sleep mode most of the time for many applications. Its automatic power management lets you realize large power savings using the drive's sleep mode while still servicing data-transfer requests.

During the first second of activation after receiving a data-transfer request, the drive consumes 3.5W. In the next second, the drive consumes 2W while performing the requested data transfer. For the next five seconds, the drive is in its 1W idle mode. While in the idle mode, the drive keeps the platter spinning in case another data-transfer request appears. If no requests are made during the 5-sec idle time, the drive drops into its 35-mW standby mode. After another five seconds of inactivity, the drive goes into its 15-mW sleep mode. The company claims the hard-disk drive consumes much less power than competing products because of this power-management scheme.

The 1.8-in. hard drive employs a loading ramp that keeps the heads off the disks while the drive is switched off. The loading ramp gives the drive its 200g shock immunity. The ramp also pushes the number of start/stop cycles the drive can endure to 1,000,000 because the heads never touch the storage media. Because no reliability penalty is incurred for stopping the platter's rotation, the 1.8-in. hard drive can save power by frequently entering its idle and sleep modes. Consequently, the automatic time delays for activating these modes are much shorter than for disk drives that land their heads on the media when the platters stop rotating.

The drive's electronics are on a separate controller card, so you can fit the device into thin spaces. The controller and head-disk assembly communicate via a flat cable. The controller circuitry includes a 32-kbyte data buffer, and the IDE disk interface can transfer data in bursts at 4 Mbytes/sec. The drive's average seek time is 20 msec, and the heads can move from track to track in 8 msec. A 40-Mbyte version will be available in the second quarter of 1992.

—Steven H Leibson

Circle No. 730
The basic idea behind our new

Updating your system code, to say the least, has been a pain. Well, erase those painful memories.

Introducing Intel Boot Block Flash Memory. The first blocked flash memory architecture that includes four separately erasable blocks with one "lockable" block for critical boot code. A remarkable design that allows one 1Mb Boot Block Flash Memory chip to eliminate up to three memory chips.

It also allows you to reconfigure your system quickly and easily so you don’t lose precious time getting to market. Also, future updates—whether it’s for hardware or software—are easy. For instance, updating a PC BIOS is as easy and cheap as sending your customers a floppy disk. And all

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you need to change your embedded program code is a serial link. Life should be so simple.

Intel Boot Block Flash Memory has two configurations compatible with microprocessors and microcontrollers that boot from either high or low memory. Such as the i960™ microprocessor or the industry-standard Intel386™ and Intel486™ microprocessor families.

Now that you have the basic idea, we'd like you to know more. So call (800)548-4725 and ask for Literature Packet #A6A38. And be the first on your block to make updating easy with Intel's new Boot Block Flash Memory.

you to know more. So call (800) 548-4725 and ask for Literature Packet #A6A38. And be the first on your block to make updating easy with Intel's new Boot Block Flash Memory.

Intel

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At last, an entirely new approach to clock speed

Get five times faster throughput from NEC K-Series™ microcomputers.

As a developer of real-time control systems, you know that designing in a faster CPU is not enough. You also need intelligent I/O management for the best possible system throughput.

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The K-Series’ unique architecture includes a revolutionary Peripheral Management Unit™ macro service for nonstop instruction execution while processing up to 16 I/O requests at the same time. By designing in the K-Series microcomputer, you can improve your system throughput by as much as 5X.

The K-Series 8-bit and 16-bit microcomputers give you a real-time output port; an advanced counter/timer system; a high-speed, high-resolution A/D converter; and many other on-chip intelligent peripherals.

Not since the invention of the hourglass has anyone come up with a more ingenious way to speed up silicon.

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To learn more about the K-Series microcomputers with up to 1K bytes of on-board RAM, 32K bytes of ROM/EPROM, and Peripheral Management Unit coprocessoring power, call now.

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Ireland Tel: 1-6794200. Telex: 90847.
Italy Tel: 02-6709108. Telex: 315355.
Korea Tel: 02-551-0450. Fax: 02-551-0451.
The Netherlands Tel: 040-445-845. Telex: 51923.
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Spain Tel: 419-4150. Telex: 41318.
Sweden Tel: 08-753-6020. Telex: 13839.
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UK Tel: 0908-891133. Telex: 326781.
USA Tel: 1-800-632-3951. Fax: 1-800-726-9288.

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A PERSPECTIVE ON DESIGN ISSUES:

Breaking the analog barriers to optimum system design

IN THE ERA OF

MegaChip
TECHNOLOGIES
Advanced Linear extends the boundaries of system performance.

Innovative analog circuits from Texas Instruments add a new edge to Digital Equipment's proven market winners. They can do the same for you.

The goal Digital Equipment Corporation set was clear: Strengthen its position as the leading supplier of Ethernet-based local area network products. Achieving the goal has been spurred by the use of Advanced Linear circuits from Texas Instruments.

These leadership ICs meet growing industry demand for linear circuits that can improve overall system performance and reliability, reduce costs and speed design cycles.

These were precisely the advantages Digital's designers needed.

Expertise and teamwork carry the day

For many years, Digital has used a wide variety of TI linear circuits — from op amps to mixed-signal devices — and values our analog viewpoint toward system design.

As Digital defined the requirements to meet its market goal, the decades-long relationship entered a new era of even more intense cooperation. With Digital handling system-level design and TI applying its linear expertise, the two teams fully utilized our LinASIC™ design methodology to create a series of mixed-signal Ethercell™ functions. They are the basis for the advanced linear devices Digital requires.

The design flow was aided by our Boston-area Regional Technology Center that provides access to LinASIC development tools and by the extensive use of EDIF to exchange information.

Enhancing Digital's competitive edge

To date, close teamwork has produced components that can enhance Digital's ability to respond quickly to market demands for feature-rich but lower cost Ethernet and communications products:

- A dual driver and dual receiver IC that minimizes the number of components required for the Attachment Unit Interface (AUI) function in an Ethernet network.
"Utilizing TI's LinASIC mixed-signal design methodology allows us to design cost-effective solutions with aggressive time-to-market goals."

— Nick Ilyadis, Product Engineer
Telecommunications and Networks Group
Digital Equipment Corporation

- An octal receiver created to solve system-level cross-talk noise problems in RS-232, -485 and -423 applications. This full-custom device, fabricated in TI's Advanced LinCMOS™ process, is designed to meet EIA and CCITT specs.

- A device that will be a complete AUI multiport concentrator on a chip. Fabricated in our LinBiCMOS™ process, it will replace a 6-inch by 12-inch circuit board that incorporates nine discrete ports, logic devices and analog circuitry. The new device will tie any combination of as many as eight units into Ethernet.

- A single-channel 10BASE-T twisted pair interface chip that includes internal precompensation and full duplex operation. Also fabricated in our LinBiCMOS process, this IC cuts component count and improves data transmission.

The Ethercell devices developed by Digital and TI will be incorporated into our existing LinASIC cell library.

**Extensive mixed-signal capabilities**

As Digital recognizes, few in the industry can match our experience in analog design and digital design. This expertise enables us to effectively combine high-performance analog functions with leadership digital functions. The resulting mixed-signal devices typify our capabilities to design and develop the Advanced Linear circuits our customers need.

**Let us help you meet your challenge**

We are ready to provide information and assistance, as well as access to the hardware and software development tools you need, to help extend the boundaries of your system performance.

Our service circles the globe, and our worldwide manufacturing capability can support your production schedules wherever you are.
TI's analog viewpoint: From process technologies come Advanced Linear ICs.

TI's LinASIC mixed-signal methodology —
A cell-based design methodology allowing the combination of high-performance analog and digital functions on the same chip. This mixed-signal capability is used for many of our catalog products and for custom/semicustom solutions. It is supported by large cell libraries, design-automation tools and these TI Advanced Linear wafer process technologies:

LinBiCMOS — Combines Advanced LinCMOS, digital ASIC CMOS and up to 30-V bipolar technologies to allow the integration of digital and analog standard cells and handcrafted analog components on a monolithic chip.

LinEPIC™ — One-micron CMOS double-level metal, double-level polysilicon technology that adds highly integrated, high-speed analog to the high-performance digital EPIC™ process.

Advanced LinCMOS — An N-well, silicon-gate, double-level polysilicon process featuring improved resistor and capacitor structures and having three-micron minimum feature sizes.

Power BIDFET™ — Merges standard linear bipolar, CMOS and DMOS processes and allows integration of digital control circuitry and high-power outputs on one chip. Primarily used for circuits handling more than 100 V at currents up to 10 A.

Multi-EPI Bipolar — A very cost-effective technology that utilizes multiple epitaxial layers instead of multiple diffusion steps to reduce mask steps by more than 30%. Used to produce intelligent power devices that can handle loads as high as 20 A and voltages in excess of 100 V.

Excalibur — A true, single-level poly, single-level metal, junction-isolated, complementary bipolar process developed for high-speed, high-precision analog circuits providing stable op amp performance.

For more information on our Advanced Linear process technologies and the products they are producing, call 1-800-336-5236, ext. 3425.

TI's LinASIC methodology and Advanced Linear process technologies are enhancing these product families

Data Transmission — This family meets the needs of most industry-standard interfaces (EIA, IEEE, ANSI) and ranges from drivers/receivers/transceivers to fully integrated controller/transceivers.

Data Acquisition — The family ranges from stand-alone A/Ds and D/As to complete data conversion subsystems on a chip; from general-purpose functions to highly integrated digital signal processor and graphics signal processor analog interface circuits. Other specialized family members include telecom and speech synthesis functions.

Intelligent Power — These devices combine high-voltage and/or high-current switches with the analog and digital circuitry required to perform interface, control, protection and diagnostic functions in microcontroller-based systems.

Operational Amplifiers — A family of op amps and comparators ranging from standard bipolar to leadership high-performance CMOS and Excalibur complementary-bipolar devices, meeting needs ranging from low power and/or low noise to high speed and/or high precision.

Custom/semicustom Functions — In modifying existing products to fit your needs or in defining your own unique functions, our LinASIC methodology allows access to existing analog cells used in the development of our catalog products and compatibility with our digital cell libraries.
Announcing a night to recognize greatness

EDN's Innovation and Innovator of the Year Awards Ceremony

On the night of November 19 during Wescon, EDN will present the 1991 Innovation and Innovator of the Year awards at the Mark Hopkins Hotel in San Francisco. You are invited to show the finalists that you support greatness in innovation by attending the awards ceremony that is the culmination of their hard work. Through its Innovation Crusade, EDN hopes to inspire engineering professionals within the electronics field to reach for higher plateaus of inspiration and creativity.

The dedication and involvement of EDN readers, like yourself, have made the Innovation Crusade and awards ceremony a reality. By taking the time to nominate your peers and, in fact, select the winners, you show commitment to quality and creativity in electronics and are driving this crusade. But don't stop there ... order your ticket to the industry event of the year and show these innovators that greatness does not go unrecognized. All proceeds of the dinner will be donated to the EDN Scholarship Fund.

To receive a reservation order form to the EDN 1991 Innovation Dinner and Awards Ceremony, fax Pam Winch at (617) 558-4470.

To receive an Innovation Ceremony Reservation form, please Circle no. 59.
The technology in these number crunchers is developing so fast that about the only things moving faster are the instructions and data they handle. Besides faster µ.Ps, architectural innovations—especially parallel and pipelined processors—are adding to the boards’ speed. But as is so often the case, software is struggling to keep pace.

Dan Strassberg, Associate Editor

Digital signal processing (DSP) is one of the most rapidly evolving areas of electronics. And within the DSP field, coprocessor boards are quite possibly the fastest-changing product category. Most of these boards plug into a computer's I/O bus and increase the computer's speed by performing DSP functions while the main processor handles housekeeping chores and other low-speed tasks. In April 1990, when EDN last took a comprehensive look at these boards (Ref 1), they were just beginning to employ parallel and pipelined processors. Today, the use of multiple DSP chips is rapidly becoming commonplace. However, system developers who use the boards have few software options to simplify allocating tasks among the multiple µ.Ps.

Table 1 (pg112) lists 38 DSP coprocessor boards from 26 firms. We selected these products from a field of more than 70 boards, most of which had not yet been introduced at the time of our April 1990 story. In choosing units for the table, we picked products that, by and large, did not appear in our earlier listing and which, in our opinion, indicate trends. As noted above, one trend is the use of multiple processors. Twenty of the boards in the table contain more than one µ.P. And the product information that vendors sent us covered even more multiprocessor boards. Another clear trend is the use of floating-point DSP chips. Two dozen of the boards in the table include them.

Despite its throughput limitations, the ISA bus—represented by 20 boards—remains the most popular bus for DSP coprocessor boards. All but one of the ISA bus boards are for the 16-bit, IBM PC/AT version. The VMEbus is well represented too; 11 DSP coprocessor boards incorporate multiple µ.Ps, high-speed I/O, and extensive memory capacity to broaden the field of applications within your computer’s grasp. (Photo courtesy AT&T Microelectronics and Heurikon Corp)
Processors from Texas Instruments, Motorola, and AT&T are the most prevalent, with a smattering of boards using parts from other semiconductor companies.

boards plug into the VMEbus. The table also shows three NuBus boards for Apple Computer's Macintosh II family, one Micro Channel Architecture board for IBM's PS/2 series, one board for the STD Bus, and one board in the diminutive Sbus format of Sun Microsystems' SPARCstations. Bear in mind that, despite its length, the table lists no more than half of the boards introduced in the past 18 months. For example, although the only Sbus board shown comes from Sonitech International, at least one other firm, Ariel Corp, makes Sbus DSP boards. Moreover, nearly all of the boards in EDN's April 1990 listing are still available.

As you might expect, processors from Texas Instruments, Motorola, and AT&T are the most prevalent, with a smattering of boards using parts from other semiconductor companies. Intel's i860 makes an appearance on a VMEbus board from CSPI. CSPI chose the Intel RISC chip because of the µP's extremely powerful floating-point processor. CSPI's competitors don't question the chip's floating-point capability; they do ask whether the i860's performance justifies its price. Some doubt whether the i860, which has the I/O structure of a general-purpose processor, can keep pace with the I/O data rates DSP chips must usually handle. CSPI is not alone in liking the i860 for DSP, though; you should look for the IC in board-level DSP products scheduled to appear within the next six months from at least one other manufacturer.

The i860 is not the only unusual DSP µP to appear on a DSP board. Array Microsystems' boards use the firm's own frequency-domain processor and controller chips. Array's literature boasts that its boards let you "plug in the world's fastest DSP." Impact Technologies' Viper 8704/30-30 sports four vector processors from Zoran Corp. Multisignal Technology's MTAP-90 also uses four processors, three of which come from United Technologies. Two of the listed boards use processors from Analog Devices Inc. One comes from the transoceanic partnership of Spectrum Signal Processing in British Columbia, Canada and Loughborough Sound Images in England. The other is the lowest-priced board in the table, Street Electronics' $175 Echo DSP, scheduled for introduction next month. Analog indicates that several other firms offer coprocessor boards based on its DSP chips, but these board vendors failed to respond to our information requests.

Most DSP operations are I/O intensive. Consequently, many DSP boards have extensive I/O capabilities. As standard features, at least six of the listed boards provide analog I/O facilities (A/D and D/A converters). Many other boards have high-speed parallel or serial digital I/O ports. Some of the parallel ports, especially the wide ones, are extraordinarily fast. Two vendors specify their boards' parallel-port transfer rates at 20M bytes/sec. One claims its port operates at 40M bytes/sec, and another says its port runs...
at 64M bytes/sec. (That's more than 0.5G bits/sec!) Despite many engineers' perceptions that DSP techniques are mainly for speech and audio work, the use of DSP has expanded into motion control and many other fields. As DSP applications diversify, users' I/O requirements are changing. Board vendors are responding to the changing requirements in several ways. One way is the inclusion of mezzanine buses. Mezzanine buses turn plug-in boards into small systems. A mezzanine bus is a connector with defined pinout and timing standards that accepts daughter cards. The daughter cards usually perform I/O functions, but some provide other facilities. For example, they can add extra memory for a processor, and sometimes they contain additional (parallel) processors.

Mezzanine-bus daughter cards often fit within the confines of the board they plug into, but not always. Sometimes, the daughter cards occupy additional slots in the bus that accept the main board. In such cases, the daughter cards may connect with the main bus only to receive power and ground. Daughter cards that occupy main-bus slots receive mezzanine-bus signals from the main board via a short cable or "frontplane." A frontplane is a printed board or semirigid set of conductors that plugs onto a connector at the edge of a board opposite its main-bus connector.

A mezzanine bus by another name ...

Apparently, some vendors use definitions of a mezzanine bus that are broader than the one given above, whereas other firms use more restrictive definitions. For example, Datel Inc sells its DSP boards only with plug-on daughter cards that perform I/O. Even though Datel has a family of pin-compatible daughter cards, the company refuses to categorize these cards' interface as a mezzanine bus. When you review the table, be mindful that different vendors have different understandings of the meaning of a mezzanine bus.

Although bus-board manufacturers have defined several mezzanine buses, each of which is vying for acceptance as a de facto industry standard, only a few of these buses appear on the listed boards. One mezzanine bus that is compatible with products from at least three DSP-board vendors is Data Translation's DT-Connect. The table shows a large number of proprietary buses. In general, if you select a board that uses a widely supported mezzanine bus, you will have a greater choice of compatible devices than if you select a board whose mezzanine bus is proprietary.

Not only is DSP I/O intensive, it is memory intensive. Some of the listed boards have provisions for accommodating prodigious amounts of memory. DSP µPs need fast memory, and the boards almost always implement their fastest memory with static random-access memory (SRAM) chips. Often, the boards configure the SRAM as cache, but the maximum size of the cache is frequently larger than the tens of kilobytes common with most CISC (complex-instruction-set-computer) µPs.

For economy (and to hold pc-board area within practical limits), when DSP boards accommodate many megabytes of memory, most of the memory usually consists of dynamic RAM (DRAM). DRAM, though slower than SRAM, is less costly and more dense. Approximately one-third of the listed boards accommodate 8M bytes or more of DRAM without need of mezzanine-bus memory cards. The table lists six DSP boards that accommodate 64M bytes of DRAM. The six boards come from three vendors. Note that 64M bytes is more storage than you'll find on the much slower but nonvolatile hard disks of most personal computers in use today!

DSP work demands EEs' skills

As has happened time and again during the last decade, hardware developments have outpaced software advances. Many of the key players in DSP applications development have had no formal training in software engineering. Instead they are EEs who have acquired software skills on the job. But DSP work cries out for

Packing DSP onto the tiny format of Sun Microsystems' Sbus presents a difficult challenge to board designers. But several firms have met the challenge. One of them is Sonitech International.
### Table 1—Representative DSP coprocessor boards

<table>
<thead>
<tr>
<th>Vendor</th>
<th>Model; when introduced; price</th>
<th>Processor/clock speed (MHz)/ number of processors</th>
<th>Memory (bytes) for 1/0 functions</th>
<th>Bus/DMAs?/ mapping</th>
<th>Mezzanine bus/width (bits)/speed (bytes per sec)</th>
<th>Memory (bytes) for program and data</th>
<th>I/O functions</th>
<th>On base board</th>
<th>With mezzanine card(s)</th>
</tr>
</thead>
<tbody>
<tr>
<td>Analogic/CDA</td>
<td>MSP-8C30; $981; $7090 to $18,500</td>
<td>TMS320C30/30/32</td>
<td>ISA-16/yes/ NS</td>
<td>SCSI/8/1.5M; Pixel/16/NS</td>
<td>0-D 64k-S</td>
<td>32M-D</td>
<td>SCSI, $500 Pixel bus connects to separate VCA card.</td>
<td></td>
<td></td>
</tr>
<tr>
<td>Array Microsystems</td>
<td>a66550; NS; $11,900</td>
<td>a6611/25/1</td>
<td>ISA-16/no memory</td>
<td>NA</td>
<td>768K</td>
<td>768K</td>
<td>I/O port—15-MHz burst-rate I/O; magnitude and phase</td>
<td></td>
<td></td>
</tr>
<tr>
<td>Ariel Corp</td>
<td>DSP-C40; $91; $4995</td>
<td>TMS320C40/NS/1</td>
<td>ISA-16/yes/ I/O and memory</td>
<td>DT-Connect/ 16/20M 32-bit/40M</td>
<td>Proprietary/ 1M-D 32k-S</td>
<td>64M-D 6M-S</td>
<td>2-channel, 16-bit oversampling ADC and DAC</td>
<td></td>
<td></td>
</tr>
<tr>
<td>MP3210; $91/</td>
<td>DSP3210/33/2</td>
<td>ISA-16/yes/ I/O and memory</td>
<td>DT-Connect/ 16/20M 32-bit/40M</td>
<td>Proprietary/ 1M-D 16k-S</td>
<td>64M-D 2M-S</td>
<td>See unit above</td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>MM-96</td>
<td>DSP96002/33/1 or 2</td>
<td>ISA-16/yes/ I/O and memory</td>
<td>DT-Connect/ 16/20M 32-bit/30M</td>
<td>Proprietary/ 1M-D 192k-S</td>
<td>64M-D 768k-S</td>
<td>All I/O functions are on external cards</td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Quad-processor; 11/91; $9995 to $13,995</td>
<td>DSP56001/NS/2 or 4</td>
<td>VME 6U/ yes/NS</td>
<td>Proprietary/ 24/NS</td>
<td>144k-S</td>
<td>576k-S</td>
<td>Next computer DSP port</td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Atlanta Signal Processors Inc</td>
<td>Vortex; 5/91; $4995 to $13,995</td>
<td>TMS320C40/30/30/1</td>
<td>ISA-16/yes/ I/O and memory</td>
<td>'C31/12/22.2M Memory/ 32/22.3M</td>
<td>2M-D 256k-S</td>
<td>64M-D 2M-S</td>
<td>68-bit, 20M-byte per sec communication ports; 2-way, 16-bit ports; 1 serial</td>
<td></td>
<td></td>
</tr>
<tr>
<td>Banshee</td>
<td>VMD; 1/91; $4995 to $14,295</td>
<td>TMS320C30/33/1</td>
<td>VME 6U depends on host/memory and I/O</td>
<td>'C30/32/22.2M</td>
<td>256k-S</td>
<td>16M-D 2M-S</td>
<td>1 TTL serial; 2 RS-422</td>
<td></td>
<td></td>
</tr>
<tr>
<td>Cheetah</td>
<td>$9995 to $12,795</td>
<td>DSP96002/33/1</td>
<td>ISA-16/yes/ I/O and memory</td>
<td>96002 I/O/ Memory/ 32/22.2M</td>
<td>64k-S</td>
<td>64M-D 2M-S</td>
<td>2 25M bit per sec serial; 20M byte per sec parallel</td>
<td></td>
<td></td>
</tr>
<tr>
<td>AT&amp;T Microelectronics</td>
<td>WE-DSP32C-BV-MVE; Q4/90; $9995</td>
<td>DSP32C-SE/5/2/4</td>
<td>VME 6U/ yes (serial and parallel ports)/ memory</td>
<td>Serial bus/ 2 wire/100k (Phillips ICbus)</td>
<td>1M-D 512k-S</td>
<td>4M-D 512k-S</td>
<td>NA</td>
<td></td>
<td></td>
</tr>
<tr>
<td>Burr-Brown</td>
<td>ZPB3400; 6/91; $4495</td>
<td>DSP32C/50/1 or 2</td>
<td>VME 6U/ yes/ memory</td>
<td>Proprietary/ 18/20M</td>
<td>1M-D 256k-S</td>
<td>4M-D 512k-S</td>
<td>NA Several analog I/O cards</td>
<td></td>
<td></td>
</tr>
<tr>
<td>Communications Automation and Control Inc</td>
<td>XCC-A0; 3/91; $995 to $1295</td>
<td>DSP-32C/40/1</td>
<td>ISA-8/no/ I/O</td>
<td>NA</td>
<td>64k</td>
<td>256k</td>
<td>Serial communication with ADCs, DACs, DSP boards</td>
<td></td>
<td></td>
</tr>
<tr>
<td>MC5-CO; 6/91; $1495 to $3495</td>
<td>DSP-32C/50/1</td>
<td>Micro-channel/ NSNS</td>
<td>Proprietary/ serial/16M bps</td>
<td>256k</td>
<td>1M</td>
<td>Serial communication with DSP boards</td>
<td></td>
<td></td>
<td></td>
</tr>
</tbody>
</table>

**Notes:**
1. NS=Not specified.
2. "D" after number of bytes denotes dynamic random-access memory (DRAM).
3. "S" after number of bytes denotes static random-access memory (SRAM).
4. NA=Not applicable.
5. VGA=IBM Video Graphics Array display standard.
6. Also performs block floating-point operations.
7. The DT-Connect standard originated with Data Translation Inc.
8. "OS"—operating system.
9. The so-called "6U" VME board is the most common VMEbus board size.
10. Although the boards are available only with daughter cards, the vendor does not describe the interface between the main card and the daughter cards as a mezzanine bus.
11. I/O daughter cards mount to Tiger 40 board but cause the board to use two bus slots.
12. "E" after number of bytes denotes electrically programmable read-only memory (EPROM).
13. In the $5995 version, the UT68S32 operates at 15 MHz and performs 75M floating-point operations per sec (FLOPS).
14. MOPS=millions of operations per sec.
15. SRAM is divided equally between processors. Each processor's memory is half local and half global.
16. "N" after number of bytes denotes nonvolatile memory.
17. "R" after number of bytes denotes read-only memory.
### Supporting software (and price, if not included with board)

<table>
<thead>
<tr>
<th>Supporting software (and price, if not included with board)</th>
<th>Comments</th>
</tr>
</thead>
<tbody>
<tr>
<td>Drivers for Interactive Unix; image libraries; MSPrtx OS*</td>
<td>Dual-banked memory lets both processors access 32M bytes of RAM simultaneously with no wait states.</td>
</tr>
<tr>
<td><a href="https://example.com">IBM PC- and VAX-based system simulators</a></td>
<td>Vendor says board does FFT-based frequency-domain functions faster than any competitor. (Vendor also sells VME boards using same µPs.)</td>
</tr>
<tr>
<td>Assembler/linker, optimizing C compiler, C drivers, DT-Connect drivers applications libraries</td>
<td>Has oversampling inputs and outputs with tracking filters.</td>
</tr>
<tr>
<td>C compiler/assembler; C drivers; DT-Connect drivers; VCOS OS; applications libraries</td>
<td>Same as unit above. In addition, dual processors perform 50M FLOPS peak.</td>
</tr>
<tr>
<td>Optimizing C compiler and OS, $2425; C and hardware drivers; monitor; applications libraries</td>
<td>Proprietary Hyperbus has two ports per board, allowing delay chains of indefinite length. Dual processors perform 100M FLOPS peak.</td>
</tr>
<tr>
<td>C drivers; Assembler/linker, $495; Symbolic debugger, $495</td>
<td>Operates at 54 MIPS. Lower indicated price includes two processors; higher price includes four.</td>
</tr>
<tr>
<td>Assembler/linker/C compiler; source debugger; Spox OS; signal generation and analysis, $3000</td>
<td>The 'C31 can process I/O for the 'C40 or can function independently. Uses dual-port memory for communicating with host PC. The Ashell program provides an integrated development interface.</td>
</tr>
<tr>
<td>Assembler/linker/optimizing C compiler/source debugger, $1595</td>
<td>Listed software tools run on IBM PCs. Data communication uses true dual-ported memory.</td>
</tr>
<tr>
<td>See Vortex board</td>
<td>Works with same Ashell program as Vortex board. 56001 processors can control I/O or function independently.</td>
</tr>
<tr>
<td>C compiler assembler, simulator, applications library, $3800</td>
<td>175M floating-point operations per sec; 75M instructions per sec. All three I/O ports (2 serial; 1 parallel) have DMA.</td>
</tr>
<tr>
<td>Driver, monitor; applications developer (DisplayXL), $1495</td>
<td>A similar board for the 16-bit ISA bus (Model AC5-40) costs $200 more and has a 50-MHz DSP32C. This board also has the serial mezzanine bus of the board below.</td>
</tr>
<tr>
<td>Assembler/linker/simulator, $495; C compiler, $1000; application library, $95; debugger, $395</td>
<td>See board above; also spectral display/digital scope (no charge)</td>
</tr>
</tbody>
</table>

Table continued

### DSP coprocessor boards

EEs' background in the underlying theory relating the time- and frequency-domain descriptions of signals; the work does not place a premium on the discipline that a software-engineering curriculum instills. DSP work also demands the resourcefulness that many EEs have developed through working on projects without having sufficient tools.

EEs are pragmatic as well as resourceful, though. When they have the option of creating their own tools (because few exist) or taking advantage of existing ones, they will usually try to use what's available. For example, EEs no longer write much DSP code in assembly language. The advent of complex floating-point DSP chips with rich instruction sets and tools such as high-level-language compilers and source-level debuggers has made coding DSP routines in assembly language unattractive in comparison with writing high-level code. Of the high-level languages, C is by far the most popular. Assembly still often gets the nod for fixed-point DSP chips and for coding routines whose operating speed is critical. Usually though, system software developers don't write such routines themselves; they take the routines from libraries developed by others.

Multiprocessing has added a new dimension to developing DSP applications software. The most straightforward multiprocessing case occurs in a real-time system that has many similar input channels, each of which produces data requiring identical or nearly identical processing. If a single DSP µP can't handle all the processing chores quickly enough, several processors can. You can assign groups of channels to each µP, but you have to make sure not to assign more tasks to a processor than it can complete before it must work on the next set of data.

*Mezzanine buses make for flexible expansion of a DSP board's I/O, memory, or processing capabilities. Here, Data Translation's DT-Connect bus (on the ribbon cables at the top) links a frame grabber board to the firm's DT2878, which contains a DSP32C.*
<table>
<thead>
<tr>
<th>Vendor</th>
<th>Model; when introduced; price</th>
<th>Processor/clock speed (MHz); number of processors</th>
<th>Bus/Domain; mapping</th>
<th>Mezzanine bus/width (bits)/speed (bytes per sec)</th>
<th>Memory (bytes) for program and data</th>
<th>I/O functions</th>
<th>On base board</th>
<th>With mezzanine card(s)</th>
</tr>
</thead>
<tbody>
<tr>
<td><strong>Communications Automation and Control Inc</strong></td>
<td>SC5; 12/90; $1495 to $1795</td>
<td>DSP; 32C/50/1</td>
<td>STD (8 or 16 bit)/no/ I/O</td>
<td>Proprietary/ serial/16M bps</td>
<td>64K</td>
<td>256K</td>
<td>See board above</td>
<td>See board above</td>
</tr>
<tr>
<td>CSPI</td>
<td>Supercard SC-2XL; VME; 6/91; From $8500</td>
<td>i860/40/2</td>
<td>VME and VSB/yes/ memory</td>
<td>CSPI (publicly available)/ 64/160</td>
<td>2M</td>
<td>16M</td>
<td>VSB interface is operation</td>
<td>NA</td>
</tr>
<tr>
<td>Dalanco Spry</td>
<td>250; 12/90; $1055 to $1395</td>
<td>TMS320C25 or TMS320E25/40/1</td>
<td>ISA-16/now/ I/O</td>
<td>Proprietary/ 16/20</td>
<td>72K</td>
<td>384K</td>
<td>None</td>
<td></td>
</tr>
<tr>
<td><strong>Data Translation</strong></td>
<td></td>
<td>DSP32C/50/1</td>
<td>ISA-16/now/ I/O</td>
<td>DT-Connect/ 8 or 16/10 MHz</td>
<td>2M</td>
<td>8M</td>
<td>mezzanine board allows doubling of memory</td>
<td>NS</td>
</tr>
<tr>
<td>Datel Inc</td>
<td>PC-430 Series; 5/91; $3995 to $4595</td>
<td>TMS320C30/32/1</td>
<td>ISA-16/yes/ I/O and memory</td>
<td>NS&lt;sup&gt;10&lt;/sup&gt;</td>
<td>512k-D</td>
<td>512k-D</td>
<td>32k-S</td>
<td>32k-S</td>
</tr>
<tr>
<td><strong>DSP Research</strong></td>
<td></td>
<td>TMS320C40/50/1</td>
<td>ISA-16/yes/ NS</td>
<td>2 (I/O and memory/32/ 100M)</td>
<td>DT-Connect/ 1540M</td>
<td>64k-S</td>
<td>66M-D</td>
<td>2M-S</td>
</tr>
<tr>
<td>Eighteen Eight Laboratories</td>
<td></td>
<td>DSP32C/50/1</td>
<td>ISA-16/yes/ (3 channel)/ I/O</td>
<td>Span 32/32 (data) 24 (address/20)</td>
<td>256k-E&lt;sup&gt;12&lt;/sup&gt;</td>
<td>256k-S</td>
<td>4.25M-S</td>
<td>4M on mezzanine board</td>
</tr>
<tr>
<td>Heurikon</td>
<td>Surfboard; 6/91; $8495 to $9995</td>
<td>DSP32C-5E/25/4</td>
<td>VME 8U/ yes (serial and parallel ports)/ memory</td>
<td>Serial bus/2 wire/100k (Philips ICBus)</td>
<td>1M-D</td>
<td>512k-S</td>
<td>4M-D</td>
<td>512k-S</td>
</tr>
<tr>
<td><strong>Impact Technologies</strong></td>
<td>Viper8704/ 30-30; 1990; $15,990 to $33,990</td>
<td>Zoran ZR34161/30/4</td>
<td>This board was described more fully in EDN’s April’90 directory but is included here because of its unusual use of four vector processors.</td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td><strong>Multisignal Technology Corp</strong></td>
<td>MTAP-90; 8/91; $5995 to $6995</td>
<td>One UT69532IQMAC</td>
<td>One UT69538832As</td>
<td>ISA-16/now/ through address and data registers</td>
<td>Proprietary/ 32/80M</td>
<td>768k-S</td>
<td>4M with mezzanine board</td>
<td>Data transfer via 6 local buses</td>
</tr>
<tr>
<td>National Instruments Corp</td>
<td>NB-DSP23201; 5/91; $3495</td>
<td>TMS320C30/27/1</td>
<td>Nibus/yes/ memory</td>
<td>RTS/serial bus/8 33M bits per sec</td>
<td>256k</td>
<td>1.28M</td>
<td>NA</td>
<td>Vendor supplies 9 boards for RTSI bus</td>
</tr>
<tr>
<td>Pacific Cyber/ Metrix Inc</td>
<td>DSP-3A; 6/91; $17,779</td>
<td>TMS320C30/40/3</td>
<td>VME 8U/ yes/ memory</td>
<td>Yes (not named)/32/ 100M</td>
<td>2M</td>
<td>3.5M</td>
<td>7.5M with mezzanine board</td>
<td>VSBuses/ 3 40M-byte per sec parallel ports</td>
</tr>
<tr>
<td>Pentek Inc</td>
<td>4823; 6/90; $6995 to $7995</td>
<td>TMS320C30/32/1</td>
<td>VME 8U/NS/memory and I/O</td>
<td>Intel Mix bus/ 32/10M</td>
<td>128k-E</td>
<td>256k-S</td>
<td>8M-D</td>
<td>2 serial (synchronous); 2 timer/counters; 2 general I/O</td>
</tr>
</tbody>
</table>

**Notes:**
1. NS = Not specified.
2. *D* after number of bytes denotes dynamic random-access memory (DRAM).
3. *S* after number of bytes denotes static random-access memory (SRAM).
4. NA = Not applicable.
5. VGA = IBM Video Graphics Array display standard.
6. Also performs block floating-point operations.
7. The DT-Connect standard originated with Data Translation Inc.
8. OS = Operating system.
9. The so-called '6U' VME board is the most common VMEBus board size.
10. Although the boards are available only with daughter cards, the vendor does not describe the interface between the main card and the daughter cards as a mezzanine bus.
11. I/O daughter cards mount to Tiger 40 board but cause the board to use two bus slots.
12. 'E' after number of bytes denotes electrically programmable read-only memory (EPROM).
13. In the $5995 version, the UT69532 operates at 15 MHz and performs 75M floating-point operations per sec (FLOPS).
## Supporting software (and price, if not included with board)

<table>
<thead>
<tr>
<th>Supporting software</th>
<th>Comments</th>
</tr>
</thead>
<tbody>
<tr>
<td>pSOS + Unix-compatible OS, C and Fortran compilers for SPARC CPUs</td>
<td>Includes FIR filter code generator and data-acquisition software. Block move commands transfer data to PC memory at 3M bytes per sec without DMA.</td>
</tr>
<tr>
<td>Assembler, debugger, hardware interface routines, waveform editor, sample code (included)</td>
<td></td>
</tr>
<tr>
<td>C compiler, $1500; support library, $500; advanced image-processing library, $1495</td>
<td>Total harmonic distortion more than 68 dB below full scale to fifth harmonic. Can transfer 4M samples per sec without pauses (1 channel).</td>
</tr>
<tr>
<td>C source debugger, libraries for all on-board devices and communicating to host</td>
<td>Development package with optimizing C compiler, $1495. As many as 16 boards connect together. PC- and workstation-based tools support multiple µPs.</td>
</tr>
<tr>
<td>598 microcoded routines in PROM; support for C, Fortran, and Pascal included</td>
<td>You can call the microcoded routines from high-level programs in languages from seven vendors. Runtime software supports 8 boards simultaneously.</td>
</tr>
<tr>
<td>C compiler, assembler, simulator, applications library, $3800</td>
<td>175M floating-point operations per sec, 75M instructions per sec. All three ports (2 serial, 1 parallel) have DMA.</td>
</tr>
<tr>
<td>Microprogram routines, monitor, debugger included</td>
<td>Meta-assembler, $2000. Sustained operation at 100 MLOPS and 40 MOPS. Slave unit adds 2 ALUs and a floating point unit.</td>
</tr>
<tr>
<td>Analysis library, $695; interface kit, $295; Labview 2, $1995; developer tool kit, $2500</td>
<td>Board has master and slave NuBus interfaces. When board is slave, bus master can write to memory on board. As master, board transfers to host memory.</td>
</tr>
<tr>
<td>Support function library and development utilities included</td>
<td>Performs block DMA at 80M bytes per sec. Cross-complier kit and Spox OS, $5100. FIFO buffers between µPs and to external ports.</td>
</tr>
<tr>
<td>Debugger, Spox OS with ADC and DAC drivers; run on Sun-4 and IBM PC/AT</td>
<td>Board vendor has ported Comdisco Systems Signal-Processing Workstation software to this board.</td>
</tr>
</tbody>
</table>

### Using the Macintosh II family to develop and run DSP applications

Another approach—exemplified by boards from AT&T and Heurikon—uses both parallelism and pipelining. In these boards, there are two groups of three pipelined processors. The three processors in each group work in sequence on the same data: The first processor places its output data in a buffer; the second processor takes data from the buffer, processes it further and deposits it into a second buffer; the third processor receives its input from the second buffer and does still more processing. The processors run algorithms that divide the tasks so the buffers don't overflow and the processors don't have to wait for new data. The pipelined processors are fast enough to keep up with new data as it appears in real time.

Designing the algorithms so that the pipelined processors get along harmoniously and keep up with real time is not a trivial job. So far, there doesn't appear to be any commercial software that automatically optimizes the sharing of tasks among the processors. However, Comdisco's (Foster City, CA) Signal-Processing Worksystem (SPW), a $25,000 (approximately) workstation-based development package, optionally includes a graphical tool called Multiprox (MPX) that assists you in dividing the work. Once you've made a cut at assigning the tasks to processors, SPW will generate the code and simulate the results. If you are unsatisfied, you can try dividing the work differently.

As happens early in the life of most technologies that exhibit great potential, DSP is in ferment. The processor chips' capabilities are increasing rapidly. The cost of a given amount of computational power is declin-
<table>
<thead>
<tr>
<th>Vendor</th>
<th>Model; when introduced; price</th>
<th>Processor/clock speed (MHz)/ number of processors</th>
<th>Bus/EMA7/ mapping</th>
<th>Mezzanine bus/width (bits)/speed (bytes per sec)</th>
<th>Memory (bytes) for program and data</th>
<th>On base board</th>
<th>With mezzanine card(s)</th>
</tr>
</thead>
<tbody>
<tr>
<td>Sonitech International Inc</td>
<td>5SBus; 5/91; $3995 to $6995</td>
<td>TMS320C30/33/1</td>
<td>SBus (1 slot/NS memory)</td>
<td>Parallel I/O expansion/32 data, 4 address/32M</td>
<td>Min 256k-S Max 2M-S</td>
<td>2 µP serial ports, 1 µP parallel port</td>
<td>NA</td>
</tr>
<tr>
<td>Spectral Innovations</td>
<td>MacDSP II; 4/91; $7995</td>
<td>DSP32C50/2/ 68000/10/1</td>
<td>NuBus/yes/ I/O</td>
<td>NA</td>
<td>2M-D</td>
<td>2M-D</td>
<td>2M-D</td>
</tr>
<tr>
<td>Spectrum Signal Process- ing Inc</td>
<td>VASP; 3-board set; Q0/1; $45,265 to $110,515</td>
<td>DSP96002/27/5</td>
<td>VME/yes/ memory</td>
<td>Signal Bus/64/100M</td>
<td>640k-N* 1.46M-S</td>
<td>160M-D (dual-ported)</td>
<td>NA</td>
</tr>
<tr>
<td>Street Electronics</td>
<td>Echo DSP; 10/91; $175</td>
<td>TMS320C30/32/4</td>
<td>VME 9U by 400 mm/ master/ slave VME interface</td>
<td>NA</td>
<td>1.25M-S</td>
<td>1.5M-S</td>
<td>Synchronous interface 64M bytes per sec</td>
</tr>
<tr>
<td>Texas Instruments</td>
<td>TMS320C40 PDDS; 8/91; $15,900</td>
<td>TMS320C40/50/4</td>
<td>Uses ISA-bus half-card controller or SC6 port</td>
<td>Global bus/32/100M 8 communication ports/serial/20M</td>
<td>18k-R 512 (cache)</td>
<td>1.5M with mezzanine board</td>
<td>Global bus and ports described at left at left</td>
</tr>
<tr>
<td>Zola Technologies</td>
<td>Dual DSP Audio Card; Q0/91; $2500 to $5995</td>
<td>DSP56001/32/2</td>
<td>NuBus/NS/ all data memory mapped to bus</td>
<td>NA</td>
<td>120k</td>
<td>120k</td>
<td>NA</td>
</tr>
</tbody>
</table>

Notes:
1. NS=Not specified.
2. '·D' after number of bytes denotes dynamic random-access memory (DRAM).
3. '·S' after number of bytes denotes static random-access memory (SRAM).
4. NA=Not applicable.
5. VGA=IBM Video Graphics Array display standard.
6. Also performs block floating-point operations.
7. The DT-Connect standard originated with Data Translation Inc.
8. 'OS'='operating system.
9. The so-called '6U' VME board is the most common VMEbus board size.
10. Although the boards are available only with daughter cards, the vendor does not describe the interface between the main card and the daughter cards as a mezzanine bus.
11. I/O daughter cards mount to Tiger 40 board but cause the board to use two bus slots.
12. 'E' after number of bytes denotes electrically programmable read-only memory (EPROM).
13. In the $5995 version, the UT6932 operates at 15 MHz and performs 75M floating-point operations per sec (FLOPS).
**DSP coprocessor boards**

<table>
<thead>
<tr>
<th>Supporting software (and price, if not included with board)</th>
<th>Comments</th>
</tr>
</thead>
<tbody>
<tr>
<td>Runtime and DSP libraries included, development systems</td>
<td>Architecture is same as those of vendor’s VME, ISA-16, and Micro-channel boards.</td>
</tr>
<tr>
<td>Same as board above</td>
<td>VMEbus master operation lets board transfer data from frame grabbers without host intervention.</td>
</tr>
<tr>
<td>Runtime library included, development systems</td>
<td>80 M FLOPS. Communication ports, each with its own DMA control, let you set up P arrays of your choice (tree, ring, cube, etc.).</td>
</tr>
<tr>
<td>Signal analysis, $495; array processor library, $495; assembler/simulator, $500; DSP library, $100; C compiler, $1500</td>
<td>Supports Apple Real-time Operating System Executive (AROSE), which provides pre-emptive multitasking and round-robin task scheduling with 110-µsec context switching. DSP µPs communicate via dual-ported SRAM.</td>
</tr>
<tr>
<td>Assembler/linker, C compilers for IBM PCs and Sun stations, $495 to $3900</td>
<td>Three board types: general signal processing, I/O, and 2-port memory. Maximum price includes 5 fully loaded memory boards. Typical configuration processes 2.2G FLOPS peak.</td>
</tr>
<tr>
<td>Symbolic monitor/debugger, assembler/linker, C compiler, simulator, Spox OS</td>
<td>Unit is both a DSP board and a complete i386-based PC system board for passive-backplane systems.</td>
</tr>
<tr>
<td>Monitor/debuggers, high-level language interface library, assembler, $500; C compiler, $2500; simulator, $2000</td>
<td>Board has 55-square-cm prototype area.</td>
</tr>
<tr>
<td>See board above, Spox OS (Price NS)</td>
<td>Has 2 memory expansion connectors. Allows 80 M bytes of program and 24G bytes of data storage.</td>
</tr>
<tr>
<td>Assembler, linker, debugger, signal-processing library, Spox OS</td>
<td></td>
</tr>
<tr>
<td>Low-bit-rate speech coding and music recording/playback software</td>
<td>Very low-cost board with a programmable DSP µP, ADC, and DACs. Development software comes from the chip vendor, Analog Devices. Microphone and speakers included.</td>
</tr>
<tr>
<td>Optimizing ANSI C compiler, assembler, linker, debugger, run-time library, Spox OS drivers, simulator</td>
<td>Parallel debugger uses JTAG scan interface to permit development of software that runs simultaneously on a virtually unlimited number of TMS320C40s.</td>
</tr>
<tr>
<td>Assembler, linker, librarian, $495; algorithm design and modelling package, $995; sound recording, editing playback, $995</td>
<td>Base price is for board alone. Maximum price is for board, external data-acquisition unit and software.</td>
</tr>
</tbody>
</table>

14. MOPS=millions of operations per sec.  
15. SRAM is divided equally between processors. Each processor’s memory is half local and half global.  
16. ‘-N’ after number of bytes denotes nonvolatile memory.  
17. ‘-R’ after number of bytes denotes read-only memory.
Manufacturers of DSP coprocessor boards

For more information on DSP coprocessor boards such as those described in this article, circle the appropriate numbers on the Information Retrieval Service card or use EDN's Express Request service. When you contact any of the following manufacturers directly, please let them know you read about their products in EDN.

**Analogic CDA**
8 Centennial Dr
Peabody, MA 01960
(508) 977-3009
FAX (508) 977-9220
TLX 681-7408
Mike Drumm
Circle No. 401

**Array Microsystems**
1420 Quail Loop Rd
Colorado Springs, CO 80906
(719) 540-7999
FAX (719) 540-7950
Circle No. 402

**Ariel Corp**
441 River Rd
Highland Park, NJ 08904
(908) 349-2900
FAX (908) 249-2123
TLX 4987279
Tony Agnello, President
Circle No. 403

**Atlanta Signal Processors Inc**
770 Spring St
Atlanta, GA 30306
(404) 892-7265
FAX (404) 892-2512
William E Jouris
Circle No. 404

**AT&T Microelectronics**
565 Union Blvd
Allentown, PA 18103
(610) 372-2447
Circle No. 405

**Bridgeworth Signal Processing Inc**
Box 469
Custer, WA 98240
(604) 335-9003
FAX (604) 335-9073
Circle No. 406

**Bruehl and Kjaer**
Naerum Hovegarde 18
DK-2850 Naerum Denmark
(206) 828-6560
FAX (206) 827-3721
Circle No. 407

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DSP coprocessor boards

when the system boards of all PCs and workstations include at least one DSP µP. The firms are hoping that Medialink will establish the standard for communicating with DSP µPs in computers based on 80x86 CPUs.

A move to workstations and to the VMEbus

But DSP-board vendors' interest in the VMEbus—a bus that has long been a mainstay of the workstation world—provides evidence of a different sort of change: The increasing power of DSP chips and the growing popularity of multiprocessor architectures are causing engineers to look closely at developing new DSP products on VMEbus-based workstations rather than on PCs. Not only do workstations perform important development tasks, such as compilation, faster than most PCs do, the VMEbus can accommodate larger boards that use more dc power than those that fit PCs. Also encouraging the use of workstations for DSP development is the growing availability of workstation-based DSP development tools.

But from a DSP-board standpoint, not all is rosy on the workstation front. Although several vendors have introduced boards for the Sbus of Sun Microsystems' SPARCstations, the small board format limits the units' capabilities.

All the evidence points to a continuation—even an acceleration—of the breakneck pace of change in the world of DSP boards. Fueled by increases in the power of DSP chips and reductions in the chips' cost, potential new applications will mushroom. With the explosion in applications will come the need for new and different boards—flexible ones for development work and low-cost ones for use in some of the DSP-based products the development work will produce.

References
2. Leibson, Steven H, "DSP development software," EDN, November 8, 1990, pg 156.

Biomation announces Configurable Logic Analysis System (CLAS) support for Texas Instruments and Motorola Digital Signal Processors (DSPs). The DSP tools include support for the TMS 320C25, TMS 320C30, and DSP 56001. The tool consists of probing hardware, disassembly software, and all setup files. Each DSP support tool for the CLAS range in price from $2950 to $3950.

The CLAS family of logic analyzers provides up to 384 channels configurable as one to four independent analyzers for monitoring multiple processors at speed. The analyzer can capture and correlate all bus cycles at up to 50 MHz on all channels and can provide hardware timing capabilities with 1 nsec resolution. The new CLAS 2000 features an embedded controller with a 13" color monitor. The 96-channel base unit sells for $15,950, including probes.
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The PC is the most popular computer for engineering development work, but lack of graphics-display and printing standards has blocked developing appropriate workstation-class engineering software. Windows 3.0 opens the flood gates.

Steven H Leibson, Executive Editor

While workstation vendors and users continue their quest for the framework grail, PC software vendors have had most of the major framework components dropped in their laps in one package. This boon, in the form of Microsoft Windows 3.0, promises to unshackle the PC's latent ability to do workstation-level engineering work and costs less than $100 per copy. Many vendors of software packages for applications ranging from engineering design to data acquisition already offer Windows-compatible programs, and many more programs are being developed.

According to the EDN News Edition's 1991 EDA survey, the PC holds a solid lead over all other computers as an engineering development platform (Ref 1). Of the top four computer types used for electronic design automation, 80386-, 80286-, and 80486-based PCs hold positions 1, 2, and 4, respectively. The 80486 μP is relatively new, so you can expect PCs to hold the top three positions next year.

PCs dominate engineering

Taken as a group, PCs dominate engineering work. Even so, several factors prevent engineering-software vendors from fully exploiting the advanced PC hardware available today. One of the chief culprits has been DOS. Even version 5, the latest DOS incarnation, offers little support for graphics and suffers from a relative lack of memory. Programs running under DOS 5 are still limited to 640 kbytes of RAM. Consequently, PCs with many megabytes of RAM and high-performance, high-resolution displays need individual treatment from engineering-software vendors. Each machine is a special case.

DOS program developers either ignore high-performance PCs by writing code for the lowest common denominator or create and support numerous device drivers for the various PC displays, printers, and mice. These hardware-support activities can divert software...
vendors’ resources away from making improvements to the engineering aspects of their products. For example, a vendor of pc-board layout tools may have to choose between adding yet another display driver or improving its automatic router.

Microsoft’s Windows 3.0 solves DOS’s display-driver and memory-scarcity problems, so application developers can work on the application instead of wasting time and effort on the PC’s hardware needs. Windows manages the PC’s display—no matter what display-adapter card you have—and presents a unified display interface to the application software. It does the same for printers and mice. Further, Windows frees application programs from DOS’s 640-kbyte barrier. In fact, engineering-software vendors cite these features as the main reasons for adopting Windows 3.0. Table 1 lists a healthy sample of Windows-based engineering software already on the market. Many more such products are on the way.

Some stalwart holdouts (both users and vendors) have put off the switch to Windows claiming that graphical user interfaces (GUIs) are for sissies and that DOS-based applications run faster. In truth, Windows does ask more from the PC, and lower-performance machines will bog down to the point where they’re unusable. However, PCs based on 80386 and 80486 µPs—the type most often used for scientific and engineering applications—have little trouble running Windows. PC hardware advances, which seem to occur on a daily basis, make Windows’ performance less of a problem as time passes.

In effect, Windows 3.0 uncouples PC hardware and software. If a PC-hardware vendor develops a faster display adapter or builds a higher-resolution display, Windows can adapt without requiring changes in the application software. The only new software you’ll need is a Windows display driver, and the display vendor—the appropriate party—becomes responsible for developing that code. The same fortuitous situation exists for printer manufacturers. Software vendors cite this feature, above all others, as the main reason for switching to writing Windows applications.

The second most popular reason for switching is Windows’ ability to make more than 640 kbytes of memory available to an application program. Some programs, such as Deutsch Research’s Spicewindows Professional, simply cannot run in 640 kbytes. Prior to Windows, the only remedy for this lack of memory was third-party DOS extenders, which have several drawbacks: They’re not standardized, they cost the vendor and the user extra money for each application program, and they can cause compatibility problems for other DOS programs.

Windows lets application programs use more memory than the PC has RAM by implementing a simulated form of virtual memory that spoils parts of programs to disk when the PC runs out of RAM. But unlike true virtual-memory systems such as Unix, Windows requires the software developer’s cooperation to pull this trick off successfully.

Similarly, Windows provides a form of multitasking called “cooperative multitasking” that also works only if the application code cooperates. (For more information about developing Windows-based applications, see box, “Hints from veteran Windows application developers.”)

Even if graphics standards and memory management were all that Windows offered, many engineering-software vendors would still adopt the GUI because...
“Windows has got to be the future of ECAD on the PC.”—Jeff Deutsch, president, Deutsch Research

of its popularity with PC users. However, Windows now has several additional features that make the PC a far better candidate for engineering applications than ever before. One such feature is the built-in, context-sensitive help system. This system is rapidly replacing paper user manuals because it is more convenient to use and serves the user better than a book.

Altera is one vendor that cites this advantage to writing Windows programs. The company’s Max+Plus II PLD development system includes 3 Mbytes of on-line help information. Tim Southgate, software development manager at Altera, says that context-sensitive help isn’t a radical idea for Windows applications, but it is radical for CAD tools. Altera’s help system lets you click on a displayed object and immediately find out what it does and how to use it.

Mathsoft used Windows’ help system in its Mathcad technical computation package and was even able to extend the concept. Using the Windows help system, the company created electronic handbooks that let you cut standard formulas from the handbook and paste them into your Mathcad document. These formulas are not just text representations, they’re “live.” You can feed constants and variables to them, and they’ll compute results.

Mathsoft’s use of the help system demonstrates Windows’ ability to link the operation of different applications. Software developers can use these intertask communications channels to pass information between applications. Programs. In addition to the help system, Windows provides for intertask communications through three other means: the Windows clipboard, a facility called dynamic data exchange (DDE), and shared memory in dynamic link libraries (DLLs).

The Windows clipboard lets you cut an object from one window and paste it into another with blissful disregard of the operation’s machinations. Depending on the application program, you can transfer a bit map, a block of text, a scalable representation called a Windows metafile, or all three representations to the clipboard. Altera’s Max+Plus II, for example, can transfer all three object types.

<table>
<thead>
<tr>
<th>Vendor</th>
<th>Product name</th>
<th>Product description or use</th>
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</tr>
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<td>Altera Corp</td>
<td>Max+Plus II</td>
<td>PLD development system</td>
<td>$9995</td>
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<td>Design verification</td>
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<td>Waveform Tool</td>
<td>Simulation interface</td>
<td>$695 to $1995</td>
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<td>Chronology Corp</td>
<td>Timing Designer</td>
<td>Timing-diagram entry</td>
<td>$995</td>
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<td>Data Translation</td>
<td>Global Lab Image</td>
<td>Image analysis</td>
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<td>DS-Carte</td>
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<td>Fr 8000</td>
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<td>Start-CAD</td>
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<td>Fr 4900</td>
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<td>Spicewindows Professional</td>
<td>Analog simulation</td>
<td>$2295</td>
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<td>Smash</td>
<td>Mixed analog and digital simulation</td>
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<td>Interactive Curve Display</td>
<td>Visual analysis of Spice output files</td>
<td>$295</td>
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<td>Draf ix Windows CAD</td>
<td>Mechanical CAD</td>
<td>$695</td>
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<td>HP 4990A Proview</td>
<td>LAN-protocol analysis</td>
<td>$5000</td>
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<td>Hyperception Inc</td>
<td>Hypersignal-Windows</td>
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<td>$795 to $2995</td>
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<td>Laboratory Technologies Corp</td>
<td>Labtech Notebook for Windows</td>
<td>Laboratory data acquisition</td>
<td>$1495</td>
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<tr>
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<td>Objectmaker</td>
<td>CASE for Ada, C, and C++</td>
<td>$8000</td>
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<td>Mathcad</td>
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<td>Schematics</td>
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<td>V-System/Windows</td>
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<td>$1495</td>
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<tr>
<td>NCI</td>
<td>PA480485</td>
<td>25/50-MHz, 48-channel logic analyzer</td>
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<td>System Architect</td>
<td>CASE</td>
<td>$1395 to $1595</td>
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<td>FPGA development system</td>
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<td>Driverlinx</td>
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<td>Simucad Inc</td>
<td>Silos III</td>
<td>Logic and fault simulation</td>
<td>$1200</td>
</tr>
<tr>
<td>Symantec Corp</td>
<td>On Target</td>
<td>Project management</td>
<td>$399</td>
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Notes:
1. The price of Chronology’s Timing Designer software changes to $1495 on October 1, 1991.
2. The price of Microsim’s Schematics software package changes to $1750 on October 1, 1991.
At times, you may want information to move from one application to another without manual intervention. Hyperception's Hypersignal-Windows package illustrates the advantages of this transfer mode. You can set up a simulated system in the product's block-diagram editor and, through DDE, send signals generated by the simulation to a graphical-analysis package for scrutiny. There are other ways to send data from one program to another, but the DDE facility provides a standardized method for performing this function.

Jim Zachman, Hyperception's president, says that DDE will enable software developers and engineers to solve new types of problems.

Quicklogic also uses DDE to carry information between concurrently running programs in its pASIC Toolkit. The PLD compiler and the schematic editor are independent programs that run concurrently, and the two programs need to communicate. The editor sends netlists to the compiler, and the compiler sends back-annotation information to the editor. If an error occurs during compilation, you can click on the error message in the compilation window, and the offending node will be highlighted in the schematic window. Messages to perform these feats flow through the Windows DDE pipeline.

However, DDE doesn't solve all intertask communications problems. DDE creates a conduit between concurrently running application programs, but it doesn't define the format of the information that flows through that conduit. Application-program developers must agree on the data format before DDE can become useful. For programs written by the same vendor, the data-format problem doesn't present much of an obstacle. But until engineering-software vendors band together to create some DDE communications standards, you should not expect Windows programs "with DDE support" to work together unless the vendors explicitly state that the programs can communicate with each other.

Microsoft set a de facto DDE standard for business software with its $495 Excel spreadsheet. Most business applications that "support DDE" actually conform to the Excel protocol. That standard doesn't serve the engineering community's needs well because it concerns itself with only business-type information. Microsoft is in the early stages of developing a higher-level messaging specification called object linking and embedding (OLE), which may move the industry towards a more comprehensive communications protocol.

Bridging the communications gap

Like DDE, Windows DLLs can also ease the burden of communications between different programs. Quicklogic employs DLLs to translate information passed between the program components of its pASIC Toolkit. Rather than reinvent schematic entry, Quicklogic's tool employs the CAD/CAM Group's Schematic Capture Tool for the graphic design of PLDs. Quicklogic's Toolkit generates a netlist from the completed schematic. CAD/CAM's product didn't use the netlist format Quicklogic wanted to use, so Quicklogic linked a

You can perform data acquisition and analysis simultaneously under Windows. Laboratory Technologies' Labtech Notebook for Windows can capture data while a spreadsheet analyzes and presents results.
Hints from veteran Windows application developers

If you haven't written code for a graphical user interface (GUI) before, Windows will probably throw you a few curves. Unlike conventional programming, in which the computer drives the user, GUls are event driven: The user drives the computer. Consequently, your programming style must change. Instead of writing a monolithic piece of linear code that runs from initialization to completion, you must create numerous program modules that wait for appropriate activating events to transpire before executing. Most first-time Windows programmers interviewed for this story cited the need for this shift in perspective. Once you're over this initial hurdle, most programmers say that writing code for Windows is no different from writing other types of programs.

You will have to learn about Windows' idiosyncrasies, however. For example, C programmers are accustomed to using C's malloc function to allocate memory and to obtain a pointer to that memory from the operating system. They then use free to dispose of that memory. Under Windows, you cannot use malloc and free because Windows simulates a virtual memory system. Thus, Windows doesn't hand out absolute memory addresses unless you really need to use that memory.

Name that memory block

To allocate a block of memory, you must first use a Windows function call to get a memory-block "handle," or name. When you want to use that memory, you use a second call to lock the block of memory and obtain a pointer to the locked memory block. Your program should keep the memory pointer only for as long as it plans to actively use the memory. When the program no longer needs that memory, you should free the memory block for other applications' use.

Alternatives to Windows memory-allocation techniques can make programming a lot easier. Chronology found one way to reduce the complexity of Windows memory allocation. The company developed its Windows product, Timing Designer, using a $400 C++ compiler for Windows from Zortech (Woburn, MA, (617) 937-0696, FAX (617) 937-0793). The C++ compiler's new and delete memory-allocation calls replace C's malloc and free functions and mask the complexities of memory management under Windows. Incidentally, Windows limits the total number of memory allocations to 8000 for all active programs. Windows programmers soon learn to independently suballocate 32-kbyte memory blocks within their programs.

Several veteran developers note that C compilers for Windows have a tough time with large programs. Altera's Tim Southgate and Deutsch Research's Jeff Deutsch both say they used compilers running under OS/2 because Windows compilers simply could not accommodate the multimegabyte size of their programs. Deutsch cites the 32-bit addressing capabilities of OS/2 compilers as a real benefit for developing large Windows applications. As an alternative to running compilers under OS/2, Model Technology employed Oxygen, a $99 package from Rational Systems Inc (Natick, MA, (508) 653-6006, FAX (508) 655-2753). Oxygen lets you run OS/2 compilers under Windows.

The Windows user interface also adds a great deal of complexity to your code. "You may need as many as 300 Windows function calls to open a dialog box," says Bill Falk, Quicklogic's interface specialist. Falk overcame the complexity of the Windows user-interface model by adopting XVT (Extensible Virtual Toolkit), a $795 Windows-development product from XVT Software Inc (Boulder, CO, (303) 443-4223, FAX (303) 443-0969). XVT lets you create a dialog box with one call. The package handles both display and printing functions.

Writing code for XVT instead of Windows not only reduces complexity, it makes your program portable. XVT Software offers compatible versions of the product for the Apple Macintosh operating system, OS/2 on the PC, and Unix systems running the X Window system. In fact, the IEEE's P1201.1 standards committee has selected the XVT product specification as the base document from which it will draft a standard application programming interface for portable GUI applications. (This move neatly sidesteps the Motif-vs-Open Look GUI debate that has been raging in the Unix community for almost two years.) Falk says XVT lets you make 90% of your code portable across the four operating environments. According to Falk's tests, you pay a 2% performance penalty for this flexibility.

Windows' display performance is an issue you must deal with. Chronology experimented with rubber-band animation for waveform editing in Timing Designer but found Windows display performance sluggish in that mode. (Note that even workstations running the X Window system have trouble providing speedy user-interface performance. Fast graphics operation seems to be one of the toughest performance problems for any GUI to crack.) The current version of Timing Designer uses a simpler approach to waveform editing, but the code contains a compile-time switch to restore the rubber-band visual effect when PC display performance improves.

Snappy performance is merely
nice for user responsiveness, but real-time products that run under Windows must execute with dispatch to perform their assignments. Because Windows employs "cooperative multitasking" instead of preemptive multitasking, any Windows application program could easily find itself without enough CPU cycles to complete its tasks. A real-time application can also monopolize the PC. This situation ensures that the real-time program completes its duties, but it diminishes Windows' usefulness.

A real-time crash

Even if an application program does take over the PC, Windows doesn't allow "bare-metal programming." You cannot interact directly with the PC's hardware under Windows without crashing the system. For example, you cannot write directly to the PC's screen, and you cannot manipulate the PC's interrupt controller for your own purposes.

Real-time programs often try such maneuvers to meet hard-deadline requirements. Consequently, real-time Windows application programs may simply not be able to meet hard deadlines. Fred Putnam, president of Laboratory Technologies, notes that the initial version of his company's Labtech Notebook for Windows, a real-time data-acquisition package, can't always meet hard deadlines, although the DOS version can.

Putnam also has direct experience creating international versions of Labtech Notebook for Windows. Microsoft offers international versions of Windows 3.0 with appropriate character sets for various countries. Good Windows programming practice places all program text into resource files instead of embedding the text in the program modules. This technique greatly eases converting programs to other languages, says Putnam, because almost all the internationalization effort focuses on translating text in the resource file.

Even if you plan to offer only English versions of your product, you must work carefully on the program's look and feel when writing Windows application programs. Users expect Windows programs to be consistent from one application to the next. Chronology employed a graphics designer to help create Timing Designer's user interface because, as Chronology's president Lawrence E Lewis says, most engineers and programmers lack training in contemporary visual styles or color matching.

Chronology also put together a Windows style guide for its program developers by combining published style guides for OS/2's Presentation Manager, Windows, and Apple's Macintosh. "Existing business packages set the expected operating style for all Windows programs," says Lewis. "Even if you can think of a better way to do things, you should stick with existing de facto standards because that's what Windows users expect," he adds. Lewis says that Microsoft's Excel spreadsheet for Windows sets a lot of those standards. Chronology wasn't afraid to violate this rule, however. Timing Designer's prototype trials indicated that users prefer text information in the product's tool bar instead of the icons Excel uses. Consequently, Timing Designer's tool bar contains no icons.

For early product trials, you may want to use a software prototyping tool to build a mock-up version of your product. Prototype programs incorporating just the user interface can help developers and users alike get a feel for how your product will work in the early development stages. Simucad used this approach to create a user interface for its Silos III simulator. The company employed the $495 CASE:W package from CASEworks (Atlanta, GA, (404) 399-6236, FAX (404) 399-9516) to create the prototype interface. Simucad selected this package because it generates compilable interface code once you are satisfied with your design. You finish your program by adding the code that does the application's real computational work.

Once your application is up and running under Windows, you'll find debugging the program more difficult than debugging programs under DOS. The event-driven nature of Windows applications splits your code into relatively independent modules that you must test individually. The Windows user interface complicates testing because you can't use simple keyboard-macro programs for regression testing as you can with DOS programs. You need a program that records both mouse movements and keystrokes for Windows. None of the developers interviewed could recommend such a program.

Symantec's Dave Richards says debugging Windows applications is difficult because you can't isolate concurrently running programs. Consequently, a runaway application can kill the Windows kernel or step on some other memory location and crash the operating system. That's a tough debugging environment, indeed. In general, most of the Windows programmers interviewed for this article thought that Windows debugging tools are still somewhat immature. "Event-driven debugging is a nightmare," summarizes Quicklogic's Falk.
Windows-based engineering software

translation DLL it wrote to CAD/CAM's tool. One added line to the schematic-capture tool's initialization file creates this link. The DLL converts netlists in CAD/CAM's format to Quicklogic's format.

Translation is a popular use for Windows DLLs among many application developers. Symantec uses more than 30 DLLs to translate text files among word-processor file formats in its $199 Justwrite word-processing package. The word processor loads only the DLLs it needs to satisfy a user request. Thus, using DLLs minimizes the amount of RAM the translation code consumes while retaining a broad ability to handle many file formats. Conversely, Symantec's On Target project-management package doesn't employ DLLs because Dave Richards, the engineering manager for the product, saw no inherent advantages to using DLLs.

Manufacturers of Windows-based engineering software

For more information on Windows-based engineering software packages such as those described in this article, circle the appropriate numbers on the Information Retrieval Service card or use EDN's Express Request service. When you contact any of the following manufacturers directly, please let them know you saw their products in EDN.

Altera Corp
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San Jose, CA 95134
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FAX (408) 245-6924
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CAD/CAM Group
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Cupertino, CA 95014
(408) 725-0204
FAX (408) 725-0207
Circle No. 651

Chronology Corp
2849 152nd Ave NE
Redmond, WA 98052
(206) 869-4227
FAX (206) 869-4229
Circle No. 652

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Marlboro, MA 01752
(508) 481-3700
FAX (508) 481-8620
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Jeff Deutsch, president of Deutsch Research, points out that DLLs help keep the source code of his company's Spicewindows Professional analog simulation package private. Earlier versions of Spice from a variety of vendors embedded the simulation models in the program code, which made adding models quite difficult. By specifying a DLL-based model interface for its simulator, Deutsch Research permits outside model development while still keeping its proprietary application code secure.

Altera's Tim Southgate also finds DLLs useful. He says they're efficient because different programs can share one image of a DLL loaded into memory. Programs that use C runtime libraries, for example, can use this feature to greatly reduce the memory the programs consume. Also, DLLs make a program modular, which reduces the time required to link a program together during development. (Southgate notes that linking a 1.8-Mbyte program using static linking can take an hour. One-hour cycle times can really impede software development.) Altera's Max+ Plus II uses more than 50 DLLs. Further, DLLs make field upgrades easy. A vendor need send out only the new or revised DLL instead of an entirely new program. This ability can significantly reduce media-distribution costs for large programs.

One aspect of Windows software engineering—software vendors don't often mention—is the wealth of Windows-based business software that can cross over to serve engineers. Word processors, spreadsheets, and data-base managers all work as well in the engineering domain as they do in business. You might be surprised at the engineering abilities of some business packages. For example, Winrix is a $495 image-creation and -editing package from Rix Softworks Inc (Irvine, CA, (714) 476-8266, FAX (714) 476-8486). The product performs several 24-bit color image-enhancement operations such as brightness and contrast control, color correction, and sharpening. It can also import and export a wide variety of PC image file formats.

You can easily move data back and forth between engineering packages and business packages through Windows' various forms of intertask communications. Quicklogic employed this Windows feature to create user manuals for its pASIC Toolkit. Bruce Kleinman, then Quicklogic's CAE tools architect and now the company's manager of customer engineering, used the Windows clipboard to transfer display screens from the company's PLD development tools directly into the document files that became the product's user manuals. Kleinman points out that engineering is far more than just design entry. "Engineers also must write documentation, do analysis, and perform tests," he says. Engineering and business applications for Windows support all these tasks.

Major vendors of PC business software have either introduced Windows versions of their flagship packages or are currently developing such products. Vendors of PC-based engineering software products are following suit. Now that Windows has severed the hobbling linkage between advances in PC hardware and software, developers of both product types can devote their full energy to getting every last bit of application performance from their products. Moreover, they can survey the field and find new application problems to overcome instead of worrying about recently introduced graphics cards that now need device drivers. This turn of events will draw even more software developers into the fray and further solidify the PC's position as the top engineering computer.

References

Article Interest Quotient (Circle One)
High 473 Medium 474 Low 475
Finally, engineering software that clears the way to problem solving without programming.

```c
void service_id(int eid)
{
    int stat, byte;
    /*serial poll insted*/
    byte=hpib_spoll(eid);
    if ((byte<0) || (byte==0))
        printf("SRQ Prob\n");
    return;
}
stat=my_read(eid, DVM_
if (stat>0) {
    buffy[stat] = '\0';
    printf("Data from instrumen"
else printf("I/O read error\n");
    return;
}
main()
{
    int busid, stat, MTA, MLA;
    char command[MAXCHARS];
    busid=open("/dev/hpib7", O_RDWR); /* open raw HP-IB*/
    MTA=hpib_bus_status(busid, CURRENT_BUS_ADDRESS) + 64;
    MLA=hpib_bus_status(busid, CURRENT_BUS_ADDRESS) + 32;
    stat = BUTTON_BIT;
    sprintf(command, "KM%02o", stat); /* 2 octal digits */
}
```

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The Power in Telecommunications

How component power is contributing to the future of telecom networks

Of all the developments in the 1990's, advances in telecom technology may well have the most profound impact on our daily lives.

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CIRCLE NO. 126
Techniques let you write general-purpose Spice models

By incorporating flexibility into your Spice models, you'll develop a library of accurate models that you can adapt for many applications, rather than reinventing the wheel every time. An example of such a model is a universal power converter.

David Caldwell, Consultant

Computer simulations can save you valuable time by letting you work out the major bugs in a circuit design before building it in hardware. Unfortunately, if the device models you need aren't readily available, you may not be able to make substantial design improvements before committing to hardware. One way to increase your model library is to build models general enough so you can adapt them to a variety of applications. Such models will save you time in future simulations by eliminating the need to develop new models. Also, over time these reusable models reduce the likelihood of encountering errors.

Creating a universal power-converter model illustrates several techniques for adding flexibility to Spice models. This model simulates the buck, boost, and buck-boost pulse-width-modulated (PWM) topologies; continuous and discontinuous conduction modes; operating-point, large-signal transient, and small-signal frequency-domain analyses; and positive and negative polarities. The model's versatility lets you simulate a wide variety of converters quickly and easily.

You can simulate capabilities with a flexible model that you cannot simulate with specific-case models. For example, the universal power-converter model can simulate multiquadrant converters, such as uninterruptible power supplies and power-factor-correction units. These subsystems require a versatile model because each cycle of processed power (usually 60-Hz line voltage) forces the converters to operate under a variety of conditions. To perform a complete transient simulation, the model must automatically adjust its transfer function to handle all combinations of conduction modes and polarities.

The converter model is a simple power-transfer subcircuit with several enhancements. You can add flexibility to other Spice models by using the same enhancement techniques. These techniques let you transform a specific subcircuit into a versatile analysis tool for a broad spectrum of applications. The techniques include

- Using time averaging to simplify switching networks
- Taking advantage of application similarities

The software listings in this article are available on EDN's computer bulletin board system (BBS). Phone (617) 558-4241 with modem settings 300/1200/2400, B, N, 1. Access freeware SIG and specify DSS/DE/1 followed by (k)eyword search for "MS #215".

EDN September 16, 1991
Writing general-purpose Spice models lets you reuse existing models rather than creating new models for every application.

- Generating external control ports
- Using diode networks to simulate if-then-else conditions
- Performing calculations via dependent sources
- Using internal feedback to realize difficult expressions.

Fig 1 shows a functional power-converter subcircuit. A dc transformer, an ideal device linear down to dc, represents the power transfer between the reference (R) and diode (D) ports and the inductor (L) and diode (D) ports. It transfers energy by translating voltage levels without power losses. By arranging the R, L, and D nodes, you can simulate the various converter topologies, so that the input current satisfies the derived equations.

The transformer has a variable turns ratio, N, which lets the simulator change the transformer's gain as a function of the external voltage at node C1. The simulator adjust the turns ratio through a high-gain feedback network until the resultant current flow from node R to node D is equal to the value the simulator calculates. The simulator performs the math using dependent sources and diode networks.

Spice has difficulty simulating switching networks directly, and calculating transient solutions is time consuming. In power converters, the corner frequency of the LC output filter is much lower than the switching frequency to minimize output-voltage ripple. To observe the response to a sudden load change, you must look at a time frame that is very long compared with the switching period, and Spice's algorithms do not handle the disparity in time constants very well.

You can't perform ac analyses of the subcircuit because Spice generates a linear network based on a single operating point. Switches are either closed or open in the discrete-time model, and neither condition is representative of a switch's average state. You must replace the switching components with a time-averaged model to obtain meaningful results.

The time average is the peak amplitude of the switching waveform multiplied by the duty cycle. Replacing the switching waveform with the time-averaged waveform in Spice costs you the ability to

**Glossary of terms**

**Boost topology**—The PWM power-converter topology in which the magnitude of the output voltage is always greater than that of the input, and the polarities of the two are the same.

**Buck topology**—The PWM power-converter topology in which the magnitude of the output voltage is always less than that of the input, and the polarities of the two are the same.

**Buck-boost topology**—The PWM power-converter topology in which the magnitude of the output voltage can be greater or less than that of the input, and the polarities of the two are opposite, unless an isolation transformer is used.

**Continuous conduction mode**—The mode in which the inductor current never reaches zero.

**Discontinuous conduction mode**—The mode in which the inductor current reaches zero every cycle.

**Duty cycle**—The ratio of the switch on time to the switching period.

**Pulse-width modulation (PWM)**—Duty-cycle variation of a fixed-frequency switching waveform.

**Switch-mode power converter**—A high-efficiency circuit that utilizes pulsating switches and magnetics to transform voltage levels.
see period-to-period transient responses. In return, time-averaging waveforms simplify the circuit, eliminate problems associated with simulating vastly different time constants, and provide accurate results in both the time and frequency domains. Sampling theory states that time averaging waveforms is valid at frequencies as great as half the switching frequency.

To create a time-averaged model in Spice, derive the transfer function for the switching device and generate the Spice-equivalent network to realize the equation. For an explanation of time averaging for the input current of a buck converter in both continuous and discontinuous modes, see box, "Determining the conduction mode."

The dashed box in Fig 1 shows the Spice implementation of a converter power section. The subcircuit is a time-averaged model of a switch-mode power converter. Fig 2 shows models of the three basic PWM power-converter topologies: buck, boost, and buck-boost. Note that all three models contain the same elements but in different configurations. You can derive most power-converter models from this primary set.

All three topologies operate under the same basic

---

**Determining the conduction mode**

The time-averaged value of the input current for both the discontinuous and continuous operational modes is a control parameter for the Spice power-converter model. The three topologies use the same model with rearranged nodes, so the buck-converter subcircuit (Fig 2a in the main text) can illustrate the analysis for all three.

In discontinuous-mode operation, the inductor discharges completely during every cycle. During each cycle the inductor current is zero at some point, and neither the switch nor the diode conducts. The switch pulse width causes the magnitude of the average inductor current to vary and is unaffected by previous cycles. You can characterize discontinuous-mode converters as PWM-controlled current sources because their output voltage is load-dependent.

In continuous-mode operation, the inductor discharges partially every cycle, so either the switch or the diode is always conducting. The output voltage must adjust to balance the volt-second product across the inductor at any given duty cycle. The average inductor current will automatically vary over a number of cycles until it satisfies the load at the resultant output voltage. Because the output voltage of continuous-mode converters is not load-dependent, these converters are modeled as PWM-controlled voltage sources.

A converter regulated to a constant output voltage operates in discontinuous mode at light loads and approaches continuous mode as the load draws more output current. If a simulator solves the current equations for both modes of operation, the value of greater magnitude is the correct one. When the calculated discontinuous current is greater than the calculated continuous current, the load is not heavy enough to push the converter to continuous-mode operation. Therefore, the discontinuous-current value is correct, and you can ignore the continuous-current value.

You can confirm the validity of the conduction-mode equations you derive by comparing these equations to the equations in well-established and proven references, such as Refs 1 and 2.
Diode networks can simulate if-then-else conditions.

principles. Closing the switch causes the inductor to charge. When the switch opens, the inductor kicks back and discharges its stored energy through the diode into the capacitor. The charge storage of the capacitor holds the output voltage steady. A simple way of looking at this operation is that the switch and diode generate a PWM waveform that the inductor and capacitor average.

The time-averaged dc transformer subcircuit shown as the Unicon (universal converter) 4-terminal block in Fig 1 replaces the nonlinear switch and diode of Fig 2. Adding the inductor and capacitor gives the converter the proper dynamic response. Rearranging the power nodes of the model lets you simulate any of the three converter types.

You can obtain even greater model versatility by taking a critical parameter of the circuit, such as C2 in Fig 1, and defining it as a variable whose value you set via a control voltage. This control voltage lets you adjust the characteristics of the circuit and permits more types of analysis. C2 lets you examine the transient response to a control-voltage step in the time domain and measure gain and phase as a function of the control voltage in the frequency domain.

The power-converter model has two control nodes. C1 is a user-accessible node that selects the duty cycle of the simulated switch. Internal control node C2 selects the turns ratio of the dc transformer, which simulates the average voltage across the switch and diode. The internal control node is necessary because the selected duty cycle cannot directly set the transformer’s turns ratio. The relationship between the duty cycle and the turns ratio is different for the discontinuous and continuous conduction modes, so the simulator must mathematically manipulate the model to deter-

Spice convergence

The biggest drawback of flexible Spice models is that they tend to be more complicated than single-application models. Therefore, you may encounter more difficulties in the convergence of the computer algorithms. The universal converter model used with Intusoft’s (San Pedro, CA, (213) 833-0710) IsSpice PC simulation package has successfully analyzed many power supplies. But expecting to never encounter convergence problems is unrealistic.

If convergence problems do arise, the .NODESET command lets you estimate any node voltage and allow the Spice algorithm to use that voltage for the first iteration of its computation. Setting the expected output voltage and duty cycle of the power converter increases the probability of convergence if your initial simulations fail to converge.

You can also aid convergence by using the .OPTIONS command to modify parameters. You can instruct the simulator to increase the number of iterations it can take to find a solution by changing the values of ITL1 and ITL2. You can increase the error tolerance of the program by altering RELTOL (relative tolerance) and ABSTOL (absolute tolerance).

A less sophisticated approach to obtaining convergence is to alter the topology of the circuit without changing the circuit’s function. The power-converter subcircuit of Fig 4 and Listing 1 of the main text is the result of some experimentation. There are several other ways to realize the same transfer function, but the one shown has the best convergence.

One alternate way to arrange the circuit is to switch the voltage and current sources of the dc transformer. Another way to realize the circuit is by setting the input current of the converter with a current source and varying the output voltage until the output power is equal to the input power. Because altering the circuit may be time consuming, you should only attempt such modifications after trying the .NODESET and .OPTIONS commands. Ref 3 discusses more methods to aid Spice convergence.
mine the proper turns ratio given the operating conditions of the converter.

In addition to rectifying circuits, diodes are useful for controlling Spice’s mathematical operations. This diode action is similar to the flow of a software program in which an executed expression is a function of the response to an if-then-else statement.

Diode networks in the power-converter subcircuit determine if the model is operating in the discontinuous or continuous conduction mode. If the simulator calculates the current for both modes of operation, the value of greater magnitude is the correct one. The diode network in Fig 3 models this effect. The left half shows the diode ORing scheme for positive polarity currents; the right half shows the scheme for negative currents. Either of the networks would work alone if you knew the polarity of the current, but both networks are necessary to make a flexible model that can handle currents of either polarity.

By taking the voltage across the load resistor in the positive network (node X) and subtracting the load-resistor voltage of the negative network (node Y), you can find the correct magnitude and polarity of the converter’s input current. If the current is positive, the voltage at node X will be the greater of the calculated currents for both conduction modes, and the simulator sets the voltage at node Y to zero, and the voltage at node Y represents the absolute value of the current. The simulator negates the voltage at node Y when it again calculates the difference between the voltages at nodes X and Y.

The diode network determines the greater of the two voltage magnitudes while retaining the original polarity of the signals. This characteristic means that you can change conduction modes or polarities during a simulation, and the model will automatically modify its transfer function to fit the new operating conditions. Thus, you can use the Spice subcircuit to model and simulate multiquadrant converters such as uninterruptible power supplies and power-factor-correction units.

Note that using diodes to select which expression executes is an approximation that includes the error of the forward voltage drop of the diode. Fortunately, you can minimize this error. Multiplying the signals by a scale factor can ensure that the result is very large compared with the diode drop. You might also reduce the forward voltage of the diode by changing its default parameters. Increasing the value of the saturation current or reducing the emission coefficient will also minimize the approximation error.

Fig 1-The complete Spice universal power-converter model contains four subcircuits, which perform lossless energy transfer, generate the duty cycle, and calculate the reference-diode current and the turns ratio.
tive appearance of the polynomial format, it allows Spice to execute many types of expressions. You can even implement division and other desirable functions that don't appear to fit this format. Spice literature, such as Ref 3, provides examples of many of these functions.

Spice calculates the input current to the power-converter model using polynomial-dependent sources. Although the polynomial format is powerful, Spice doesn't perform some computations easily. Carefully selecting parameters may help circuit generation and simulation run more smoothly.

By using dependent sources and the diode network, the op amp forces the input current of the converter model to equal the reference value that the simulator calculates. Fig 1 illustrates this internal feedback. The op amp multiplies the difference between the measured current and the calculated value by 1,000,000. The simulator uses the result to select the dc-transformer turns ratio. An increase in the turns ratio results in a decrease in the input current; thus, this operation is similar to that of a high-gain op amp with negative feedback.

You can use internal feedback when an expression is difficult to derive or realize in Spice. In the converter model, deriving the turns ratio of the dc transformer as a function of the duty cycle for the discontinuous mode is not trivial. Deriving the input current for both conduction modes is easier. You can use high-gain negative feedback to satisfy the derived equations.

Fig 4 is the complete Spice schematic of the universal power-converter model; Listing 1 is its associated netlist. The model limits the duty cycle to between 1 and 99%, which corresponds to voltage values of 0.01 to 0.99V at control node C. The model also limits the turns ratio of the dc transformer to values greater than 1, which is the value that represents the operational limits of the converter topologies. Scaling factors convert the voltage across the sense resisters to current and amplify voltage signals so that the relative voltage drops across the diodes are negligible.

You can further generalize the model to simulate additional converters by altering one value. Inserting the variable T/2L in the discontinuous-current calculation (EDIS in Listing 1 and Fig 4) tells the subcircuit the switching period and the output inductance value of the converter. Substitute T/2L for 0.02273 in the Spice listing as follows:

EDIS 12 0 POLY(2) 1 3 9 0 0 0 0 0 0 0 0 0 0 T/2L

References

Author's biography
David J Caldwell works as a consultant in the field of analog-circuit design and analysis in Hermosa Beach, CA. He has worked on power and control systems and has been responsible for developing custom hardware in a variety of applications. David has a BSEE from the University of Michigan and an MSEE from the University of Southern California and is a member of the IEEE.

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Phase compensation extends op amp stability and speed

Because most op amps lack provision for altering internal phase compensation, circuit designers often add external compensation to counter the effects of capacitance loading and parasitic capacitance and inductance. External phase compensation also permits the use of lightly compensated, high-speed amplifiers in low-gain circuits.

Jerald Graeme, Burr-Brown Corp

To counter the effects of capacitance loading and parasitic capacitance and inductance, circuit designers can use one of four external phase-compensation methods that suit almost any application. Two of the methods specifically address capacitance loading requirements by controlling the amplifier’s open-loop response. The first method requires empirical component selection, but also offers a unique filtering action. The second method removes much of the empirical selection, but can restrict output voltage range.

The other two methods address any phase compensation requirement by controlling the $1/\beta$ curve of the amplifier feedback. These two methods also offer an opportunity for increased slew rate. The second $1/\beta$ method is especially useful for the voltage-follower configuration. An analysis of differential-input configurations defines which method out of the four is best for your design.

All four methods satisfy the external-phase compensation that a capacitive-load drive commonly requires. As Fig 1 illustrates, capacitive loading degrades frequency stability. Load $C_L$ reacts with the op amp’s open-loop output resistance ($R_o$) to produce an added pole in the feedback path. This pole transforms the amplifier’s open-loop response as illustrated by the unloaded and loaded curves of the plot. Phase shift from the added pole introduces response ringing and can even cause oscillation.

Adding the inverse feedback-factor curve, $1/\beta$, to the open-loop response quantifies this response degradation. The nature of the intercept of this curve with the amplifier’s open-loop gain predicts stability conditions. The difference in the slopes of the two curves relates to the net phase shift in the feedback loop. At the intercept, internal phase compensation limits this slope difference, or rate-of-closure, to preserve stability (Ref 1). For Fig 1, the $1/\beta$ curve has zero slope, and the loop phase-shift depends only on the slope of the amplifier’s open-loop response. In the unloaded case, this response has a single-pole roll off at the intercept with the rate of closure of 20 dB/decade at the intercept. This rate-of-closure predicts a stable 90° phase shift in the loop.

In the loaded case, a second pole at $f_p = 1/2\pi R_s C_L$ alters the amplifier’s open-loop response. The resulting 2-pole, or 40 dB/decade, response slope signals a phase shift that eventually reaches 180°. If the phase shift reaches 180° at or before the intercept with the $1/\beta$ curve, oscillation results. Even if oscillation does not occur, this second pole increases response overshoot and ringing, gain peaking, and bandwidth limiting. The
When driving a capacitive load, you commonly need to add external phase-compensation to the op amp.

Phase margin (the amount of phase shift <180°) predicts the actual response degradation (Ref 2). Typically, a phase margin between 45 and 60° is desired to limit overshoot to 30% and peaking to 3 dB.

For the capacitive-load case of Fig 1, the net phase shift at the intercept is \( \phi_m = 90° + \tan^{-1}(f/f_p) \). Here, the 90° shift results from the first amplifier pole, and \( f_p \) is the frequency of intercept with the 1/\( \beta \) curve. This intercept frequency is also the bandwidth limit of the circuit. At the intercept, the feedback demand for gain and the available amplifier gain cross. Beyond this frequency, there is insufficient amplifier gain for continuance of the full-circuit response.

Graphical analysis provides insight

You can obtain a design equation for \( f_p \) by a graphical analysis of Fig 1's curves. In the unloaded case, the response has a maximum bandwidth defined by the unity-gain crossover frequency \( f_c \). For gains higher than unity, the \( \beta \) factor reduces the maximum bandwidth to the frequency \( \beta f_c \). With capacitance loading, the intercept retreats along the 1/\( \beta \) curve to an intercept frequency, \( f_p \), as shown. You can define this frequency in terms of \( \beta f_c \) and \( f_p \) through a geometric evaluation of the curves. Note that the dashed line indicating \( f_p \) forms right triangles bounded by the 1/\( \beta \) curve and the two open-loop responses. The hypotenuse of the loaded triangle has a 2-pole slope, or twice the slope of the hypotenuse of the unloaded triangle. Thus, the base of the loaded triangle is one-half the length of the base of the unloaded triangle.

Given the logarithmic nature of the frequency axis, this relationship between triangle bases is expressed as \( \log(f_p) - \log(f) = 0.5 \log(\beta f_c) - \log(f) \). Solving this expression for \( f_p \) defines this new bandwidth limit at the geometric mean of \( f_p \) and \( \beta f_c \). And, for Fig 1,

\[
BW = f_p = \sqrt{f_p \beta f_c}
\]

For the specific components of Fig 1, \( R_s = 30 \Omega \), making \( f_p = 530 \text{ kHz} \). Also, \( f_c = 6 \text{ MHz} \), \( \beta = 0.5 \) and the resulting intercept frequency and bandwidth limit is \( f_p = 1.26 \text{ MHz} \). Then, from before, \( \phi_m = 90° + \tan^{-1}(f/f_p) = 157° \). The resulting phase margin is \( \phi_m = 180° - \phi = 23° \), which predicts marginal stability.

Little can be done to restore bandwidth under capacitive loading, although the technique in Fig 3, described later, offers some improvement. More important is the restoration of stable performance, which requires added phase compensation. The most frequently used external-phase compensation permits stable drive of large capacitive loads through the addition of a decoupling resistor and a feedback capacitor. Fig 2 shows this configuration, with \( R_C \) and \( C_C \) providing the phase compensation. In this circuit, \( R_s \) is part of the total gain-setting network and is also integral to the overall phase compensation. For a voltage-follower circuit, you also need \( R_s \) for phase compensation. The circuit shown is a noninverting amplifier, but you can apply the compensation technique to any configuration.

However, using this technique with differential-input connections degrades common-mode rejection, as discussed later with Fig 6.

The Fig 2 phase compensation provides a bypass-feedback loop that takes control of the op-amp feedback at higher frequencies. With this compensation, the response of the primary feedback loop still develops a 2-pole roll off, but this response does not reflect op-amp-feedback conditions. Instead, the bypass-feedback loop retains stable feedback conditions and the response curve is largely unaffected by the capacitive

---

*Fig 1—Capacitive loading of an op amp's output resistance introduces a second pole in the open-loop gain response for a -40 dB/decade slope at the 1/\( \beta \) intercept.*
load. Compensation resistor $R_c$ first isolates the op amp from the effect of $C_L$ and then compensation capacitor $C_c$ bypasses the primary feedback loop.

At first, the addition of $R_c$ would seem to aggravate the problem because it moves the pole created by $C_L$ to an even lower frequency, $f_p'$. Similarly, the addition of $C_c$ causes the $1/\beta$ curve to drop to the unity-gain axis for the maximum possible demand on stability. As shown, the response curve of the primary loop has a well-developed 2-pole response at this curve's intercept with the $1/\beta$ curve. This action suggests poor frequency stability.

However, this response curve only represents the open-loop gain from the op-amp inputs to the circuit output. This curve does not represent the feedback conditions controlling the amplifier at higher frequencies. With two feedback paths, the op amp is controlled by whichever path supplies the feedback current to resistor $R_1$. At low frequencies, the impedance of $C_c$ is large, and the feedback path through $R_c$ and $R_2$ dominates. At high frequencies, $C_c$ prevails and the response curve of the bypass loop is in control at the $1/\beta$ intercept. As a result, the bypass response curve represents the open-loop gain from the op-amp inputs to the op-amp output and not to the overall circuit output.

The amplifier input-to-output response normally provides stable conditions for gain or $1/\beta$ all the way down to unity gain. As shown, the resulting bypass response is almost unaffected by $C_1$, because of the decoupling provided by $R_c$. This response intercepts the $1/\beta$ curve before fully developing a 2-pole roll off and predicts good stability characteristics. In practice, Fig 2's OPA2604 drives the 10,000-pF load with only 12% overshoot and 0.3-dB gain peaking. For audio amplifiers like the OPA2604, this phase compensation permits stable drive of the capacitance of long shielded cables.

**Component selection remains empirical**

The actual choice of $R_c$ and $C_c$ in Fig 2 is complicated by the nature of the op amp's open-loop output impedance. This impedance is not simply resistor $R_o$ as modeled in Fig 2. A typical op amp has an open-loop output resistance in the range of 100Ω to 1 kΩ at dc, but the output impedance drops dramatically to about 10 to 50Ω as frequency increases. At very high frequencies, this impedance may rise again. Also, the output impedance is sensitive to the instantaneous level of the amplifier's output current.

Numerous factors contribute to these effects, making complete modeling of output impedance not generally worthwhile. As a result, circuit analysis only offers a basic guide to selection of $R_c$ and $C_c$, and the final choice is empirical. Note that circuit simulation with op-amp models is limited by this same constraint. Spice op-amp models typically include high- and low-frequency output impedances that are modeled by resistors.

Despite these limitations, guidelines can expedite the initial selection of $R_c$ and $C_c$. First, you choose a value for $R_c$ that is in the range of the op amp's high-frequency output resistance, typically 10 to 50Ω. To determine the high-frequency value of $R_o$, you find frequency $f_p$ from a measured response plot and then $R_c = 1/2\pi f_p C_c$. You should not make $R_c$ arbitrarily large, because the voltage drop across $R_c$ detracts from the output-voltage range. This voltage drop does not introduce a gain error because $R_c$ is enclosed in the primary feedback loop. Larger values of $R_c$ also restrict the bandwidth, which is now limited to $f_p' = 1/2\pi(R_o + R_c)C_c$. Fortunately, even small values of $R_c$ dramatically reduce the phase shift developed across $R_o$ by $C_L$. 

---

**Fig 2—A decoupling resistor, $R_c$, and bypass capacitor, $C_c$, isolate an op amp from the effects of the capacitance load, $C_L$.**
Phase-compensation methods involve the control of the amplifier's open-loop response or the control of the 1Ω curve of the amplifier's feedback loop.

Once R<sub>c</sub> is selected, bench tests complete the phase compensation with the selection of C<sub>c</sub>. A good initial value for C<sub>c</sub> is one that causes the bypass path to take effect around the frequency f<sub>p'</sub>. This choice avoids disturbance to the open-loop gain curve of the bypass loop and places the closed-loop bandwidth limit at f<sub>p'</sub>. For very large capacitive loads, this initial C<sub>c</sub> value is too conservative, but the required bench testing corrects for this. To calculate the initial C<sub>c</sub>, you approximate the f<sub>p'</sub> value by f<sub>p'</sub> = 1/2π(R<sub>0</sub> + R<sub>c</sub>)C<sub>c</sub>, where R<sub>0</sub> equals the high-frequency value of the output impedance. Then, the break frequency of C<sub>c</sub> with the R<sub>c</sub> + R<sub>2</sub> path is set at this f<sub>p'</sub> value. Assuming R<sub>e</sub> = R<sub>0</sub>, the initial compensation capacitance for Fig 2 is

\[
C_c = \frac{(R_0 + R_c)}{R_2}C_L, \quad R_e = R_0.
\]

With this capacitor in place, you adjust its value while observing the circuit's square-wave response. This adjustment is made by tests using the full range of C<sub>L</sub> and load-resistance values expected in the application. Fortunately, the compensated circuit response has a low sensitivity to the resistance and capacitance values. The circuit retains degraded, but stable, response over a 100:1 range around the design center. Thus, 2:1 variations in R<sub>0</sub> due to manufacturing tolerances, do not greatly affect circuit stability. However, you still need bench testing to define the design center.

Compensation also filters noise

The phase compensation of Fig 2 also provides unique filtering that rejects amplifier noise better than most op-amp filter circuits (Ref 3). The op amp amplifies the input-voltage noise by a gain of 1/β = 1 + (R<sub>e</sub>/R<sub>1</sub>) in Fig 2 and in the analogous inverting configuration. To filter out high-frequency noise, it's common practice to bypass R<sub>2</sub> with a capacitor. However, this only removes the R<sub>e</sub>/R<sub>1</sub> portion of the op amp's noise gain. Without R<sub>c</sub> and C<sub>c</sub>, the amplifier's high-frequency noise continues to receive a gain of 1/β = 1 up to the open-loop roll-off of the op amp's gain. This same condition is true for almost any op-amp connection, including active filters. For low-frequency applications, the inadvertently included op-amp noise can dominate noise performance.

In the Fig 2 configuration, the filter formed by R<sub>c</sub> and C<sub>L</sub> interrupts the continuation of a unity noise gain. At higher frequencies, the op amp is still under the control of a unity feedback factor as provided by the C<sub>c</sub> feedback. Thus, amplifier input noise continues to receive a corresponding unity gain at high frequencies. However, this unity gain extends only to the op-amp output. Between this output and the actual circuit output is the lowpass filter of R<sub>c</sub> and C<sub>L</sub>. This filter shunts the high-frequency amplifier noise to ground. For filter applications, C<sub>L</sub> is not incidental and you must add it as an element in the circuit design.

Pole and zero compensate for C<sub>L</sub>

A second external-phase-compensation method removes most of the empirical component selection. However, this method does reduce the output voltage range when significant output currents are supplied. This second method (Fig 3) introduces a paralleled resistor and capacitor in series with the amplifier output, but inside the feedback loop. The result is a pole and zero compensation of a capacitive-loaded amplifier. As illustrated, the circuit is a voltage follower, but this compensation method applies to all op-amp configurations.

With the circuit in Fig 3's compensation, the capacitive load that creates the problem becomes part of the phase compensation solution. As before, load C<sub>L</sub> reacts with the circuit's open-loop output resistance, creating a second response pole. In the uncompensated case, C<sub>L</sub> reacts with R<sub>e</sub> to produce a pole at f<sub>p'</sub>, which compromises frequency stability as described with Fig 1. To restore stability, this pole is first moved back to f<sub>p'</sub> by adding resistor R<sub>c</sub>. The resulting response is free to be redirected anywhere within the bounds of the uncompensated response. Bypassing R<sub>c</sub> with C<sub>c</sub> gradually removes the effect of the lower frequency f<sub>p'</sub> by restoring a 20-dB/decade response slope. This is the response slope at the new f<sub>p'</sub> intercept with the 1/β curve, and stability is improved.

To quantify the improvement and select the compensation components, you need to examine the frequencies of the compensated poles and zeros relative to f<sub>p'</sub>. You can use many pole and zero combinations. Different combinations produce optimum conditions for different op-amp configurations. However, it is desirable to use a systematic approach to select compensating components. Fortunately, circuit stability is rather insensitive to the chosen pole-zero combination, and a single selection method adequately restores phase margin for all configurations.

Phase shift at the compensated intercept is interpreted from the duration of the new 20-dB/decade region. For about 90° of phase margin, you would set this region to span one decade of frequency both before and after f<sub>p'</sub>. Experience shows that the decade after
$f_i'$ is important because secondary poles in this region add even more phase shift. However, the decade before the intercept is unnecessarily restrictive of bandwidth. In practice, the 20-dB/decade span before intercept is reduced to about one-half of a decade of frequency. Given the logarithmic nature of the frequency axis, the one-half decade equates to about a factor of three in frequency.

Fig 3 shows a compensated response that approximates the above conditions. The compensated intercept frequency is set at $f_i' = 3f_i$, which results in a 20-dB/decade response span up to $3f_i$. Thus, above $f_i'$, the reduced response slope covers a frequency range of 9:1 or almost a decade. Before the intercept, this span continues as set by the choice of $f_i$. For one-half decade in this region, you should place the compensation zero at $f_z = f_i' / 3$, which is approximately equal to 0.1$f_i$. The result is a 20-dB/decade span covering a frequency range of about 30:1.

The component selection for the Fig 3 circuit follows from the previously stated conditions and the measurement of $f_i$. Resistor $R_e$ is chosen first through a relationship between frequencies $f_i$ and $f_i'$. These two frequencies are also separated by a 30:1 range as seen from the geometry of the responses. The straight-line extensions of the compensated and uncompensated responses form a parallelogram. Thus, the distance between $f_i$ and $f_i'$ equals that between $3f_i$ and $0.1f_i$—a 30:1 span. To make $f_i' = f_i / 30$, the compensation resistor is set at $R_c = 30R_o$. Note that this setting makes $R_c = 3R_o$, and the resulting phase compensation is insensitive to the actual impedance of $R_o$. Thus, empirical fine tuning of the compensation is no longer necessary.

A drawback of the higher $R_c$ value is reduced output voltage range due to the large voltage drop across this resistor. The high-frequency value of $R_o$ is still approximated by empirical measurement of frequency, $f_i'$. Op-amp data sheets do not always reflect this $R_o$ value, which is determined from the relationship $R_o = \frac{1}{2\pi f_o C_L}$.

Using the selected value of $R_c$, capacitor $C_c$ is defined by the response conditions established for Fig 3. For $f_i' = 0.1f_i = 1/2\pi R_o C_c$, the compensation capacitance is defined by $C_c = 5/\pi R_o f_i$. Frequency $f_i$ is known from the previous expression of $f_i' = f_i / \beta R_c$, where $f_i' = 1/2\pi R_c C_c$, and $f_i$ is the unity-gain crossover frequency of the op amp. For Fig 3 with $R_c = 30R_o$,

$$C_c = \sqrt{0.018C_L / R_o \beta f_i}.$$  

With the resulting phase compensation, the OPA2604 again drives a 10,000-pF load. The resulting overshoot is 18% and gain peaking is 1.3 dB. As with Fig 2, Fig 3's phase compensation retains a degraded but stable response for a 10:1 increase or decrease in the value of the load capacitance, $C_L$. Bandwidth is again set by the intercept of the open-loop gain and the $1/\beta$ curve. As described, this intercept is set at $f_i' = f_i / 3$. As with Fig 1, $f_i = \sqrt{f_i f_i'}$, where $f_i = 1/2\pi R_o C_L$, and the Fig 3 bandwidth is

$$BW = \sqrt{0.18f_i f_i' C_L}.$$  

With the specific components shown, the capacitance loading reduces bandwidth to 600 kHz from the 6 MHz of the unloaded case.

For the voltage-follower example, $1/\beta$ follows the 0 dB or unity-gain axis in Fig 3, but this axis does not generally define the critical intercept. In other op-amp configurations, the $1/\beta$ curve is shifted upward and the
Depending on the circuit, you can use either empirical or analytical component-selection methods.

intercept with this curve defines $f_i$ for the component selection. The $\beta$ factor in the previous equation for $C_c$ automatically adjusts the component selection for this difference in intercept. A second caution with Fig 3 is that the pole-zero compensation results in poor settling time (Ref 4). Where settling time is important, you should use the circuit of Fig 4 or Fig 5 without capacitor $C_c$.

Compensation tailors $1/\beta$

In the previous two circuits, phase compensation is directed toward control of the amplifier’s open-loop response at the $1/\beta$ intercept. The circuits that follow control the $1/\beta$ response itself. Instead of reshaping the open-loop response, these circuits tailor the $1/\beta$ curve to intercept the open-loop response at the point where this response offers good stability, which is accomplished with either negative or positive feedback. The $1/\beta$ phase compensation permits the same capacitive load drive as the previous circuits. In addition, the $1/\beta$ method offers an opportunity for a higher slew rate.

The circuit in Fig 4 alters the feedback factor using negative feedback provided by $R_e$ and $C_c$. This method, shown in Fig 4 as a noninverting-amplifier configuration, also applies to all other op-amp configurations. For the voltage-follower case, resistor $R_2$ is again added as part of the phase compensation. In addition, the Fig 4 phase compensation applies to a 2-pole amplifier response of any origin. The second pole can be the result of capacitive loading, a lightly phase-compensated amplifier, or parasitic effects in a high-frequency amplifier. This versatility is not available for the circuits in Figs 2 and 3. Fig 2 depends on a unity-gain-stable op amp, and Fig 3 requires the load capacitance as part of the phase compensation.

Fig 4's circuit connects the phase-compensation elements between the op-amp inputs to alter the feedback factor without altering the circuit’s closed-loop gain. Elements $R_e$ and $C_c$ are bootstrapped on the input signal $e_i$, and they produce no feedback current in direct response to $e_i$. This signal is impressed only upon $R_1$, where the signal creates a feedback current to produce a corresponding voltage on $R_2$. Thus, $R_1$ and $R_2$ continue to control the closed-loop gain experienced by $e_i$.

The circuit does, however, impress the feedback error signal between the op-amp inputs to alter the feedback factor. Elements $R_e$ and $C_c$ are bootstrapped on the input signal $e_i$, and they produce no feedback current in direct response to $e_i$. This signal is impressed only upon $R_1$, where the signal creates a feedback current to produce a corresponding voltage on $R_2$. Thus, $R_1$ and $R_2$ continue to control the closed-loop gain experienced by $e_i$.

To phase compensate the circuit in Fig 4 for capaci-
tive loading, you first approximate $A_{\text{min}}$ from the specified amplifier output resistance. Resistance $R_0$ forms a pole with $C_L$ at $1/(2\pi R_0 C_L)$, and you choose the compensation to align the $1/\beta$ curve with this pole. The pole nearly always occurs in a region of the amplifier response where the amplifier gain ($A$) is approximately equal to $f_c/f$. Here, $f_c$ is the unity-gain crossover frequency of the op amp. At the intercept frequency $f = f_i$, making $A_{\text{min}} = f/f_i = 2\pi R_0 C_L f_i$.

Next, you choose $C_C$ to ensure that $f_p$ and $f_z$ do not disturb the phase conditions at the intercept chosen above. Making $f_p = 0.1f_i$ sufficiently removes $f_p$ and $f_z$ from the intercept. Then, the phase contributions of $f_p$ and $f_z$ are both fully developed and cancel when the intercept is reached. For $f_p = 0.1f_i$, $C_C = 5/\pi R_0 f_i$. In this case, $f_i$ is the frequency of the intercept and also the frequency at which $A_{\text{min}}$ occurs. For lightly compensated amplifiers, you can read this frequency from the open-loop response curve of the data sheet. In other cases, you determine the value of $f_i$ by measurement.

**Phase compensation has side effects**

The phase compensation for Fig 4's circuit offers access to an increased slew rate but reduces input impedance. A higher slew rate results when you use lightly compensated op amps in low gain applications. Several op amps are available with two phase-compensation options to offer higher slew rate and bandwidth to high-gain applications. One option phase-compensates the amplifier for unity-gain stability and serves all applications. The other option uses lighter phase compensation to avoid restriction of slew rate and bandwidth for gains at or above some value of $A_{\text{min}}$. The circuit in Fig 4's external phase compensation bridges the difference. The higher slew rate normally available to higher gain applications becomes available to lower gains as well.

The key to this speed benefit is the altered $1/\beta$ curve. The Fig 4 circuit applies the faster, lightly compensated version of the amplifier to low-gain applications, with frequency stability restored by the external phase compensation. For the OPA37 shown, the compensation extends the slew rate to $12V/\mu\text{sec}$ from the $2V/\mu\text{sec}$ of the unity-gain-stable OPA27 companion product.

Bandwidth, however, does not similarly enjoy this increase because the elevated $1/\beta$ curve moves the $f_i$ intercept back in frequency. As a result, bandwidth is essentially unchanged from that of the unity-gain-stable version. Settling time is improved with this operation because of the increased slew rate. However, this improvement is counteracted by a long settling tail introduced by $f_i$ and $f_p$. To avoid this tail, caused by the added pole and zero, you can replace $C_C$ by a short circuit. However, removing $C_C$ increases the gain available to the amplifier’s input offset voltage and low-frequency noise.

The circuit's (Fig 4) phase compensation also alters input impedance for noninverting applications. At first, you might expect a very low impedance because the compensation elements connect directly to the circuit input. However, as described earlier, these elements are bootstrapped on the input signal, and no input current flows from them in direct response to $e_i$. Indirectly, $e_i$ creates a signal on $R_e$ and $C_C$ through the gain-error signal between the op-amp inputs. This signal is $e_i/A = A_{CL} e_i/A$, where $A_{CL}$ is the closed-loop gain of the circuit and $A$ is the open-loop gain of the amplifier. The resulting current supplied to the circuit input defines an input impedance of $Z_i = AZ_{CL}/A_{CL}$, where $Z_C = R_C + (1/C_C s)$. Thus, the bootstrapping of $Z_C$ boosts...
One method of phase compensation adds the benefit of a filtering action that can significantly reduce amplifier noise.

The resulting input impedance by the loop gain $A/A_c$. For higher-frequency voltage followers, the input capacitance of Fig 4's amplifier degrades the phase compensation. When used in a voltage-follower circuit, this compensation requires the addition of an $R_2$ resistance in the negative feedback path. This added resistance reacts with the amplifier input capacitance and introduces additional phase shift in the feedback loop. Both the differential and common-mode input capacitances of the amplifier react with this $R_2$ resistance.

The result is another zero in the $1/\beta$ response, causing this response to rise as shown by a dashed line in the Fig 4 plot (Ref 1). The rise signals increased phase shift in the loop at higher frequencies. For wideband amplifiers, this added phase shift significantly degrades stability. For example, consider the 16-MHz OPA637 connected as a follower using the phase compensation of Fig 4. With $R_2 = 2 \, \text{k}\Omega$ and $C_c$ chosen by the previous equation, the circuit develops 65% overshoot and extensive ringing.

Normally, a follower has no $R_2$ resistance in the negative feedback path and totally avoids the effect of the input capacitance. This feedback resistance is removed for follower compensation by using positive, rather than negative, feedback to alter the $1/\beta$ curve (Ref 5). The resulting configuration actually benefits from amplifier input capacitance. Moreover, positive feedback is the only external phase-compensation method available to committed, voltage-follower op amps. The positive-feedback method also works for phase compensation of other noninverting configurations. However, these configurations require an $R_2$ resistance and little advantage remains over Fig 4's method. Also, you should not use the positive feedback approach for differential-input configurations, explained by Fig 6.

The Fig 5 voltage-follower case illustrates positive-feedback phase compensation. In this circuit, compensation elements $R_c$ and $C_c$ again form a feedback voltage divider with $R_2$. However, $R_2$ is no longer in the negative feedback path where it could react adversely with amplifier input capacitance. Instead, the circuit adds a positive feedback path to the normal follower connection. With both negative and positive feedback factors, $\beta_-$ and $\beta_+$, the net feedback of an op amp is the difference between the two feedback factors (Ref 6). For Fig 5, $\beta_- = 1$ and $\beta_+ = R_2/(R_2 + Z_c)$, where $Z_c = R_c + (1/C_c s)$. The result is a net feedback factor of

$$\beta = \frac{1 + R_c C_c s}{1 + (R_c + R_2) C_c s}.$$  

The resulting $1/\beta$ curve, which is much like that of Fig 4, has a pole and zero to lift the $1/\beta$ curve before the intercept. For Fig 5, the zero occurs at $1/2\pi(R_c + R_2)C_c$ and the pole occurs at $1/2\pi R_c C_c$. The bootstrapped phase-compensation elements limit disturbance to closed-loop gain and input impedance. The compensation elements ride on signal $e_i$ because of bootstrap feedback from the amplifier output. Because $e_i$ does not directly develop a signal on these elements, the circuit remains a voltage follower with $e_0 = e_i$. The only signal on these elements results from the gain-error signal between the op-amp inputs. This signal, $e_j/A = e_j/A$, appears across $Z_c = R_c + (1/C_c s)$, resulting in a circuit input current of $e_j/A Z_c$. Thus, the input impedance of Fig 5 is $Z_i = A Z_c$.

Component selection favors $Z_i$ or noise

The choice of the Fig 5 components follows the Fig 4 approach but with an added degree of freedom. The high-frequency value of $1/\beta$, $1 + (R_2/R_c)$, is again chosen for an intercept at the amplifier's minimum stable gain $A_{\text{min}}$. Typically, $A_{\text{min}}$ occurs at the second amplifier re-
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<table>
<thead>
<tr>
<th>Device</th>
<th>µPD17134A</th>
<th>µPD17135A</th>
<th>µPD17136A</th>
<th>µPD17137A</th>
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<tr>
<td>ROM (bits)</td>
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<td>2048 x 16</td>
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<td></td>
</tr>
<tr>
<td>RAM (bits)</td>
<td>112 x 4</td>
<td></td>
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<td></td>
</tr>
<tr>
<td>I/O port</td>
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<td>Analog input</td>
<td>4 channels (usable as port pins)</td>
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<td></td>
<td></td>
</tr>
<tr>
<td>Timer</td>
<td>8-bit timer: 2ch Basic interval timer/Watchdog timer: 1ch</td>
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<tr>
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<td>1 channel (usable as a port pin)</td>
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<td>Stack</td>
<td>5 levels</td>
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<td></td>
<td></td>
</tr>
<tr>
<td>Power-on reset</td>
<td>Provided</td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>System clock</td>
<td>RC oscillation</td>
<td>Ceramic oscillation</td>
<td>RC oscillation</td>
<td>Ceramic oscillation</td>
</tr>
<tr>
<td>Instruction execution time</td>
<td>8µs (2MHz)</td>
<td>2µs (8MHz)</td>
<td>8µs (2MHz)</td>
<td>2µs (8MHz)</td>
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<tr>
<td>Standby function</td>
<td>STOP/HALT</td>
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<td></td>
<td></td>
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<tr>
<td>Power supply</td>
<td>2.7 to 5.5V (5% ±10% when A/D in use)</td>
<td></td>
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<td>Package</td>
<td>26-pin plastic shrink DIP/28-pin plastic SOP</td>
<td></td>
<td></td>
<td></td>
</tr>
</tbody>
</table>

One-time PROM

µPD17P136A
µPD17P137A
µPD17P136A
µPD17P137A

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Phase compensation often involves tradeoffs in performance parameters such as slew rate, input impedance, and bandwidth.

sponse pole as shown. Again, $A_{\text{min}}$ is a specified value for the op amp or often set by capacitance loading at $A_{\text{min}}=2\pi R_2 C_2 f_2$. For Fig 5, $R_2 = R_2/(A_{\text{min}} - 1)$. Next, the pole of the $1/\beta$ response is set a decade below the intercept or $f_\pi = 1/2\pi R_2 C_2 = 0.1 f_\pi$. This setting assures that the $f_\pi$ and $f_\theta$ shown have canceling phase effects when the intercept is reached. Then, $C_2 = 5/\pi R_2 f_\pi$.

The above equations for $R_2$ and $C_2$ define the relative values of the compensation elements. However, the absolute values depend upon first choosing a value for $R_2$. In Fig 4, this resistor is part of the normal feedback network and the resistor value is chosen with other criteria. In Fig 5, however, $R_2$ only serves as a phase compensation element, and you are free to set its resistance value.

The factors now guiding the $R_2$ choice are input impedance and noise. With $Z_1 = A Z_C$, input impedance increases with higher values of $R_2$ and lower values of $C_2$. The previous equations for $R_2$ and $C_2$ show that input impedance increases with increasing $R_2$ values. However, noise also increases because $R_2$ generates a voltage noise of $\sqrt{4KTR_2}$ at the amplifier input. Thus, the choice of the $R_2$ value is a compromise.

With the specific components shown in Fig 5, a compromise $R_2 = 2 \, K\Omega$ results in $R_2 = 500\Omega$ and $C_2 = 200 \, \mu F$. The OPA637 then delivers a slew rate of 135V/$\mu$sec, as compared with the 55V/$\mu$sec available with the unity-gain-compensated OPA627. Resulting overshoot is 16%, as compared with 65% in an equivalent solution from Fig 4. This latter improvement is the result of the difference in effects of amplifier input capacitance. As described with Fig 4, this input capacitance causes the circuit’s $1/\beta$ curve to rise at high frequencies, which increases the loop phase shift. In Fig 5, the opposite effect occurs, and the $1/\beta$ curve declines as a result of amplifier-input capacitance. The amplifier’s common-mode input capacitance declines $R_2$, which rolls off the positive feedback and the $1/\beta$ curve. As indicated by a dashed line, this action reduces, rather than increases, the rate-of-closure of the $1/\beta$ and gain curves.

Where noise is more important than input impedance, you choose $R_2$ so that its noise voltage is only about one-third that of the amplifier input. This one-third factor turns into a one-ninth contribution to overall rms noise. The rms addition of the resistor and amplifier noises first raises each term to the second power. As a result, the resistor noise is essentially negligible. For a resistor noise $\sqrt{4KTR_2}$ equal to one-third the amplifier noise ($e_n$), $R_2$ is set to

$$R_2 = e_n/36K,$$

where $K$ is Boltzman’s constant, or $1.38 \times 10^{-23}$, and $T$ is the temperature in degrees Kelvin, or °C + 273. Under these conditions, the $e_n = 5 - nV/\sqrt{Hz}$ of the OPA637 calls for $R_2 = 500\Omega$. Then, $R_2 = 125\Omega$ and $C_2 = 820 \, \mu F$.

Differential input connections of op amps impose a special restriction on external phase compensation. The benefit realized with differential inputs is common-mode rejection, and phase compensation added to the circuit can degrade this rejection. To retain high common-mode rejection, you must place any added phase-compensation where there is no common-mode swing across the compensation elements.

Fig 6 illustrates this technique with the differential-amplifier connection. Consider a common-mode signal connected to the $e_1$ and $e_2$ inputs. Under balanced conditions, the circuit rejects this signal and produces no signal at the $e_0$ output terminal. However, a common-
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Differential-input connections of op amps impose special restrictions on external phase compensation.

A common-mode signal is present at the op-amp input terminals. The voltage divider formed by $R_a$ and $R_b$ transmits a portion of the $e_2$ signal to the op amp’s noninverting input. This signal is also developed at the inverting input of the amplifier through the feedback control of this input. For the equal-value resistors shown, one-half of any common-mode signal connected to the $e_2$ terminal appears at both amplifier inputs.

These input and output signal conditions are representative of all differential-input connections of op amps. A common-mode signal is transmitted to the op-amp inputs but not to the op-amp output. Any phase compensation elements added between these inputs and the output contain a common-mode signal. The resulting signal current degrades common-mode rejection by introducing a signal imbalance.

For example, if you apply the circuit in Fig 5’s compensation to the circuit in Fig 6, $R_c$ and $C_c$ are connected from the op-amp output to the amplifier’s noninverting input. Common-mode swing on these elements then introduces a signal current to the junction of $R_3$ and $R_4$. The effect of this current is not balanced by a matching current at the junction of $R_1$ and $R_2$, and a common-mode error signal results at the circuit output. A similar error develops with application of Fig 2’s external phase compensation.

For differential-input op-amp connections, any external phase compensation added should be of the type illustrated in Fig 3 or Fig 4. With Fig 3’s method, the compensation elements are in series with the amplifier output and do not support a common-mode swing. With Fig 4’s method, demonstrated by the circuit in Fig 6, the only signal across $R_c$ and $C_c$ is the differential error signal between the op-amp inputs. This error signal contains a component of common-mode error but is small compared to the actual common-mode signal.

The resulting signal current in $R_c$ and $C_c$ degrades common-mode rejection, but far less than the compensation methods in Figs 2 and 5. Selection of the $R_c$ and $C_c$ values in Fig 6 follows directly from the discussion of Fig 4. Fig 6 also includes $R_3$ and $R_4$, which are not present in Fig 4, but these resistors do not alter the feedback factor. The phase-compensation effects are the same for the two circuits.

References

Author’s biography
Jerald Graeme is the manager of instrumentation components design at Burr-Brown and has been with the company for 25 years. During that time, he has developed numerous linear circuits, including op amps, instrumentation amplifiers, analog multiplexers, V/F converters, and D/A converters. Jerry has a BSEE from the University of Arizona and a MSEE from Stanford University. Leisure-time activities include scuba diving, photography, and woodworking.
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Programmable oscillator runs without μP

Jon Klein
Micro Linear, San Jose, CA

The circuit in Fig 1, using a clever scheme adaptable to other programmable devices, allows you to operate the ML2035 programmable sine-wave generator, IC3, without a controlling μP. IC1, a 74HC4060 counter, provides both the sine-wave generator’s clock as well as a gating pulse to shift register IC2. When IC1’s pin 5, Q5, goes high, IC2 begins shifting eight hard-wired bits into the sine-wave generator to program it. After IC2 shifts the 8 bits, Q5 goes low, enabling normal operation. The circuit can produce both 50- and 60-Hz outputs from a NTSC color-burst crystal (3.579545 MHz). Table 1 lists binary codes for other crystal frequencies. The sine-wave generator’s output exhibits a maximum of 0.5% THD. EDN BBS/DL_SIG #1019

Table 1—Shift register values and frequency errors for standard crystal values

<table>
<thead>
<tr>
<th>fCRYSTAL (MHz)</th>
<th>fOUT</th>
<th>D10</th>
<th>D6</th>
<th>DHEX</th>
<th>74HC165 Code</th>
<th>Error</th>
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<tr>
<td>4.00</td>
<td>50</td>
<td>105</td>
<td>69</td>
<td>0110</td>
<td>0.14%</td>
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<tr>
<td>4.00</td>
<td>60</td>
<td>126</td>
<td>7E</td>
<td>0111</td>
<td>0.14%</td>
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<tr>
<td>4.194304</td>
<td>50</td>
<td>100</td>
<td>64</td>
<td>1011</td>
<td>0.00%</td>
<td></td>
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<tr>
<td>4.194304</td>
<td>60</td>
<td>120</td>
<td>78</td>
<td>1011</td>
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<td>46</td>
<td>1011</td>
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<td>6.00</td>
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<td>84</td>
<td>54</td>
<td>1011</td>
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<tr>
<td>8.00</td>
<td>50</td>
<td>52</td>
<td>34</td>
<td>1100</td>
<td>-0.82%</td>
<td></td>
</tr>
<tr>
<td>8.00</td>
<td>60</td>
<td>63</td>
<td>3F</td>
<td>1100</td>
<td>0.14%</td>
<td></td>
</tr>
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</table>

To Vote For This Design, Circle No. 746
Slow peripherals interface to fast 68000s

Don Atkins
Motorola, Austin, TX

If you plan to interface slow peripherals to 68000-family μPs, you may have to lengthen the μP's data-hold time during write operations. At faster frequencies, the M68000 family shortens the Address Strobe-Data Strobe (AS-DS) to data-invalid time (ie, the data-hold time) because the clock cycle is shorter. If data from the μP is buffered and the DS signal qualifies the chip-select signal to the peripheral, then worst-case propagation delays may violate the data-hold-time specification of the peripheral. Even fast peripheral devices may be at risk if the propagation-delay skews through the data buffer and the chip-select qualifier is large enough.

Fig 1 shows a sample circuit where the μP interfaces to a write-only hardware register (IC3), a 74LS273 octal D-type flip-flop. Decoded address lines generate a chip-select (CS) signal for IC3, qualified by both the read/write (R/W) and data strobe (DS) signals.

The AS signal qualifies the I/OSEL signal from the address-decode block, connecting to both the 74F245 (IC1) and the 74F164 (IC2). The 74F245 bidirectional data buffer allows the μP to read and write 8-bit peripheral devices. The 74F164 shift register generate the DSACK0 signal, which terminates the bus cycle.

During write operations, the μP transmits data and clocks them into IC3 on the negative edge of the DS signal. The problem with this circuit is that without the components shown connected by dashed lines (and DS hooked directly to the third 74F32), the design violates IC3's 5-ns data-hold time. Calculations show that the hardware provides 0.9 nsec of data-hold time, whereas the 74LS273 requires 5 nsec. An easy fix to this problem would be to substitute a faster D-type flip-flop that requires 0 nsec of data-hold time. This quick fix only provides 0.9 nsec of safety for data-hold.
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*MAR-8, Input/Output Impedance is not 50ohms, see data sheet.

Also, for your design convenience, Mini-Circuits offers chip coupling capacitors at 12 cents each.†

### Table: Amplifier Specifications

<table>
<thead>
<tr>
<th>MODEL</th>
<th>FREQ.</th>
<th>GAIN, dB</th>
<th>MIN. PWR.</th>
<th>NF, dB</th>
<th>PRICE $</th>
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<td>MAR-1</td>
<td>DC-1000</td>
<td>18.5 15.5</td>
<td>13.0</td>
<td>0</td>
<td>5.0 0.99 (100)</td>
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<tr>
<td>MAR-2</td>
<td>DC-2000</td>
<td>13 12.5 11 8.5</td>
<td>+3</td>
<td>6.5 1.50 (25)</td>
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<td>MAR-3</td>
<td>DC-2000</td>
<td>13 12.5 10.5 8.0</td>
<td>+8</td>
<td>6.0 1.70 (25)</td>
<td></td>
</tr>
<tr>
<td>MAR-4</td>
<td>DC-1000</td>
<td>8.2 8.0</td>
<td>7.0</td>
<td>+11</td>
<td>7.0 1.90 (25)</td>
</tr>
<tr>
<td>MAR-5</td>
<td>DC-2000</td>
<td>20 16 11 9</td>
<td>0</td>
<td>2.8 1.29 (25)</td>
<td></td>
</tr>
<tr>
<td>MAR-6</td>
<td>DC-2000</td>
<td>13.5 12.5 10.5 8.5</td>
<td>+3</td>
<td>5.0 1.90 (25)</td>
<td></td>
</tr>
<tr>
<td>MAR-7</td>
<td>DC-1000</td>
<td>33 23</td>
<td>19</td>
<td>+10</td>
<td>3.5 2.20 (25)</td>
</tr>
</tbody>
</table>

**NOTE:** Minimum gain at highest frequency point and over full temperature range.

- 1dB Gain Compression
- +4dBm 1 to 2 GHz

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EDN September 16, 1991

CIRCLE NO. 140 201
DESIGN IDEAS

time and limits the design to a maximum of 33 MHz.

The components connected by dashed lines generate an early data-strobe signal (EDS) to provide longer data-hold times. The EDS signal asserts when DS asserts. The EDS signal then negates during write cycles when the DSACKX signal asserts. This action creates an extra clock cycle of data-hold time. At 33 MHz, the data-hold time increases to 35 nsec.

If you need longer data-hold times, you can use IC2 to negate the EDS signal sooner. Each successively lower-numbered output pin you choose to connect on IC2 retards the EDS signal and increases the data-hold time by one clock period.

Peripherals like the MC68681 Dual Asynchronous Receiver/Transmitter (DUART) and the MC68901 Multi Function Peripheral generate their own data-acknowledge (DTACK) signal. Fig 2 shows how to interface an MC68681 DUART (IC3) to increase the data-hold time from the µP. In this case, an Early-Address Strobe (EAS) qualifies the memory-mapped chip select (CS) signal through a 74F32 2-input OR gate. The output of the 74F32, DUARTCS, then connects to the CSinput of IC3. Like the EDS signal, the EAS signal asserts with the µP's AS and negates during write cycles based on one of the outputs of the 74F164 shift register (IC2). The AS signal qualifies the memory-mapped IOSEL signal from the address decode block to generate the Buffered-Output Enable (BOE) signal used to enable the 74F245 data transceiver (IC1) and to release IC2.

The final major difference between Fig 1's circuit and Fig 2's is a third memory-mapped signal DTACKEN from the address-decode block. The DTACKEN signal asserts whenever a peripheral that generates its own acknowledge signal is selected. This action prevents IC2 from terminating the access until IC3 asserts the DTACK signal. If the µP selects a peripheral that does not generate its own DTACK signal, then the DTACKEN signal does not assert. This sequence allows IC2 to start shifting data immediately and terminate the access by asserting the DSACK0 signal. EDN BBS/DL_SIG #1021

To Vote For This Design, Circle No. 747

---

**Fig 2**—Similarly to Fig 1, this peripheral-interface circuit allows slower peripherals that develop their own acknowledge signal to interface to fast µP's.
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CIRCLE NO. 141
Design Ideas

Relay has electrically resettable fuse

Sam Ochi  
IXYS Corp, San Jose, CA

Fig 1 shows an intelligent, fully isolated, solid-state ac relay, having a resettable 10A electronic fuse. The relay can switch 6 kW (600V ac at 10A). A 5V signal from either a system controller or a manual switch applied to V_IN turns the relay on. Within 1 µsec of sensing a short circuit or an overload, the relay will shut itself off, turn on LED D1, and set flag FLT. Under system control, this solid-state relay can complete an on/off cycle in less than 1 µsec at repetition rates as high as 50 kHz. Such cycling proves useful for starting highly inductive loads.

A 5V signal applied to V_IN enables IC1, a PWM single-phase, de-motor controller, to turn on the relay. Pushing switch S1 or energizing the RST line resets the relay. IC1 drives terminals 3 and 4 of the primary of transformer T2, a communications transformer, through C1 and R1. T2's secondary, terminals 5 and 6, energizes motor controller IC2. C2, C3, and R4 serve to filter any high dV/dt common-mode noise present between the ac power line and IC1's ground.

IC2 converts its received differential signal to a full V_{EE}-to-V_{DD} swing (pin 15). The pin-15 signal drives the series-connected NMOS power transistors, Q1 and Q2, via gate resistors R3 and R4. V_{DD}, which is typically 15V with respect to the sources of Q1 and Q2, is more than enough to turn them on. Conversely, V_{EE}, which is typically -5V, provides a noise margin of 5V to hold the power NMOS devices off in very-high-noise environments.

Once Q1 and Q2 are on, IC2 uses R5 and R6 to sense the currents flowing through Q1 and Q2. During the positive half cycle of the input-ac waveform, Q2 acts as the main switching device, and Q1's internal drain-to-
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source diode conducts. The voltage across the current-sense resistor (R5) is positive with respect to the floating common ground point, FGND, the intersection of R5 and R6.

When more than 10A flows through Q1 and Q2, a positive 1V or more appears across R6 that will forward bias D2 and drop the remaining voltage across R7 and Rs. About 200 nsec after 300 mV or greater potential appears across Rs, IC2’s output, OUT, will go to VEE from VDD. IC2’s T+ (pin 5) and T- (pin 6) outputs will transmit a fault signal. R9 and C4 communicate the fault signal through T2 to IC1’s R- (pin 6) and R+ (pin 7).

When IC1 receives a fault signal, it sets latch IC3, disabling the relay’s input and lighting LED D1. The circuit’s operation during negative ac-power swings is similar. You can reset the relay manually with switch S1 or via input RST.

Transformer T1 and associated circuitry provide the fully floating VDD power for IC2. IC1’s charge-pump clock drives power-transfer transformer T1. T1 is a ferrite toroid (Fair-rite part #5975000201) transformer that is segment wound using 10 turns of #30 Kynar for the primary and 22 turns of #30 Kynar for the secondary. This transformer has 2500V input-to-output isolation. Also, you can obtain this transformer from PSC Electronics part #PSC-5061.

T2 is two ferrite-bead transformers in one encapsulated 8-pin DIP. One source of this transformer is Delta Electronics part #BD4414/15. Of course, you can purchase the ferrite beads from Fair-rite (Fair-rite part #2664000101) and wind 6 turns of #36 magnet wire for the primary and two turns of #30 wire with Kynar insulation for the secondary.

Temperature sensor produces pulse train

Jhoti Vandana
SEMP, Kalpakkam, India

The circuit in Fig 1a converts the current output of the AD590/592 temperature sensor, IC1, into a pulse train. The sensor measures temperatures from -55°C to +150°C. The width of interval T1 (Fig 1b) varies inversely with temperature. The time constant R1C1 sets interval T2. Because T2 can vary with power-supply fluctuations, make sure your supply is well regulated. Also, you must use low-leakage diodes to preserve IC2’s accuracy.

To Vote For This Design, Circle No. 748
How single-chip fuzzy logic can move your product to the head of its class

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Op amp works as clamp

Greg Schaffer  
**Maxim Integrated Products, Sunnyvale, CA**

Forget about amplifying. Instead, think of an op amp as a clamp. The input-protection diodes of a precision op amp can serve as clamping diodes for two independent analog-signal lines (Fig 1). When not clamping, the device’s diodes offer extremely low leakage currents of 50 to 100 fA at 20°C. Maximum clamping current is ±10 mA. **Table 1** lists the clamping diodes’ forward voltage versus forward current.

Clamping voltages \( V_1 \) and \( -V_2 \) connect to the supply terminals of the low-voltage CMOS op amp. You can set these clamping voltages at any level between zero and the op amp’s absolute-maximum supply voltage (12V total), provided \( V_1 \) is more positive than \( -V_2 \). With 10V across the supply pins, the amplifier draws less than 50 µA typ. If pin 3 remains positive with respect to pin 2, the typical supply current is less than 1 µA. Leakage approximately doubles for each 8°C rise in temperature. **EDN BBS/DL_SIG #1017**

To Vote For This Design, Circle No. 750

**Table 1—Diode forward voltage vs current**

<table>
<thead>
<tr>
<th>Diode current (mA)</th>
<th>Diode voltage ( V )</th>
<th>Diode current (mA)</th>
<th>Diode voltage ( V )</th>
</tr>
</thead>
<tbody>
<tr>
<td>0.01</td>
<td>0.635</td>
<td>-0.01</td>
<td>-0.608</td>
</tr>
<tr>
<td>0.10</td>
<td>0.714</td>
<td>-0.10</td>
<td>-0.670</td>
</tr>
<tr>
<td>1.00</td>
<td>0.822</td>
<td>-1.00</td>
<td>-0.751</td>
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<tr>
<td>2.00</td>
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<td>-0.787</td>
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<tr>
<td>5.00</td>
<td>0.921</td>
<td>-5.00</td>
<td>-0.850</td>
</tr>
<tr>
<td>10.00</td>
<td>0.980</td>
<td>-10.00</td>
<td>-0.931</td>
</tr>
</tbody>
</table>

**Fig 1**—This circuit takes advantage of the low-leakage input diodes of a precision CMOS op amp, using them to clamp two analog-signal lines.
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CIRCLE NO. 147
EDN September 16, 1991
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- Has adjustable operating parameters

The AD7774 multichannel I/O device is specifically designed for closed-loop motion control and servo systems. The device includes a 4-channel, 8-bit A/D converter (sharing two track/hold amplifiers), two 8-bit and one 11-bit D/A converters, analog output amplifiers, an internal reference, and a microprocessor interface. The I/O device allows either independent or simultaneous sampling of inputs. Three key operating parameters are independently adjustable: the mid-point of the ADC's transfer function (bias), the input voltage swing of the ADC (span), and the mid-point output voltage of the DAC (bias). By adjusting these biases and the span, you can optimize the performance of the converters—especially in applications where only a positive supply rail is available—by referencing the input and output voltages to a point other than analog ground. The AD7774 operates from 5 and 12V supplies. In 28-pin DIP and plastic-leaded-chip-carrier packages, from $18 (1000).

Analog Devices, 181 Ballardvale St, Wilmington, MA 01887. Phone (617) 937-1428. Circle No. 380

Encoder For TV And VCR Computer Graphics

- Accepts seven digital formats
- Generates NTSC or PAL analog signals

The SAA7199 digital video encoder enables high-quality computer graphics and digital video to be displayed on TV monitors or stored on video tape. The encoder allows personal computers and workstations to perform the same display, editing, titling, and special-effects functions that normally require expensive analog editing boards and systems. The encoder accepts seven different digital formats including CCIR601 (a common digital data structure for NTSC, PAL and SECAM) or computer graphics such as 24-bit RGB or 8-bit VGA. The encoder generates analog output signals in both NTSC and PAL formats. Three user-selectable modes are available. In the master mode, the SAA7199 accepts timing information from the graphics system; in the stand-alone mode, it generates graphics timing signals based on a provided video clock; in the genlock mode, it locks to an analog video signal and generates all graphics timing signals. The genlock mode allows graphics overlay on any video source. $47 (100).

Signetics Co, Box 3409, Sunnyvale, CA 94088. Phone (408) 991-4577. Circle No. 381

Floppy-Disk Controller

- Supports 4-Myebyte drives
- Pin-compatible with standard devices

The FDC37C65C+ floppy-disk controller supports all drive formats including 360-kbyte, 1.2-Mbyte, and the new 4-Mbyte format used in "super-floppy" drives. The C+ controller offers the same features as the industry-standard FDC37C65C floppy-disk controller, with additional support for 4-Mbyte floppy disks. The + designation represents the addition of a 16-byte FIFO and a vertical recording format. The pinout remains the same, which significantly reduces development time and expense when replacing the earlier device. The support for vertical-format drives is enabled by addressing the mode-control register. The FDC37C65C+ controller operates from a

EDN September 16, 1991
single 5V supply and is 100% compatible with IBM software. $6.31 (50,000).

Standard Microsystems Corp. Component Products Div, 35 Marcus Blvd., Hauppauge, NY 11788. Phone (516) 273-3100. Circle No. 382

Real-Time Clock
- Includes on-chip static RAM
- Available as a complete module
The MCCS146818B real-time clock includes 128 bytes of low-power static RAM and features a timing system that lets you use the device with either Motorola or Intel microprocessor timing cycles. The CMOS device includes all the common battery-backup functions, such as a complete time-of-day clock with a 12- or 24-hour mode, a daylight-savings-time option, an alarm with a programmable interrupt, and a 100-year calendar with leap-year compensation. The device counts seconds, minutes, hours, days, day of the week, date of the month, and year. A module version, which interfaces with 1-MHz processor buses, includes the CMOS clock, a 32.768-kHz crystal, and a lithium battery. Clock chip, in a 24-pin plastic DIP, $4.65; in a 28-pin plastic leaded chip carrier, $5.03; complete 24-pin module, $8.08.

Motorola Inc, MOS Digital-Analog IC Div, Box 6000, Austin, TX 78762. Phone (800) 521-6274. Circle No. 383

64-Bit Microprocessor
- Operates at 50 MHz
- Features 100-Mflops performance
Designed for use in high-end computing systems, the 64-bit i860-XP microprocessor provides a peak performance rate of 100 Mflops at 50 MHz. Available in both 40- and 50-MHz versions, the CPU maintains full binary compatibility with the first-generation i860-XR. At 50 MHz, the i860-XP offers performance of 20 double-precision Linpack Mflops and can exceed 40 SPECmarks to meet the number-crunching computing needs of scientific and engineering applications. The CPU includes a RISC (reduced-instruction-set computer) integer unit, two pipelined floating-point units, a graphics unit, 16-byte instruction and data caches, and a memory-management unit. An on-chip bus unit supports pipelined

When considering DSP, take
burst transfers of 400 Mbps. Other features include bus-snooping hardware and a cache protocol that maintains cache consistency between multiple XP processors. The i860-XP comes in a 262-pin ceramic pin-grid array. 50- and 40-MHz versions, $699 and $560 (1000), respectively.

Intel Corp, Box 7641, Mount Prospect, IL 60056. Phone (800) 548-4725, or local office. Circle No. 384

12-Bit A/D Converters
- Include S/H circuit
- Have 8.5- and 25-µsec conversion times

Designed to plug into most ADC574 sockets without system modification, the ADS574 and ADS774 are 12-bit successive approximation A/D converters. Both devices feature an internal sample/hold circuit, a 2.5V reference, a clock, a digital interface for microprocessor control, 3-state output drivers, and internal scaling resistors for input ranges of 0 to 10V, 0 to 20V, ±5V, or ±10V. For 12-bit conversion, the ADS574 and ADS774 have a maximum acquisition-and-conversion time of 25 and 8.5 µsec, respectively. Both parts operate from a single 5V supply. Depending on the operating mode, a -12 or -15V supply is optional, but a +12 or +15V supply is not used. Other key specifications are ±1/2-LSB integral nonlinearity, ±3/4-LSB differential nonlinearity, −77-dB THD and 78-dB SFDR (spurious-free dynamic range). The ADS574 and ADS774 are available in 0.3- or 0.6-in.-wide, 28-pin plastic or side-brazed hermetic DIPs, and in 28-pin SOIC packages. From $14.15 (100).

Burr-Brown Corp, Box 11400, Tucson, AZ 85734. Phone (602) 746-1111. FAX (602) 889-1510. TWX 910-952-1111. Circle No. 385

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Spectrum

CIRCLE NO. 148 Putting DSP to work 217
allowing the output to respond correctly to the applied input. The TLE2027 has a unity-gain bandwidth of 15 MHz and a typical voltage gain of 45V/µV with a 2000Ω load. The TL2037, which is a faster, decompensated version of the TLE2027, has a gain-bandwidth product of 80 MHz, a 50° phase margin, and is stable at gains of five or greater. Package options include DIP, SO and metal can. In commercial plastic DIPs, $1.19 (1000).

Texas Instruments Inc, Semiconductor Group (SC-91047), Box 809066, Dallas, TX 75280. Phone (800) 336-5236, ext 700; (214) 995-6611, ext 700. Circle No. 386

Power Converter/Regulator
- Generates ± voltages locally
- Operates over a 3.5 to 15V range

For components such as op amps and comparators that need voltages unavailable from the system power supply, you can use the UC1054 to generate the required voltage locally. A charge-pump device, the UC1054 can generate or regulate positive and negative voltages between 3.5 and 15V, using any supply voltage in that range. The chip provides as much as 100 mA of output with a typical voltage loss of 1.1V over the full range. Typical circuit configurations include a voltage inverter, voltage regulator, and negative or positive voltage doubler. You can configure the device as a voltage regulator by placing a voltage divider between the output and the on-chip 2.5V reference pin. An oscillator pin lets you adjust the 25-kHz frequency of the internal oscillator or to synchronize it with another device. A shutdown feature reduces the quiescent supply current to 100 µA. In 8-pin DIP and SOIC packages, from $2.40 (10,000).

Dallas Semiconductor, 4401 S Beltwood Pkwy, Dallas, TX 75244. Phone (214) 450-0448. Circle No. 388

14-Bit A/D Converter
- Includes S/H amplifier
- Converts at rates to 2 MHz

The ADS-942 14-bit A/D converter uses a subranging architecture to provide high speed and precision. The converter, which features a fast S/H amplifier, can digitize sinusoidal signals to 1 MHz at a 2-MHz sampling rate or step inputs at a 1.3-MHz conversion rate. Functionally complete, the ADC contains an internal clock, 3-state outputs, and an internal 10V reference. The reference can supply 5 mA to
INTEGRATED CIRCUITS

external circuitry. Other key specifications include total harmonic distortion of -85 dB and a S/N ratio of -77 dB. A pin-selectable feature provides analog input signals of 0 to 10V or ±5V. The digital inputs and the 3-state outputs are TTL and CMOS compatible. The ADS942, which comes in a small, 32-pin DIP, operates from 5V and ±15V supplies and consumes 2.9W. From $374 (OEM qty).

Datel, 11 Cabot Blvd, Mansfield, MA 02048. Phone (508) 339-3000. FAX (508) 339-6356. TLX 174388. Circle No. 389

Analog Interface Chip
- Has 25-kHz sampling rate
- Extends voice band to 7600 Hz
For processing signals beyond the 300 to 3000-Hz voice band, the TLC32046 features a user-programmable, analog-input bandpass/low-pass filter having a nominal bandwidth of 300 to 7600 Hz. The maximum sampling rate is 25 kHz. The chip is a complete analog-to-digital and digital-to-analog input/output system that interfaces directly with the TMS320 DSP family. The chip integrates several functions, including 14-bit A/D and D/A converters, a bandpass antialiasing filter, a low-pass output-reconstruction filter, signal conditioning, control, and timing. The device offers three operating modes—telephone, word, and byte—and a selectable (sin X)/X correction for D/A conversion. For flexibility, the device offers programmable sampling rates, filter bandwidths, A/D path gain, and multiplexed analog inputs. The analog input can be single-ended or differential. TLC32046, in a 28-pin DIP or 28-pin quad flatpack, $14.63 (1000).

Texas Instruments Inc, Semiconductor Group (SC-91045), Box 809066, Dallas, TX 75380. Phone (800) 336-5236, ext 700; (214) 955-6611, ext 700. Circle No. 390

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Basic Math Library
- Compiled subroutines callable from HTBasic
- For statistics, signal processing, and numerical analysis

The HTBasic Advanced Math Library is an addition to HTBasic, a PC-based engineering Basic. The library is a collection of fast, compiled subroutines that are callable from HTBasic and that are useful in statistics, data reduction, signal processing, and numerical analysis. It includes routines for probability density functions, curve fitting, FFTs, digital filtering and windowing, built-in waveforms, root finding, Bessel and related functions, and other higher mathematical functions. HTBasic, compatible with HP 9000 Series 200/300 HP BASIC, offers features such as HP-style IEEE 488.2 commands, data acquisition and RS-232C instrument-control statements, complex arithmetic, HP-style graphics, and SCPI compatibility. The library requires use of the DOS 386 version of HTBasic. Library, $400; DOS 386 HTBasic, $925.

User-Interface Software Package
- Simplifies user-interface development
- For test-and-measurement applications

HP Basic Plus software reduces the number of lines of programming code required to create user interfaces on instrument controllers. The software has 29 commands that create graphical objects needed for user-interface development. The graphical objects are dialogue boxes (for error messages, file information, warnings, and other user messages); data displays (bar display, meters, XY displays, and strip charts); text displays, user-input devices (such as sliders, buttons, and string inputs); pull-down and cascading menus; and displays for HP graphics-language (HP-GL) files. The software, which requires use of HP Basic release 6.2, runs on HP Basic workstations such as the HP 9000 Series 300 controllers. It also runs on PCs with either an HP 82300C or HP 82324A measurement coprocessor. HP Basic Plus, $450; HP Basic 6.2, $1050; upgrade, $250. Delivery, eight weeks ARO.

Hewlett-Packard Co, 19310 Pruneridge Ave, Cupertino, CA 95014. Circle No. 361

Process Automation Kit
- Defines and implements automatic process management
- For software-, electronic-, or mechanical-engineering projects

Teamnet is a Unix-based engineering data-management system for tracking product development. It can use any tool that runs on any computer on an NFS-based network without the need to modify or encapsulate the tool. The kit provides the tools necessary to automate the flow of information between work groups, project leaders, and corporate management. Organizations can extend and customize it to meet their needs with reusable process modules. The kit allows automation of processes such as sign-off requests at each release level; it also provides dependency management, tracking components of a product that might be affected by a proposed change. Including 5-day on-site training, $45,000.

Teamone Systems Inc, 710 Lakeway Dr, Sunnyvale, CA 94086. Phone (408) 730-3500. Circle No. 362

TransEra, 3707 N Canyon Rd, Provo, UT 84604. Phone (801) 224-6550 Circle No. 360

Text continued on pg 227
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EDN September 16, 1991
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- Provides layout for high-speed, high-density modules
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Reverse-Engineering Tool For Fortran Programs

- Shows structure of existing programs written in Fortran
- Helps create documentation for previously undocumented code

Teamwork/Fortran Rev graphically reveals the structure of existing Fortran programs, helping engineers understand undocumented code and create new documentation. It automatically generates structured-design charts from Fortran source files; Teamwork/SD, another tool in the supplier's line of CASE products, can display the charts. Users can use a mouse to browse or edit the source code underlying displayed modules, and they can suppress the display of individual modules or entire groups of modules. For example, a user can choose to suppress the display of specific subroutine calls or eliminate all common-block data modules. The product works with many dia-

Text continued on pg 230
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- Increase user productivity in programming and debugging
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Circle No. 354

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- Uses test history to optimize test routines

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Circle No. 355

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- Maintain 1-µsec accuracy

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Text continued on pg 241

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<table>
<thead>
<tr>
<th>Title</th>
<th>Type</th>
</tr>
</thead>
<tbody>
<tr>
<td>SPP/e</td>
<td>PROM monitor debugger &amp; I/O library</td>
</tr>
<tr>
<td>SPP</td>
<td>SPP/e with architecture &amp; cache simulator</td>
</tr>
<tr>
<td>IDT/c</td>
<td>IBM/SUN X-compiler</td>
</tr>
<tr>
<td>C EXECUTIVE</td>
<td>Real time monitor</td>
</tr>
<tr>
<td>ADA</td>
<td>ADA compiler</td>
</tr>
<tr>
<td>VxWorks</td>
<td>Real time o.s.</td>
</tr>
<tr>
<td>RISC/os</td>
<td>UNIX</td>
</tr>
</tbody>
</table>

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tional Aeronautics and Space Administration (NASA) 36 and 2137. The boards keep time with an accuracy of 1 µsec. The AITG-VME-9U is for Sun workstations that use VMEbus I/O boards in the so-called 9U format. The AITG-S is a single-width Sbus card for Sun's SPARCstations. VME device, $2250. Delivery, 30 to 45 days ARO. Sbus device, $2350. Delivery, November 1991.

Odetics Inc, 1515 S Manchester Ave, Anaheim, CA 92802. Phone (714) 774-5000. Circle No. 356

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The HP 8711A RF network analyzer helps you characterize circuit components at high frequencies. The instrument contains a 1-Hz resolution, 300-kHz to 1.3-GHz, swept, synthesized signal source that completes a full-band sweep in 50 msec. The analyzer has a 9-in. CRT display and a dynamic range of 90 dB. The unit has a 3½-in. floppy-disk drive. With an optional interpreter but without a host com-

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• Has 4-pole Butterworth response
• Corner frequency is settable from 170 Hz to 25.6 MHz
The Model 35 is a plug-in board for the vendor's IEEE-488-programmable modular-instrument chassis. The board contains a 4-pole Butterworth active lowpass filter with cutoff frequencies that you can program from 170 Hz to 25.6 MHz with 2½-digit resolution. Below 2.56 MHz, the cutoff frequencies are accurate to ±2%; from 2.56 to 25.6 MHz, accuracy is ±5%. The board offers both dc and ac coupling and has an input amplifier with selectable gains of 1, 10, and 100 ±1%. You can bypass the filter and use the board as an amplifier with 50-MHz bandwidth. The maximum input is ±1.5V pk divided by the gain. $1800. Delivery, six to eight weeks ARO.

Kron-Hite Corp, 255 Bodwell St, Avon, MA 02322. Phone (508) 580-1660. Circle No. 357

Harness the awesome power of TI's TMS320C40 digital signal processor to your AT or compatible computer—the Vortex system board from ASPi is all you need!

The Vortex is particularly well-suited for prototyping and implementing multiprocessor configurations. The six 'C40 communication ports allow direct processor-to-processor communication; almost any number of Vortex Boards can be linked quickly and easily by just plugging them together.

Besides the main TMS320C40 processor, a Vortex Board has a TI TMS320C31 floating-point processor. The 'C31 can be used with the 'C40 for I/O processing or filtering, or for entirely separate functions. This gives the Vortex a total floating-point capacity of 83 MFLOPS.

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- Fast switching speed
- Adjustable turn-on times
- Low profile 6-pin mini-DIP
- Cost efficiency

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### INPUT ELECTRICAL CHARACTERISTICS

<table>
<thead>
<tr>
<th>Part Number</th>
<th>FB00CD</th>
<th>FB00FC</th>
<th>FB00KB</th>
<th>Units</th>
</tr>
</thead>
<tbody>
<tr>
<td>Continuous Input Current (I_{IN})</td>
<td>Min</td>
<td>Max</td>
<td>mA_{DC}</td>
<td></td>
</tr>
<tr>
<td>Input Current (Guaranteed On)</td>
<td>10</td>
<td>50</td>
<td>mA_{DC}</td>
<td></td>
</tr>
<tr>
<td>Input Current (Guaranteed Off)</td>
<td>100</td>
<td>500</td>
<td>µA_{DC}</td>
<td></td>
</tr>
<tr>
<td>Input Voltage Drop at (I_{IN}) = 25mA</td>
<td>2.5</td>
<td>V_{DC}</td>
<td></td>
<td></td>
</tr>
</tbody>
</table>

### OUTPUT ELECTRICAL CHARACTERISTICS

<table>
<thead>
<tr>
<th>Part Number</th>
<th>FB00CD</th>
<th>FB00FC</th>
<th>FB00KB</th>
<th>Units</th>
</tr>
</thead>
<tbody>
<tr>
<td>Bidirectional Load Current (I_{LOAD})</td>
<td>Min</td>
<td>Max</td>
<td>mA_{DC}</td>
<td></td>
</tr>
<tr>
<td>DC Load Current (I_{LOAD})</td>
<td>2.0</td>
<td>5.0</td>
<td>mA_{DC}</td>
<td></td>
</tr>
<tr>
<td>Bidirectional Load Voltage (V_{LOAD})</td>
<td>Min</td>
<td>Max</td>
<td>V_{DC}</td>
<td></td>
</tr>
<tr>
<td>DC Load Voltage (V_{LOAD})</td>
<td>80</td>
<td>180</td>
<td>V_{DC}</td>
<td></td>
</tr>
<tr>
<td>ON-Resistance (R_{ON}) at (I_{LOAD})</td>
<td>Min</td>
<td>Max</td>
<td>Ohms</td>
<td></td>
</tr>
<tr>
<td>Turn-On Time (T_{ON})</td>
<td>800</td>
<td>1800</td>
<td>µs</td>
<td></td>
</tr>
<tr>
<td>Turn-Off Time (T_{OFF})</td>
<td>300</td>
<td>600</td>
<td>µs</td>
<td></td>
</tr>
</tbody>
</table>

**Notes:**
1. A series resistor is required to limit continuous input current to 50mA (peak current can be higher).
2. Rated input current is 25mA for all tests.
3. Loads may be connected to any output terminal.
4. ON resistance shown is for the bidirectional configuration. The DC ON resistance is 1/4 of these values.

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<table>
<thead>
<tr>
<th>Dimensions</th>
<th>Code</th>
<th>Capacitance</th>
<th>Code</th>
<th>Code</th>
</tr>
</thead>
<tbody>
<tr>
<td>NEW T1 ... 1.75x1.75</td>
<td>25</td>
<td>5.8x5.8x1.75</td>
<td>25</td>
<td>5.8x5.8x1.75</td>
</tr>
<tr>
<td>CERAMIC-TYPE T1 ... 1.55x1.55</td>
<td>15</td>
<td>6.8x6.8x1.5</td>
<td>15</td>
<td>6.8x6.8x1.5</td>
</tr>
</tbody>
</table>

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- **Capacitance Change (%)**
- **Temp. Characteristics YSV**
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40-MHz 386 Computer
• Uses AMD's Am386DX µP and a 64-kbyte cache
• Has 4 Mbytes of dynamic RAM and a 220W power supply
The ME 386-40 ISA bus computer uses AMD's 40-MHz Am386DX µP. The base configuration has a 64-kbyte cache, 4 Mbytes of dynamic RAM, a 1.2-Mbyte, 5½-in. floppy-disk drive, a parallel port, two serial ports, a keyboard, and a 220W power supply. The cache is expandable to 256 kbytes, and you can expand the motherboard's memory to 64 Mbytes. The motherboard has a socket for either an Intel 80387 or a Weitek 3167 coprocessor. The computer delivers 9.71 MIPS. The motherboard has six 16-bit and two 8-bit ISA bus expansion slots. You can opt for a hard-disk drive with capacities ranging as high as 750 Mbytes, and you have a choice of a 101-key keyboard or a keyboard with a trackball mouse. Base configuration, $1949; base configuration with an 80-Mbyte, hard-disk drive, 1.44-Mbyte, 3½-in. floppy-disk drive, super VGA color card and monitor, and either DOS 3.3 or 4.01, $2899.

Facsimile Relay
• Digitizes and compresses Group III fax data
• Connects a PBX trunk to a modem's data input port
The FR-100/EM4W facsimile (fax) relay lets you transmit Group III fax data over a data network. The unit digitizes and compresses the analog output signal from a Group III fax machine and produces 9600- or 4800-bps digital data. The unit connects a fax machine or a PBX trunk to the data port of a modem or a multiplexer. To transfer fax data over a data network, you need a fax relay at each end of the link. The relay supports both DTMF and pulse dialing and handles PBX signals type I through V. The relay operates from 110 to 220V ac and consumes 15W max. The unit measures 5.5 x 9.0 x 8.5 in. and weighs 7 lbs. $3640.

Entropic Speech Inc, 10011 N Foothill Blvd, Cupertino, CA 95014. Phone (408) 973-9800. FAX (408) 973-0336. TLX 1561464. Circle No. 375

Pen Recorders
• Display 24 input signals in four colors
• Sequentially scan each channel for 0.1, 0.2, or 0.5 secs
The HR Series of pen recorders measure and record as many as 24 input signals. The recorders display the data in three modes—analogue trends, analog trend with digital printout, and data logger. The units scan each input channel for 0.1, 0.2, and 0.5 sec/channel. They display analog data in four different colors, permitting six channels/color. You can program the units to record the following parameters using LCD displays—year, month, day, minute, recording mode, chart speed, data size, print interval, type of input signal, and measuring range. The recorders can also print a message of as many as 79 characters/line at any location on the chart. A clock and a timer for starting and stopping measurements are also included. The recorders have IEEE-488 or RS-232C ports for computer communications. From $3495.

Soltec Corp, Sol Vista Park, 12977 Arroyo St, San Fernando, CA 91340. Phone (800) 423-2344; (818) 365-0800. FAX (818) 365-7839. Circle No. 376
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<table>
<thead>
<tr>
<th>1GB-plus Disk Drive Comparison Criteria</th>
<th>Maxtor Panther P0-12S</th>
<th>Seagate Wren 7</th>
</tr>
</thead>
<tbody>
<tr>
<td>Capacity (unformatted)</td>
<td>1.2GB</td>
<td>1.2GB</td>
</tr>
<tr>
<td>Seek Time</td>
<td>13ms</td>
<td>15ms</td>
</tr>
<tr>
<td>Track-to-Track</td>
<td>2ms</td>
<td>2.5ms</td>
</tr>
<tr>
<td>Internal Transfer</td>
<td>17.4 to 29.7Mb/s</td>
<td>15-23Mb/s</td>
</tr>
<tr>
<td>Maximum Seek</td>
<td>26ms</td>
<td>34ms</td>
</tr>
</tbody>
</table>

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Sbus Graphics Board

- Drives 1280 x 1024-pixel displays
- Runs on Sun's Open Windows 2.0 software

The GXTRA 1280 single-slot graphics card works with the Sbus in Sun SPARCstations. It drives 1280 x 1024-pixel displays and has a Sun-4 keyboard and mouse port. The board contains an 8-bit-color frame buffer, and it runs on Sun's OpenWindows 2.0 software. Windows executes partially on the board and partially on the host CPU. You can install multiple Sbus boards to service additional users on a single SPARCstation. The board uses a proprietary gate array, which accelerates low-level graphics primitives such as drawing 2-D vectors, solid and stipple fills, and characters. $2250.


80286 Single-Board Computer

- Contains 4 Mbytes of PROM disk emulation
- ISA bus board contains 4 Mbytes of DRAM and two RS-232C ports

The IND-286 single-board-computer (SBC) works with a passive 8-bit ISA bus. The SBC contains a 16-MHz 80C286 µP and features ROM-DOS, an MS-DOS 3.3-compatible, ROM-based, disk-operating system. The board also includes a battery-backed, 4-Mbyte, PROM disk emulator and a watchdog timer. The emulator boots the system and lets you place application software in EPROM or battery-backed static RAM. The board's flash EPROM programmer permits field upgrades. The SBC features as much as 4 Mbytes of dynamic RAM. It has five kinds of ports: two RS-232C; one parallel printer; one keyboard; one floppy disk; and one IDE hard disk. A clock/calendar and a socket for an optional 80C287 coprocessor also comes with the board. Using an embedded BIOS setup utility, you can configure a system and set the clock/calendar. The board consumes 4W. $795.


Ethernet Board

- Installs in Macintosh II and SE/30 computers
- Comes in coax or 10BaseT twisted-pair versions

The Ether DS Ethernet adapter board installs in the direct slot of a Macintosh II or SE/30 computer. A coax version supports thick or thin Ethernet and a twisted-pair version supports 10BaseT Ethernet networks. The board's drivers for Apple's Ethertalk Phase I and Phase II protocols free you from using high-level protocols. Macintosh computers can communicate via AppleTalk, TCP/IP, DECSnet, or other high-level protocols. Network management software, which comes with each board, provides statistics on Ethernet performance and lets you run loop-back diagnostic tests. $395.

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Brushless DC motors provide extended life in demanding applications

These compact 12-24 VDC motors are designed for tape cartridge drives, business machines, medical equipment, pumps/compressors and similar applications. Available in 2.0" and 3.2" diameters with stall torque from 10 to 84 oz-in. Custom shaft and housing and configurations to match your requirements. AMETEK, Lamb Electric Division, 627 Lake Street, Kent, OH 44240. Tel: 216-673-3451; Fax: 216-673-8994. In Europe, Friedrichstrasse 24, 6200 Wiesbaden, Germany. Tel: 611-370031. Fax: 611-370033.
Pressure Transducers
- Designed to handle rugged environments
- Provide gauge or absolute-pressure measurements

The Model 1230 and 1231 pressure transducers feature all 316L stainless steel construction and employ a proprietary technology that isolates the semiconductor sensor from harsh media and environments. Both are available in gauge and absolute-measurement versions in pressure ranges of 5 to 5000 psi. Static pressure-measurement accuracy for standard B grade units equals 0.25%; 0.125% accuracy is available in A grade units. Respective thermal errors from -25 to +82°C are ±2.5 and ±1.25%. Standard versions are available with a choice of constant current or voltage excitation. Output span is a normalized 100 ±2 mV dc, and long-term measurement repeatability equals ±0.02%. A 4-pin, in-line connector provides electrical connections. Model 1230, $75 to $80; Model 1231, $90 to $115.

Foxboro/ICT Inc, 199 Riveroaks Pkwy, San Jose, CA 95134. Phone (408) 946-1010. Circle No. 391

Current Source
- Develops a 4- to 20-mA output
- Has a ±1% accuracy

Model 930 in combination with the MK298 mounting kit can convert a 0 to 10V input into a 4- to 20-mA output. With a different mounting kit, the unit develops a constant output of 0.5 to 500 mA. Converter accuracy equals ±15 of full scale. The response time to a step change in the load of 10 to 100Ω in 100 μsec is 10 μsec max. Typical frequency response with a 100Ω load equals 10 kHz. The converter operates with any supply voltage in the 12 to 32V range and draws 60 mA max at full load. $108. Delivery, stock to six weeks ARO.

Calex Mfg Co Inc, 3355 Vincent Rd, Pleasant Hill, CA 94523. Phone (800) 542-3355; (415) 932-3911. FAX (415) 932-6017. Circle No. 392

Crystal Oscillator
- Features ±55-ppm/V sensitivity
- Has 25-ppm stability

The Model VC-7025 voltage-controlled crystal oscillator (VCXO) features a specified control sensitivity of ±55 ppm/V. Sensitivity val-
ues as high as ±70 ppm/V are attainable. Housed in a 14-pin DIP measuring only 0.31 x 0.52 x 0.82 in., the oscillator has a 25-ppm frequency stability over a 0 to 70°C range and features 5-nsec rise and fall times. Output frequency range for the oscillator spans 2 to 35 MHz. The unit can drive a 10-gate load (TTL or CMOS) and operates from a single 5V supply. Current drain equals 35 mA. Nominal control-voltage level equals 2.5V dc, and control-voltage range spans 0.5 to 4.5V dc. Deviation sensitivity measures ±50 ppm/V typ, and monotonic linearity equals 20% max. Aging characteristic for the oscillator is specified at ±1 ppm/year. $14.50 (1000). Delivery, 8 to 10 weeks ARO.

Raltron Electronics Corp, 2315 NW 107th Ave, Miami, FL 33182. Phone (305) 593-6033. FAX (305) 594-3973. Circle No. 393

High-Power Resistors
- Handle 250W
- Available in 0.1% tolerances

Designed specifically for snubber protection circuits, REG resistors can handle continuous loads of 250W and withstand 2-kW instantaneous pulses. Resistance values range from 1 to 1500, and resistance tolerances of 0.1 to 5% are available. Over a 20 to 60°C range, temperature coefficient of resistance equals 20 ppm/°C max. Isolation and inductance values equal 5000V ac min and 400 nH max, respectively. Resistor construction provides an efficient thermal interface. The Manganin resistive element mounts on a ceramic plate, which then mounts directly to a large copper baseplate. This construction guarantees an internal heat resistance of 0.1° K/W max. From $150.

Isotek Corp, 566 Wilbur Ave, Swansea, MA 02777. Phone (508) 673-2900. FAX (508) 676-0885. Circle No. 394

Cooling Module
- Controls fans or blowers
- Is RS-232C compatible

The CMM cooling management module is a smart control system that accepts temperature, air flow, or other sensor data as inputs. The unit provides failure prediction and
COMPONENTS & POWER SUPPLIES

The module features an embedded microcontroller with PID (peripheral-integral-differential) loops to control fans or blowers. The unit is RS-232C compatible and allows you to perform system upgrades using software. The modules are available with custom I/Os in 5 to 48V versions, and they can control from 6 to 20 fans or blowers. The module can synchronize all fans to avoid “beat” phenomenon, and it can compensate for filter blockages and other user-defined temperature variations. From $150 (100).


Power MOSFETs
- Feature on-chip current limiting
- Protected from shorted load conditions

The MLP1N06CL and MLA1N06CL TMOS power MOSFETs have integrated on-chip current limiting, gate-to-source voltage clamping, and gate-voltage protection. The voltage-clamping capability protects the device against unclamped inductive switching transients and overvoltage stress conditions. This feature provides high immunity to ESD. The devices also self-protect against shorted load conditions by limiting current flow when the gate is fully enhanced. Both units can be driven directly with CMOS or TTL drivers. MLP1N06CL, in a standard TO-220 package, $1.48; MLA1N06CL, in a fully isolated TO-220 package, $1.73 (1000). Delivery, stock to eight weeks ARO.

Motorola Inc, 5005 E McDowell Rd, Phoenix, AZ 85008. Phone (602) 244-3370. FAX (602) 244-4015. Circle No. 396

Futurebus + Backplane
- Conforms to the hard metric specification
- Features 13 slot positions

This 128-bit Futurebus + backplane conforms fully to the P1301 hard metric specifications as well as the P896.2 specification from revision 5.4. The unit has 13 slots positioned on a 30-mm spacing and accepts

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12SU daughter boards. Each slot has 80 pins available for user-specified I/O via a rear connector. Arbitration is implemented as an optional 48-pin connector located at the center of each slot of the backplane. Power distribution is implemented via press-fit connectors rated for 45A. Multiple power and ground planes are provided on the 5 and 2.1V lines to alleviate the problem of ground bounce. $1920. Delivery, four to six weeks ARO.

Bice-Vero Inc, 1000 Sherman Ave, Hamden, CT 06514. Phone (203) 288-8001. FAX (203) 287-0062. Circle No. 397

DC/DC Converters

- Only 0.27 in. high
- Operate to 125°C

MSA Series 5W dc/dc converters are only 0.27 in. high and are rated for full-power operation from -55 to +125°C. The units operate over the full MIL-STD-704 input range of 16 to 40V. Single- and dual-output models are available with 5, 12, 15, ±12, and ±15V options. Dual-output models support unbalanced loading with as much as 90% of the total rated load available from either output. The converters are fully isolated and offer typical line and load regulation as low as 15 mV. Typical output-ripple voltage is 50 mV, input-ripple current is 40 mA p-p, audio-rejection specifications are 50 dB. From $225 (100).

Interpoint Corp, Box 97005, Redmond, WA 98073. Phone (206) 882-3100. Circle No. 399

Digital Panel Meter

- Has an LCD readout
- Features 0.1% accuracy

The Model DPM5035L 3½-digit voltmeter features snap-in installation and a built-in bezel. It has a basic measurement range of ±199.9 mV dc with an accuracy of 0.1% ±1 digit. Power consumption is 2 mW at 9V dc and 1 mW max at 5V dc. A 0.5-in.-high LCD provides the readout. The unit operates from a 5 to 15V power supply and has an input impedance of 10¹⁰Ω min. Decimal-point position is user selectable. The meter operates over a 0 to 50°C range, measures 3.1×1.7×0.95 in., and weighs approximately 1.6 oz. $22.55 (100). Delivery, stock to six weeks ARO.

DI International Inc, 95 E Main St, Huntington, NY 11743. Phone (516) 673-6866. Circle No. 398

Optical Switch

- Has no contact mechanism
- Activates with a 15g force

The EE-SA105 optical switch operates without a contact mechanism, using an infrared LED and phototransistor combination to indicate activation. It activates with a 15g operating force and has a 0.050-in. pretravel. The infrared LED accommodates 50-mA forward current levels and has an output of 0.5 mA min at VCE equals 5V. The switch has a high output when in the rest position; fully activated, the switch has a 200-mA-max dark-current output. LED output intensity degrades only 7.5% after 500 hours of continuous operating time. $0.99 (5000).

Omron Electronics Inc, 1 E Commerce Dr, Schaumburg, IL 60173. Phone (708) 843-7900. Circle No. 400
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Economic Justification

Justifying Bar-Code Data-Collection Systems

This workbook, Economic Justification, details investing in a bar-code data-collection system, using one of three economic-analysis techniques: payback, present value, or rate of return. The 28-pg booklet also presents examples such as time and attendance, labor tracking, work-in-process tracking, shipping and receiving, and warehouse management. Worksheets and formulas round out the publication.

Burr-Brown Corp, Box 11400, Tucson, AZ 11400.
Circle No. 366

Catalog Documents Add-On Products For CAD/CAM

The 1991 Third Party Catalog features the vendor's software. It discusses approximately 200 hardware and software products that complement or extend the uses of the Personal Designer CAD package and the Personal Machinist CAM package. More than 80 third parties—including hardware and software vendors, CAD/CAM users, and CAD/CAM resellers—developed and now offer the products described in the catalog. Included are Application Software for augmenting the company's two software packages in areas such as solid design, parametrics, sheet-metal folding and unfolding, and kinematics; Symbol Libraries for applications ranging from mold design and steel detailing to tool design and welding; Data Management Software for tracking, revision control, and controlling access to engineering documents; Translators for exchanging the software packages' databases with Chrysler, Ford, GM, and other databases; Networking Products, which links more than one of the two software-package systems; Macros and Utilities for time saving and convenience in areas such as text editing, plot spooling, and redefining keyboard and menu lay-

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outs; Training Manuals and Teaching Aids to augment the standard documentation and tutorials; and PC Hardware, which provides graphics boards, plotters, digitizers, and other peripherals.

Computervision, 100 Crosby Dr, Bedford, MA 01730. Circle No. 367

Source Book Covers IBM PC-Related Products
Computer Systems Edition II features more than 800 IBM PC-related products. It describes applications in telecommunications, industrial and education laboratories, factory automation, and process measurement and control industries. The 96-pg publication notes the addition of 20-, 15-, and 10-slot rack and benchtop chassis, 8- and 15-slot chassis with electroluminescent displays, 6-, 10-, and 15-slot OEM card cages, industrial portable and transportable computers, and a universal rack-mount kit. Other additions include an 80486 25-MHz, EISA plug-in CPU card, 19-in. rack accessories, A/D and communications cards, and Labtech Notebook with Iconview.

Industrial Computer Source, 4837 Mercury St, San Diego, CA 92111. Circle No. 368

Support Products For Peripherals And Computers
This catalog offers an array of support products for the company's peripherals and computers. Divided into seven sections, the publication covers serial HP-IB (IEEE-488) converters; IBM PC/AT, PS/2, and 386 interfaces; HP 900 file-transfer packages; HP-IB bus extenders; the Macintosh/HP-IB converter; the parallel/HP-IB converter; and cables and accessories. Block diagrams, specifications, and pricing complete the catalog.

IOtech, 25971 Cannon Rd, Cleveland, OH 44146. Circle No. 369

Comprehensive Handbook Covers MIL-STD-1553 ICs
The 608-pg 1553 Product Handbook describes the vendor's line of monolithic MIL-STD-1553 ICs for high-reliability aerospace and defense markets. A tutorial on MIL-STD-1553 explains how to design systems to meet its requirements. The publication covers the monolithic protocol devices and details monolithic transceivers with block diagrams, features, characteristics, and package pinouts for each product. Application notes, discussions of quality and reliability, ordering information, and the complete text of MIL-STD-1553B round out the handbook.


DMA, Data-Acquisition Fundamentals, And Interrupts
Three application notes examine fundamentals of DMA and data ac-
LITERATURE

acquisition, and programming interrupts. Data Acquisition Fundamentals (Part No. 340019-01) explains the use of PCs such as the IBM PC/XT, PC/AT, PS/2, or Macintosh for laboratory research, industrial control, and test and measurement. It illustrates such elements of data acquisition as transducers, signal conditioning, data acquisition, and analysis hardware and software. Programming Interrupts for Data Acquisition on 80x86-Based Computers (Part No. 340022-01) deals with interrupt programming on computers based on the 80x86 family of µPs that are used on IBM PC/XT, PC/AT, PS/2, and EISA computers. DMA Fundamentals on Various PC Platforms (Part No. 340023-01) shows how DMA is implemented in a typical PC architecture and compares several PC DMA applications.

National Instruments, 6504 Bridge Point Pkwy, Austin, TX 78730. Circle No. 371

Hewlett-Packard, Tektronix, and Fluke. It also highlights factory-new test equipment, including Tektronix oscilloscopes and Fluke DMMs.

RAG Electronics Inc, 21418 Parthenia St, Canoga Park, CA 91304. Circle No. 372

Listing Of Nanosecond Waveform Generators

This 113-pg catalog mentions more than 300 models of nanosecond waveform generators, including ultrahigh-speed pulse generators, impulse generators, monocycle generators, samplers, delay generators, and accessories. Approximately 40% of the models presented are new, and the book provides an enlarged applications-information section.

Avtech Electrosystems Ltd, Box 5120, Station F, Ottawa, ON K2C 3H4, Canada. Circle No. 373

Publication Lists New And Used Test Equipment

This catalog of new and used electronic test equipment provides listings of oscilloscopes, spectrum analyzers, DMMs, power supplies, signal sources, and environmental chambers from manufacturers such as

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Remember when you were in high school and those people came in to talk about careers? You probably saw an airline pilot and a nurse and maybe even an engineer. The engineer spoke briefly about what he did, and you didn't understand very much of it. Then he left, and you never saw him again. Years ago, that was considered volunteering in the schools.

Today volunteer programs are much more sophisticated and much more important. The problems besetting the American educational system are well known—falling test scores, American students ranking far behind foreign students in science and math, and fewer American students going into engineering every year. American schools need to be revitalized, and engineers are being called upon to help.

On February 19th of this year, the two honorary cochairmen of the National Coalition of Engineering Societies for Precollege Mathematics and Science Education met with President George Bush in the Oval Office of the White House. They presented him with a nine-foot scroll that included the signatures of the presidents and executive directors of the 41 national engineering societies that make up the Coalition. At the meeting they announced their goal of recruiting 100,000 volunteer engineers to help in improving math and science education.

No one has attempted a volunteer program on this scale before, and it will require some real effort from the engineers who choose to join it. "We're not interested in having someone come into a school one time and do a Mr. Wizard or a Mr. Math," says Lee DeLorme, the acting executive director of Engineers for Education. "We're asking our volunteers to make a long-term commitment. Commitment is the key to the program."

One of the nagging problems with volunteer programs in the past was that engineers and teachers sometimes didn't coordinate their efforts. The engineers would give demonstrations that had little to do with the course, or, worse yet, try to take on the role of teacher. "I think the focus shouldn't be on teaching," says DeLorme. "Rather, the volunteer should be an added resource for the teacher and the school. The role that the volunteer assumes in the school—tutor or adviser or whatever—should be done, not in a vacuum, but in consultation and agree-
ment with the individual teacher. Once they determine what the school needs and what the engineer can contribute, then they can develop an effective program."

DeLorme says the response to Engineers for Education has been surprisingly quick and very gratifying. During the first three months following the formal announcement of the program at the White House, more than 500 engineers have called the hot line and volunteered.

As Engineers for Education has expanded its working relationship with industry, it has found that many high-tech companies already support various volunteer programs, and many engineers already donate their time to local schools. Hewlett-Packard, for example, is involved in dozens of volunteer programs around the country.

Russ Herrell is an electrical engineer who works in the research and development laboratory at Hewlett-Packard's facility in Fort Collins, CO. He's also the chairman of the steering committee of the Visiting Scientists program, which pairs up a company scientist or engineer with a teacher in one of the local schools. The program was founded in 1983 and has been very popular with both students and teachers.

Herrell says that the program benefits teachers because they see demonstrations that give insights into applications of some of the things they're teaching. "At the high-school level, teachers are aware they're teaching skills—computer skills or engineering skills—but they don't know how they're applied. A little hands-on demonstration of the fruit of the labor usually goes over very well with the students, too. Students are always awed by some of the fancier technologies that we can bring into the classroom to show them," he says.

Engineers who volunteer in schools have an important function that goes beyond giving demonstrations or even teaching. They are also role models for the students. "When I was growing up, an engineer was someone like Steven Douglas on 'My Three Sons.' What did he do? I didn't know," says Herrell. "If you get to a certain age and you don't know anything about a topic, you begin to lose interest in it. You mentally close the door on it. We want to prevent that.

"We actually had one female engineer go into a second-grade class, and a little girl came up to her and said, 'Gee, I don't think I can be an engineer. I'm a girl.' Where did she get that idea? We do a lot of good just by being role models."

Volunteers face problems

There are problems involved in volunteering beyond making sure the engineer is working closely with the teacher and is contributing something meaningful to the class. First among the complaints is that there's never enough time. Business hours aren't the same as school hours, and it's sometimes difficult for engineers to get away in the middle of the day. The situation can be improved if a company has flex time or if it simply gives its engineers the time off they need.

Another problem is the lack of a comprehensive, national plan for improving the schools. Volunteer ing helps bring industry and educat

A student displays a picture he created with a computer after only a few hours of instruction.
and the engineers feel they're getting something out of it, then they must be doing something successfully."

Like Hewlett-Packard, IBM supports many volunteer programs around the country. An unusual one took place at a summer camp in Fairlee, VT, and was funded by the state. Last year three IBM employees taught children eight to thirteen years old how to use a computer. Many of them were the sons and daughters of migrant farm workers and had never seen a computer before. Penny Swank, a systems analyst, was one of the volunteer instructors.

A feeling of accomplishment

"We tried to give the students some confidence with computers," she says. "We provided programs so they could walk out of that room having produced something, whether it was a greeting card or a picture or a banner. The idea was to give them the feeling they could accomplish something using a computer."

The camp took in 80 to 90 children and had a network of 10 computers. Students were given at least one hour of instruction each week, and they could also work with the computers in their spare time. The computer room quickly became one of the most popular places in the camp.

"We had to schedule hours for it to be closed so we wouldn't be totally inundated with kids," says Swank. "There was a lot of work that had to be done to prepare the curriculum from day to day, and we just had to close the room to do that work. In fact, after we put the kids to bed at 10 o'clock, we worked until one or two in the morning getting ready for the next day.

"There's no way to give a child a computer-science education when you only have a few hours. Our goal was to give the children some sort of confidence level with the computer, particularly those who were afraid when they came in. The idea was to give them an opportunity to achieve some sort of success, and I think we did that. It was an excellent program."

Not all stories about volunteer programs have happy endings. Last year the state of Vermont withdrew its funding for the camp. Unless the director can raise money from another source, it will close permanently.

Some professional organizations sponsor volunteer programs. The National Society of Professional Engineers (NSPE), for example, runs MathCounts, a series of competitions between teams of seventh and eighth graders from around the country that culminates in a national championship each May in Washington, DC. The purpose of MathCounts is to build mathematics skills and promote strategic problem solving among students. More than 8000 volunteers from the NSPE donate their time to the program each year as organizers, coaches, and administrators.

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Professional Issues

contests, and a national engineering aptitude search. The aptitude search is a guidance test that helps students evaluate their chances of success if they choose to go to engineering school. JETS has been running these programs for 40 years. Other professional organizations also support precollege educational activities (see box, "You can help").

You don’t have to work for a large high tech firm or belong to a professional organization to help improve our schools, however. You can make a contribution by doing something as simple as attending a meeting of your local school board. You understand what kind of preparation a student needs to succeed in engineering school or in a technical profession. Talk to your school administrators and teachers and make sure that your schools are providing sufficient instruction in science and math. You can help, but first you have to become involved.

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EDN September 16, 1991
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276 EDN September 16, 1991
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• "C" Programming

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• Component Level
• PALS/PLD
• FPGA
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• RFI
• DOS-UNIX-UNIX
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EDN covers new and developing technologies to inform its readers of practical design matters that will be of concern to them at once or in the near future.

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Raytheon
<table>
<thead>
<tr>
<th>ADVERTISERS INDEX</th>
<th>PAGE</th>
</tr>
</thead>
<tbody>
<tr>
<td>Ability Systems Corp</td>
<td>267</td>
</tr>
<tr>
<td>Abbott Electronics</td>
<td>156</td>
</tr>
<tr>
<td>ACCEL Technologies Inc</td>
<td>269</td>
</tr>
<tr>
<td>Actel</td>
<td>255</td>
</tr>
<tr>
<td>Adaptec Products Co</td>
<td>203</td>
</tr>
<tr>
<td>Advanced Micro Devices</td>
<td>10-11, 52-53, 88-89, 212-213</td>
</tr>
<tr>
<td>Advanced Technology Development Inc</td>
<td>250</td>
</tr>
<tr>
<td>Aerospace Optics</td>
<td>79</td>
</tr>
<tr>
<td>Alcatel</td>
<td>125</td>
</tr>
<tr>
<td>Allen Systems</td>
<td>269</td>
</tr>
<tr>
<td>American Arium</td>
<td>209</td>
</tr>
<tr>
<td>American Neurologix</td>
<td>268</td>
</tr>
<tr>
<td>American Reliance</td>
<td>268</td>
</tr>
<tr>
<td>Ametek</td>
<td>250</td>
</tr>
<tr>
<td>AMP</td>
<td>144-145</td>
</tr>
<tr>
<td>Analogic Corp</td>
<td>80</td>
</tr>
<tr>
<td>Ariens</td>
<td>205</td>
</tr>
<tr>
<td>Asahi Kasei Microsystems**</td>
<td>173</td>
</tr>
<tr>
<td>Astec America</td>
<td>211</td>
</tr>
<tr>
<td>AT&amp;T</td>
<td>252-253</td>
</tr>
<tr>
<td>Atlanta Signal Processors Inc</td>
<td>219</td>
</tr>
<tr>
<td>Avocet Systems Inc</td>
<td>272</td>
</tr>
<tr>
<td>AVX Corp</td>
<td>58</td>
</tr>
<tr>
<td>BASF**</td>
<td>26-27</td>
</tr>
<tr>
<td>Belden Wire &amp; Cable</td>
<td>C4</td>
</tr>
<tr>
<td>Biometron</td>
<td>119</td>
</tr>
<tr>
<td>BP Micro</td>
<td>272</td>
</tr>
<tr>
<td>BP Microsystems</td>
<td>68</td>
</tr>
<tr>
<td>Buckeye Stamping Co</td>
<td>265</td>
</tr>
<tr>
<td>Burr-Brown Corp</td>
<td>28, 219</td>
</tr>
<tr>
<td>Bussmann</td>
<td>210</td>
</tr>
<tr>
<td>CAD Software Inc</td>
<td>244</td>
</tr>
<tr>
<td>Cahners CAPS</td>
<td>173</td>
</tr>
<tr>
<td>Capital Equipment Corp</td>
<td>219</td>
</tr>
<tr>
<td>Capilano Computer Systems Inc</td>
<td>268</td>
</tr>
<tr>
<td>C &amp; K Components Inc</td>
<td>246</td>
</tr>
<tr>
<td>Central Semi</td>
<td>269</td>
</tr>
<tr>
<td>Cermetek</td>
<td>269</td>
</tr>
<tr>
<td>Chronology</td>
<td>217</td>
</tr>
<tr>
<td>Cirrus Logic</td>
<td>72</td>
</tr>
<tr>
<td>Comdisco</td>
<td>226</td>
</tr>
<tr>
<td>Communications Specialties Inc</td>
<td>270</td>
</tr>
<tr>
<td>Communication Specialists</td>
<td>271</td>
</tr>
<tr>
<td>Comput Digital</td>
<td>276</td>
</tr>
<tr>
<td>Conner Peripherals</td>
<td>90-91</td>
</tr>
<tr>
<td>Cypress Semiconductor</td>
<td>268</td>
</tr>
<tr>
<td>Dale Electronics Inc</td>
<td>1, 244</td>
</tr>
<tr>
<td>Data I/O Corp</td>
<td>157-172, 271</td>
</tr>
<tr>
<td>Datekey</td>
<td>97</td>
</tr>
<tr>
<td>Dataight</td>
<td>270</td>
</tr>
<tr>
<td>Datel</td>
<td>107</td>
</tr>
<tr>
<td>Deltron Inc*</td>
<td>256A-D</td>
</tr>
<tr>
<td>Design Computation Inc</td>
<td>272</td>
</tr>
<tr>
<td>Dexter Magnetics</td>
<td>264</td>
</tr>
<tr>
<td>Digi-Key</td>
<td>2</td>
</tr>
<tr>
<td>DOS Systems</td>
<td>270</td>
</tr>
<tr>
<td>ECM</td>
<td>260</td>
</tr>
<tr>
<td>Eclipse Computer</td>
<td>268</td>
</tr>
<tr>
<td>EEsof</td>
<td>56</td>
</tr>
<tr>
<td>Elcon</td>
<td>266</td>
</tr>
<tr>
<td>Electronic Measurements Inc</td>
<td>224</td>
</tr>
<tr>
<td>Emulation Technology Inc</td>
<td>42, 269</td>
</tr>
<tr>
<td>EPIX Inc</td>
<td>270</td>
</tr>
<tr>
<td>Ericsson Components</td>
<td>148</td>
</tr>
<tr>
<td>Fujitsu Inc</td>
<td>225</td>
</tr>
<tr>
<td>Fujitsu Microelectronics Inc</td>
<td>24-25</td>
</tr>
<tr>
<td>Futaba Corp of America</td>
<td>229</td>
</tr>
<tr>
<td>GE Plastics</td>
<td>268</td>
</tr>
<tr>
<td>Glassman High Voltage Inc</td>
<td>231</td>
</tr>
<tr>
<td>Grammar Engine Inc</td>
<td>24</td>
</tr>
<tr>
<td>Grayhill Inc</td>
<td>96</td>
</tr>
<tr>
<td>Hamilton Avnet Electronics</td>
<td>234</td>
</tr>
<tr>
<td>Harris Semiconductor</td>
<td>196-198</td>
</tr>
<tr>
<td>Hewlett-Packard Co</td>
<td>16, 48, 54-55, 139</td>
</tr>
<tr>
<td>Hughes Aircraft Co</td>
<td>45</td>
</tr>
<tr>
<td>Huntsville Microsystems Inc</td>
<td>C2</td>
</tr>
<tr>
<td>Hybrids International</td>
<td>272</td>
</tr>
<tr>
<td>Hypertronics Inc</td>
<td>266, 270</td>
</tr>
<tr>
<td>IBI Systems Inc</td>
<td>269</td>
</tr>
<tr>
<td>IBM Corp</td>
<td>146-147</td>
</tr>
<tr>
<td>ICHIA North America</td>
<td>228</td>
</tr>
<tr>
<td>IDT</td>
<td>61</td>
</tr>
<tr>
<td>ILC Data Device Corp</td>
<td>63</td>
</tr>
<tr>
<td>Incredible Tech</td>
<td>266</td>
</tr>
<tr>
<td>Innovative Software Systems</td>
<td>266</td>
</tr>
<tr>
<td>Intel</td>
<td>100-101</td>
</tr>
<tr>
<td>Intermetrics Inc</td>
<td>128, 232</td>
</tr>
<tr>
<td>International Rectifier</td>
<td>143</td>
</tr>
<tr>
<td>iotech Inc</td>
<td>258</td>
</tr>
<tr>
<td>Ironwood Electronics Inc</td>
<td>267, 271</td>
</tr>
<tr>
<td>Jandel Scientific</td>
<td>126, 265</td>
</tr>
<tr>
<td>John Fluke Manufacturing Co Inc*</td>
<td>38, 257</td>
</tr>
<tr>
<td>Ledronics Inc</td>
<td>267</td>
</tr>
<tr>
<td>Linear Technology Corp</td>
<td>196</td>
</tr>
<tr>
<td>Link Computer Graphics Inc</td>
<td>270</td>
</tr>
<tr>
<td>Loughborough Sound Images Ltd**</td>
<td>107</td>
</tr>
<tr>
<td>MathSoft Inc</td>
<td>128, 259</td>
</tr>
<tr>
<td>Maxim Integrated Products</td>
<td>65, 67, 69, 71, 73</td>
</tr>
<tr>
<td>Maxtor</td>
<td>248-249</td>
</tr>
<tr>
<td>MCSI</td>
<td>267</td>
</tr>
<tr>
<td>Mechanical Products</td>
<td>227</td>
</tr>
<tr>
<td>Meritec</td>
<td>267</td>
</tr>
<tr>
<td>MetaLink Corp</td>
<td>271</td>
</tr>
<tr>
<td>Micro/Sys</td>
<td>269</td>
</tr>
<tr>
<td>Microtran Co Inc</td>
<td>285</td>
</tr>
<tr>
<td>Mini-Circuits Laboratories</td>
<td>3, 4, 22-63</td>
</tr>
<tr>
<td>Mitusumi Electronics</td>
<td>250</td>
</tr>
<tr>
<td>Motorola</td>
<td>122-124</td>
</tr>
<tr>
<td>Motorola Semiconductor</td>
<td>Products Inc</td>
</tr>
<tr>
<td>Murrineta Circuits</td>
<td>264</td>
</tr>
<tr>
<td>National Instruments</td>
<td>94, 267</td>
</tr>
<tr>
<td>National Semiconductor Corp*</td>
<td>220-222</td>
</tr>
<tr>
<td>NEC Corp</td>
<td>102, 189, 256</td>
</tr>
<tr>
<td>Needham Electronics</td>
<td>272</td>
</tr>
<tr>
<td>Nichicon Corp</td>
<td>270</td>
</tr>
<tr>
<td>Nicolet</td>
<td>40</td>
</tr>
<tr>
<td>Nohau Corp</td>
<td>227, 265</td>
</tr>
<tr>
<td>OKI Semiconductor</td>
<td>26-27</td>
</tr>
<tr>
<td>Omnibyte Corp*</td>
<td>239-240</td>
</tr>
<tr>
<td>OrCAD Systems Corp</td>
<td>8-9</td>
</tr>
<tr>
<td>Orion Instruments</td>
<td>267</td>
</tr>
<tr>
<td>Otto Controls</td>
<td>230</td>
</tr>
<tr>
<td>Paradigm</td>
<td>121</td>
</tr>
<tr>
<td>P-Cad</td>
<td>84-86</td>
</tr>
<tr>
<td>Pentac Systems</td>
<td>120, 127</td>
</tr>
<tr>
<td>Performance Semiconductor Corp</td>
<td>70</td>
</tr>
<tr>
<td>Philips Components**</td>
<td>81-83</td>
</tr>
<tr>
<td>Pico</td>
<td>218, 251</td>
</tr>
<tr>
<td>Planar Systems</td>
<td>259</td>
</tr>
<tr>
<td>Power Trends Inc</td>
<td>237</td>
</tr>
<tr>
<td>Powertronic</td>
<td>270</td>
</tr>
<tr>
<td>Pulse Engineering</td>
<td>241</td>
</tr>
<tr>
<td>Qau Tech Inc</td>
<td>228</td>
</tr>
<tr>
<td>Raytheon</td>
<td>279</td>
</tr>
<tr>
<td>RC Systems</td>
<td>266</td>
</tr>
<tr>
<td>Real Time Devices</td>
<td>245</td>
</tr>
<tr>
<td>R O Associates Inc</td>
<td>214</td>
</tr>
<tr>
<td>Rogers Corp</td>
<td>272</td>
</tr>
<tr>
<td>Rolyin</td>
<td>265</td>
</tr>
<tr>
<td>Samsung Semiconductor</td>
<td>12-13</td>
</tr>
<tr>
<td>Samtec Inc</td>
<td>254-255, 272</td>
</tr>
<tr>
<td>SBE</td>
<td>180</td>
</tr>
<tr>
<td>Scientific Software</td>
<td>267</td>
</tr>
<tr>
<td>Seagate Technology</td>
<td>41</td>
</tr>
<tr>
<td>Selco Products Inc</td>
<td>271</td>
</tr>
<tr>
<td>SenSys</td>
<td>191</td>
</tr>
<tr>
<td>Sharp Electronics</td>
<td>155</td>
</tr>
<tr>
<td>Siemens Components Inc</td>
<td>74</td>
</tr>
<tr>
<td>Signetics Corp**</td>
<td>82-83</td>
</tr>
<tr>
<td>Silicon Systems Inc</td>
<td>81</td>
</tr>
<tr>
<td>Softaid Inc</td>
<td>269</td>
</tr>
<tr>
<td>Softools</td>
<td>266</td>
</tr>
<tr>
<td>Sony</td>
<td>76</td>
</tr>
<tr>
<td>Spectrum Signal Processing Inc**</td>
<td>216-217</td>
</tr>
<tr>
<td>Spectrum Software</td>
<td>235</td>
</tr>
<tr>
<td>Sprague Goodman</td>
<td>29</td>
</tr>
<tr>
<td>Stanford Research Systems Inc*</td>
<td>236</td>
</tr>
<tr>
<td>Synergy Microsystems</td>
<td>21</td>
</tr>
<tr>
<td>Taiyo Yuden (USA) Inc</td>
<td>245</td>
</tr>
<tr>
<td>Tatsum Labs</td>
<td>268</td>
</tr>
<tr>
<td>T-Cubed Systems Inc</td>
<td>266</td>
</tr>
<tr>
<td>TOKD Corp of America</td>
<td>92</td>
</tr>
<tr>
<td>TEAC Corp*</td>
<td>277</td>
</tr>
<tr>
<td>Team Visionics</td>
<td>192</td>
</tr>
<tr>
<td>Tektronix Inc</td>
<td>34-37, 44, 98</td>
</tr>
<tr>
<td>Telecom Analysis Systems</td>
<td>42</td>
</tr>
<tr>
<td>Teledyne Solid State</td>
<td>242</td>
</tr>
<tr>
<td>Teradyne Inc</td>
<td>30-31</td>
</tr>
<tr>
<td>Texas Instruments Inc</td>
<td>103-106</td>
</tr>
<tr>
<td>Todd Products Corp</td>
<td>43, 271</td>
</tr>
<tr>
<td>Tokin Corp</td>
<td>243</td>
</tr>
<tr>
<td>Toko America Inc</td>
<td>68</td>
</tr>
<tr>
<td>Transera</td>
<td>137</td>
</tr>
<tr>
<td>Tribal Microsystems</td>
<td>270</td>
</tr>
<tr>
<td>TRW LSI Products Inc</td>
<td>14-15</td>
</tr>
<tr>
<td>Two Technologies</td>
<td>266</td>
</tr>
<tr>
<td>Universal Cross Assemblers</td>
<td>269</td>
</tr>
<tr>
<td>Universal Data Systems</td>
<td>C3</td>
</tr>
<tr>
<td>US Software</td>
<td>268</td>
</tr>
<tr>
<td>Vacuumshmelze**</td>
<td>220</td>
</tr>
<tr>
<td>Valley Enterprises</td>
<td>126</td>
</tr>
<tr>
<td>Wickmann Werke</td>
<td>228</td>
</tr>
<tr>
<td>WinSystems Inc</td>
<td>96</td>
</tr>
<tr>
<td>Zilog Inc</td>
<td>174-175, 176-177, 178-179</td>
</tr>
<tr>
<td>Z-World</td>
<td>266</td>
</tr>
</tbody>
</table>

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